LM25017 48-V, 650-mA Constant On-Time Synchronous Buck Regulator

1 Features

- Wide 7.5-V to 48-V Input Range
- Integrated 650-mA High-Side and Low-Side Switches
- No Schottky Diode Required
- Constant On-Time Control
- No Loop Compensation Required
- Ultra-Fast Transient Response
- Nearly Constant Operating Frequency
- Intelligent Peak Current Limit
- Adjustable Output Voltage from 1.225 V
- Precision 2% Feedback Reference
- Frequency Adjustable to 1 MHz
- Adjustable Undervoltage Lockout (UVLO)
- Remote Shutdown
- Thermal Shutdown
- Packages:
  - WSON-8
  - HSOP-8

2 Applications

- Industrial Equipment
- Smart Power Meters
- Telecommunication Systems
- Isolated Bias Supply

3 Description

The LM25017 device is a 48-V, 650-mA synchronous step-down regulator with integrated high-side and low-side MOSFETs. The constant on-time (COT) control scheme employed in the LM25017 device requires no loop compensation, provides excellent transient response, and enables very high step-down ratios. The on-time varies inversely with the input voltage resulting in nearly constant frequency over the input voltage range. A high voltage startup regulator provides bias power for internal operation of the IC and for integrated gate drivers.

A peak current limit circuit protects against overload conditions. The undervoltage lockout (UVLO) circuit allows the input undervoltage threshold and hysteresis to be independently programmed. Other protection features include thermal shutdown and bias supply undervoltage lockout (V_{CC} UVLO).

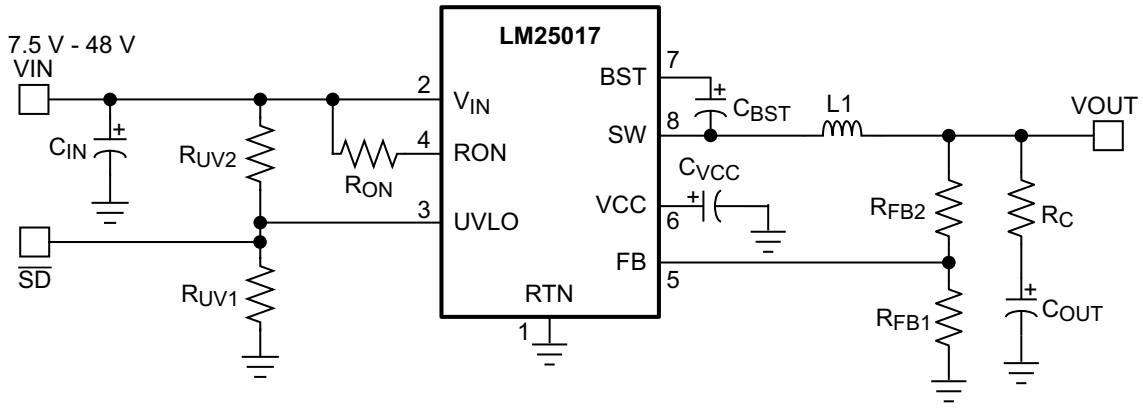
The LM25017 device is available in WSON-8 and HSOP-8 plastic packages.

Device Information[1]

PART NUMBER	PACKAGE	BODY SIZE (NOM)
LM25017	HSOP (8)	4.89 mm x 3.90 mm
	WSON (8)	4.00 mm x 4.00 mm

(1) For all available packages, see the orderable addendum at the end of the data sheet.

Typical Application Schematic



An IMPORTANT NOTICE at the end of this data sheet addresses availability, warranty, changes, use in safety-critical applications, intellectual property matters and other important disclaimers. PRODUCTION DATA.

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4 Revision History

Changes from Revision C (December 2013) to Revision D — **Page**

- Added *Pin Configuration and Functions* section, *ESD Rating* table, *Feature Description* section, *Device Functional Modes*, *Application and Implementation* section, *Power Supply Recommendations* section, *Layout* section, *Device and Documentation Support* section, and *Mechanical, Packaging, and Orderable Information* section ... 1
- Changed VIN voltage in *Typical Application* ... 1
- Changed max operating junction temperature in *Recommended Operating Conditions* table. ... 4
- Updated *Thermal Information* table with package designators. ... 4
- Changed *Soft-Start Circuit* graphic. ... 13
- Changed *Frequency Selection* section, *Inductor Selection* section, *Output Capacitor* section, *Input Capacitor* section, and *UVLO Resistors* section ... 15

Changes from Revision B (December 2013) to Revision C — **Page**

- Added Thermal Parameters ... 4

Changes from Revision A (September 2013) to Revision B — **Page**

- Changed formatting throughout document to TI standard ... 1
- Changed minimum input voltage from 9 V to 7.5 V in *Typical Application* diagram ... 1
- Changed minimum input voltage from 9 V to 7.5 V in *Pin Descriptions* ... 3
- Added Maximum Junction Temperature ... 4
- Changed minimum input voltage from 9 V to 7.5 V in *Recommended Operating Conditions* ... 4

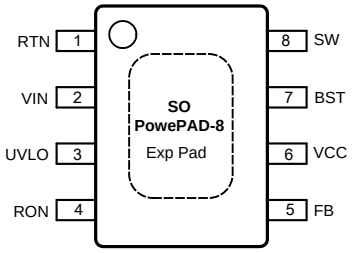
Changes from Original (December 2012) to Revision A — **Page**

- Added SW to RTN (100 ns transient) to *Absolute Maximum Ratings* ... 4

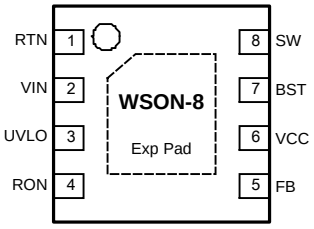
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5 Pin Configuration and Functions

8-Pin HSOP
DDA Package
Top View



8-Pin WSON
NGU Package
Top View



Pin Functions

PIN		I/O	DESCRIPTION	APPLICATION INFORMATION
NO.	NAME			
1	RTN	—	Ground	Ground connection of the integrated circuit.
2	VIN	I	Input Voltage	Operating input range is 7.5 V to 48 V.
3	UVLO	I	Input Pin of Undervoltage Comparator	Resistor divider from V_{IN} to UVLO to GND programs the undervoltage detection threshold. An internal current source is enabled when UVLO is above 1.225 V to provide hysteresis. When UVLO pin is pulled below 0.66 V externally, the regulator is in shutdown mode.
4	RON	I	On-Time Control	A resistor between this pin and V_{IN} sets the buck switch on-time as a function of V_{IN}. Minimum recommended on-time is 100 ns at max input voltage.
5	FB	I	Feedback	This pin is connected to the inverting input of the internal regulation comparator. The regulation level is 1.225 V.
6	VCC	O	Output from the Internal High Voltage Series Pass Regulator. Regulated at 7.6 V	The internal V_{CC} regulator provides bias supply for the gate drivers and other internal circuitry. A 1.0-µF decoupling capacitor is recommended.
7	BST	I	Bootstrap Capacitor	An external capacitor is required between the BST and SW pins (0.01-µF ceramic). The BST pin capacitor is charged by the V_{CC} regulator through an internal diode when the SW pin is low.
8	SW	O	Switching Node	Power switching node. Connect to the output inductor and bootstrap capacitor.
—	EP	—	Exposed Pad	Exposed pad must be connected to the RTN pin. Solder to the system ground plane on application board for reduced thermal resistance.

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6 Specifications

6.1 Absolute Maximum Ratings[1][2]

	MIN	MAX	UNIT
V_{IN}, UVLO to RTN	–0.3	53	V
SW to RTN	–1.5	V_{IN} +0.3	V
SW to RTN (100 ns transient)	–5	V_{IN} +0.3	V
BST to V_{CC}		53	V
BST to SW		13	V
R_{ON} to RTN	–0.3	53	V
V_{CC} to RTN	–0.3	13	V
FB to RTN	–0.3	5	V
Lead Temperature[3]		200	°C
Maximum Junction Temperature[4]		150	°C
Storage temperature, T_{stg}	–55	150	°C

(1) Stresses beyond those listed under *Absolute Maximum Ratings* may cause permanent damage to the device. These are stress ratings only, which do not imply functional operation of the device at these or any other conditions beyond those indicated under *Recommended Operating Conditions*. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.
(2) The RTN pin is the GND reference electrically connected to the substrate.
(3) For detailed information on soldering plastic SO PowerPAD-8 package, refer to the Packaging Data Book available from Texas Instruments, Inc. Max solder time not to exceed 4 seconds.
(4) High junction temperatures degrade operating lifetimes. Operating lifetime is de-rated for junction temperatures greater than 125°C.

6.2 ESD Ratings

			VALUE	UNIT
$V_{(ESD)}$	Electrostatic discharge	Human-body model (HBM), per ANSI/ESDA/JEDEC JS-001[1]	±2000	V
		Charged-device model (CDM), per JEDEC specification JESD22-C101[2]	±750	

(1) JEDEC document JEP155 states that 500-V HBM allows safe manufacturing with a standard ESD control process.
(2) JEDEC document JEP157 states that 250-V CDM allows safe manufacturing with a standard ESD control process.

6.3 Recommended Operating Conditions

over operating free-air temperature range (unless otherwise noted)[1]

	MIN	MAX	UNIT
V_{IN} Voltage	7.5	48	V
Operating Junction Temperature[2]	–40	125	°C

(1) *Recommended Operating Conditions* are conditions under the device is intended to be functional. For specifications and test conditions, see *Electrical Characteristics* .
(2) High junction temperatures degrade operating lifetimes. Operating lifetime is de-rated for junction temperatures greater than 125°C.

6.4 Thermal Information

THERMAL METRICS[1]		LM25017		UNIT
		NGU	DDA	
		8 PINS		
$R_{\theta JA}$	Junction-to-ambient thermal resistance	41.3	41.1	°C/W
$R_{\theta JC(top)}$	Junction-to-case (top) thermal resistance	34.7	37.3	
$R_{\theta JB}$	Junction-to-board thermal resistance	19.1	30.6	
ψ_{JT}	Junction-to-top thermal characteristic parameter	0.3	6.7	
ψ_{JB}	Junction-to-board thermal characteristic parameter	19.2	24.4	
$R_{\theta JC(bot)}$	Junction-to-case (bottom) thermal resistance	3.2	2.4	

(1) For more information about traditional and new thermal metrics, see the *IC Package Thermal Metrics* application report (SPRA953).

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6.5 Electrical Characteristics

Typical values correspond to T_J = 25°C. Minimum and maximum limits apply over –40°C to 125°C junction temperature range, unless otherwise stated. V_{IN} = 48 V unless otherwise stated. V_{IN} = 48 V unless otherwise stated. See (1).

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
V_{CC} SUPPLY						
V_{CC} Reg	V_{CC} Regulator Output	V_{IN} = 48 V, I_{CC} = 20 mA	6.25	7.6	8.55	V
	V_{CC} Current Limit	V_{IN} = 48 V(2)	26			mA
	V_{CC} Undervoltage Lockout Voltage (V_{CC} increasing)		4.15	4.5	4.9	V
	V_{CC} Undervoltage Hysteresis			300		mV
	V_{CC} Drop Out Voltage	V_{IN} = 9 V, I_{CC} = 20 mA		2.3		V
	I_{IN} Operating Current	Non-Switching, FB = 3 V		1.75		mA
	I_{IN} Shutdown Current	UVLO = 0 V		50	225	µA
SWITCH CHARACTERISTICS						
	Buck Switch $R_{DS(ON)}$	I_{TEST} = 200 mA, BST-SW = 7 V		0.8	1.8	Ω
	Synchronous $R_{DS(ON)}$	I_{TEST} = 200 mA		0.45	1	Ω
	Gate Drive UVLO	V_{BST} – V_{SW} Rising	2.4	3	3.6	V
	Gate Drive UVLO Hysteresis			260		mV
CURRENT LIMIT						
	Current Limit Threshold		0.7	1.02	1.3	A
	Current Limit Response Time	Time to Switch Off		150		ns
	OFF-Time Generator (Test 1)	FB = 0.1 V, V_{IN} = 48 V		12		µs
	OFF-Time Generator (Test 2)	FB = 1.0 V, V_{IN} = 48 V		2.5		µs
REGULATION AND OVERVOLTAGE COMPARATORS						
	FB Regulation Level	Internal Reference Trip Point for Switch ON	1.2	1.225	1.25	V
	FB Overvoltage Threshold	Trip Point for Switch OFF		1.62		V
	FB Bias Current			60		nA
UNDERVOLTAGE SENSING FUNCTION						
	UV Threshold	UV Rising	1.19	1.225	1.26	V
	UV Hysteresis Input Current	UV = 2.5 V	–10	–20	–29	µA
	Remote Shutdown Threshold	Voltage at UVLO Falling	0.32	0.66		V
	Remote Shutdown Hysteresis			110		mV
THERMAL SHUTDOWN						
T_{sd}	Thermal Shutdown Temperature			165		°C
	Thermal Shutdown Hysteresis			20		°C

(1) All hot and cold limits are specified by correlating the electrical characteristics to process and temperature variations and applying statistical process control.
(2) V_{CC} provides self bias for the internal gate drive and control circuits. Device thermal limitations limit external loading.

6.6 Switching Characteristics

Typical values correspond to T_J = 25°C. Minimum and maximum limits apply over –40°C to 125°C junction temperature range unless otherwise stated. V_{IN} = 48 V unless otherwise stated.

PARAMETER	TEST CONDITIONS	MIN	TYP	MAX	UNIT
ON-TIME GENERATOR					
T_{ON} Test 1	V_{IN} = 32 V, R_{ON} = 100 k	270	350	460	ns
T_{ON} Test 2	V_{IN} = 48 V, R_{ON} = 100 k	188	250	336	ns
T_{ON} Test 4	V_{IN} = 10 V, R_{ON} = 250 k	1880	3200	4425	ns
MINIMUM OFF-TIME					
Minimum Off-Timer	FB = 0 V		144		ns

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6.7 Typical Characteristics

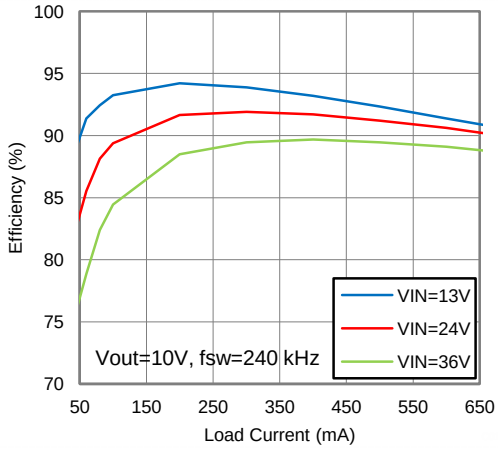


Figure 1. Efficiency at 200 kHz, 10 V

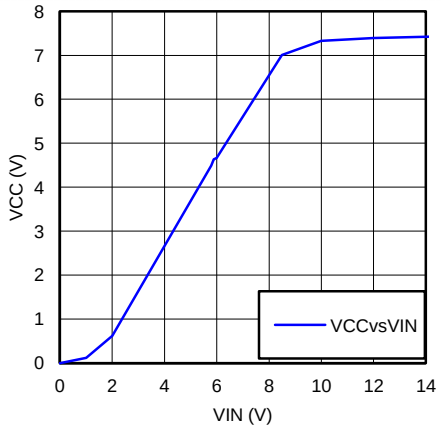


Figure 2. V_{CC} vs V_{IN}

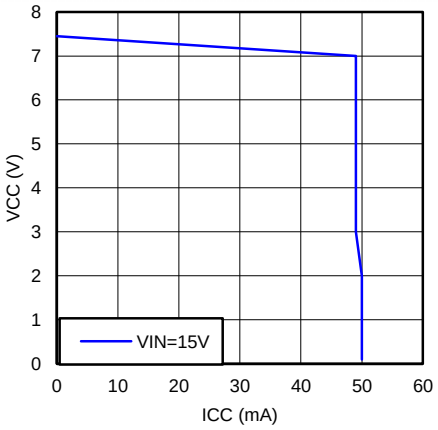


Figure 3. V_{CC} vs I_{CC}

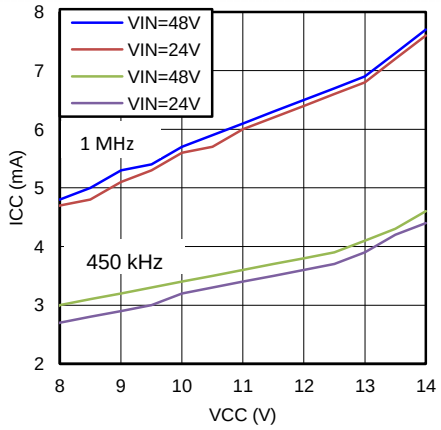


Figure 4. I_{CC} vs External V_{CC}

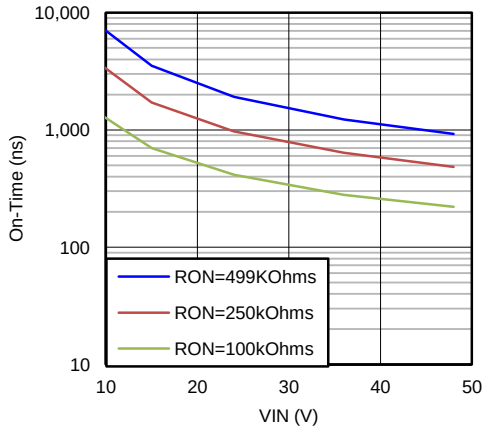


Figure 5. T_{ON} vs V_{IN} and R_{ON}

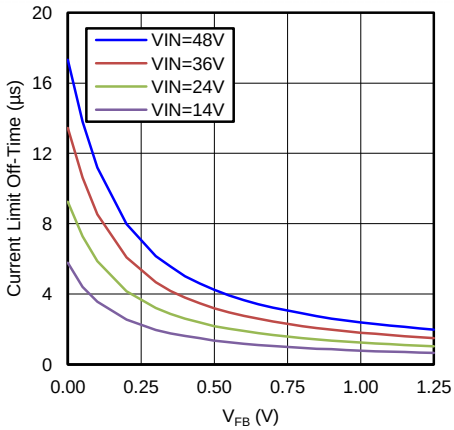


Figure 6. T_{OFF} (I_{LIM}) vs V_{FB} and V_{IN}

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Typical Characteristics (continued)

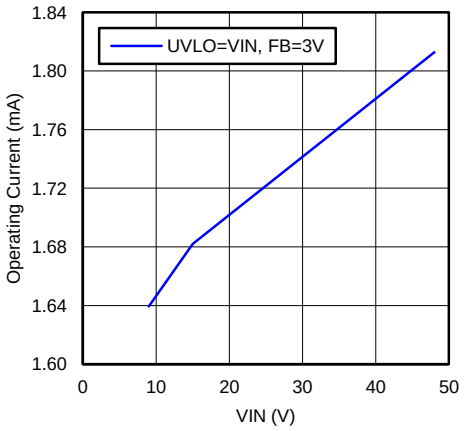


Figure 7. I_{IN} vs V_{IN} (Operating, Non Switching)

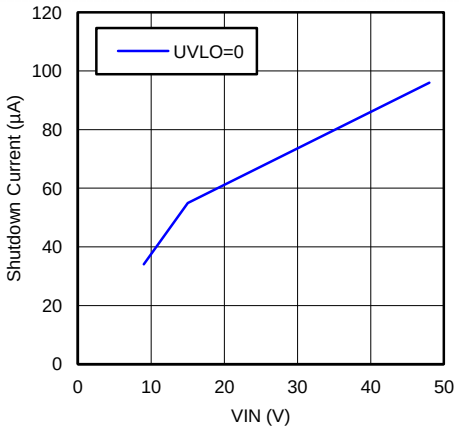


Figure 8. I_{IN} vs V_{IN} (Shutdown)

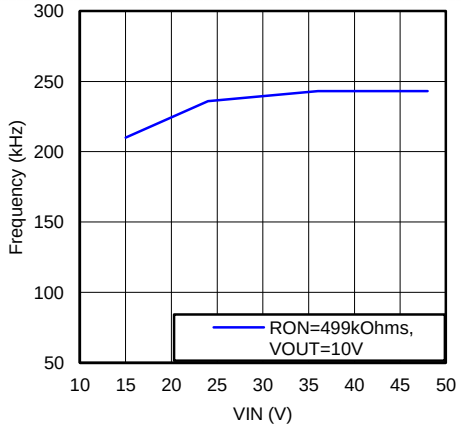


Figure 9. Switching Frequency vs V_{IN}

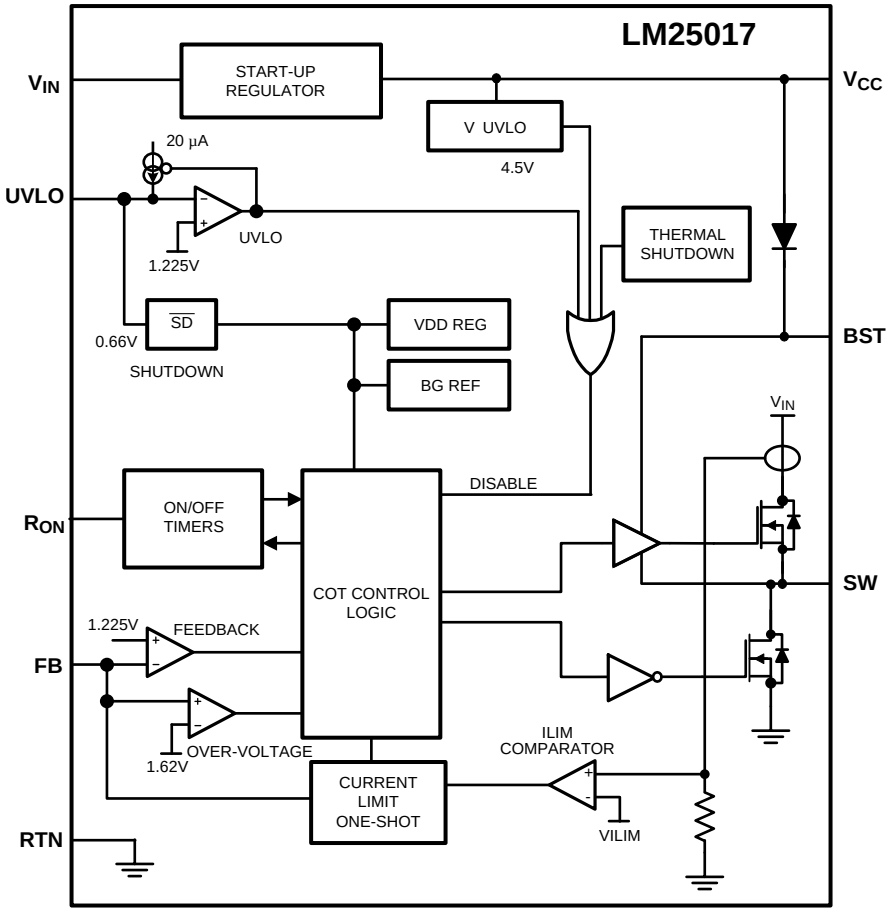
7 Detailed Description

7.1 Overview

The LM25017 step-down switching regulator features all the functions needed to implement a low cost, efficient, buck converter capable of supplying up to 650 mA to the load. This high voltage regulator contains 48-V, N-channel buck and synchronous switches, is easy to implement, and is provided in thermally enhanced SO PowerPAD-8 and WSON-8 packages. The regulator operation is based on a constant on-time control scheme using an on-time inversely proportional to V_{IN}. This control scheme does not require loop compensation. The current limit is implemented with a forced off-time inversely proportional to V_{OUT}. This scheme ensures short circuit protection while providing minimum fold-back.

The LM25017 device can be applied in numerous applications to efficiently regulate down higher voltages. This regulator is well suited for 12-V and 24-V rails. Protection features include: thermal shutdown, Undervoltage Lockout (UVLO), minimum forced off-time, and an intelligent current limit.

7.2 Functional Block Diagram



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7.3 Feature Description

7.3.1 Control Overview

The LM25017 buck regulator employs a control principle based on a comparator and a one-shot on-timer, with the output voltage feedback (FB) compared to an internal reference (1.225 V). If the FB voltage is below the reference the internal buck switch is turned on for the one-shot timer period, which is a function of the input voltage and the programming resistor (R_{ON}). Following the on-time the switch remains off until the FB voltage falls below the reference, but never before the minimum off-time forced by the minimum off-time one-shot timer. When the FB pin voltage falls below the reference and the minimum off-time one-shot period expires, the buck switch is turned on for another on-time one-shot period. This will continue until regulation is achieved and the FB voltage is approximately equal to 1.225 V (typ).

In a synchronous buck converter, the low side (sync) FET is 'on' when the high side (buck) FET is 'off'. The inductor current ramps up when the high side switch is 'on' and ramps down when the high side switch is 'off'. There is no diode emulation feature in this IC, and therefore, the inductor current may ramp in the negative direction at light load. This causes the converter to operate in continuous conduction mode (CCM) regardless of the output loading. The operating frequency remains relatively constant with load and line variations. The operating frequency can be calculated as shown in Equation 1.

$$f_{SW} = \frac{V_{OUT}}{K \times R_{ON}}$$

where

- $K = 9 \times 10^{-11}$ (1)

The output voltage (V_{OUT}) is set by two external resistors (R_{FB1}, R_{FB2}). The regulated output voltage is calculated as shown in Equation 2.

$$V_{OUT} = 1.225V \times \frac{R_{FB2} + R_{FB1}}{R_{FB1}} \quad (2)$$

This regulator regulates the output voltage based on ripple voltage at the feedback input, requiring a minimum amount of ESR for the output capacitor (C_{OUT}). A minimum of 25-mV ripple voltage at the feedback pin (FB) is required for the LM25017 device. In cases where the capacitor ESR is too small, additional series resistance may be required (R_C in Figure 10).

For applications where lower output voltage ripple is required, the output can be taken directly from a low ESR output capacitor, as shown in Figure 10. However, R_C slightly degrades the load regulation.

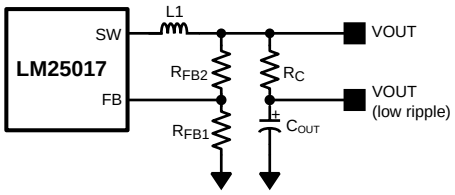


Figure 10. Low Ripple Output Configuration

7.3.2 V_{CC} Regulator

The LM25017 device contains an internal high-voltage linear regulator with a nominal output of 7.6 V. The input pin (V_{IN}) can be connected directly to the line voltages up to 48 V. The V_{CC} regulator is internally current limited to 30 mA. The regulator sources current into the external capacitor at V_{CC}. This regulator supplies current to internal circuit blocks including the synchronous MOSFET driver and the logic circuits. When the voltage on the V_{CC} pin reaches the undervoltage lockout (V_{CC} UVLO) threshold of 4.5 V, the IC is enabled.

An internal diode connected from VCC to the BST pin replenishes the charge in the gate drive bootstrap capacitor when SW pin is low.

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Feature Description (continued)

At high-input voltages, the power dissipated in the high voltage regulator is significant and can limit the overall achievable output power. As an example, with the input at 48 V and switching at high frequency, the V_{CC} regulator may supply up to 7 mA of current resulting in 48 V × 7 mA = 336 mW of power dissipation. If the V_{CC} voltage is driven externally by an alternate voltage source between 8.55 V and 14 V, the internal regulator is disabled. This reduces the power dissipation in the IC.

7.3.3 Regulation Comparator

The feedback voltage at FB is compared to an internal 1.225-V reference. In normal operation, when the output voltage is in regulation, an on-time period is initiated when the voltage at FB falls below 1.225 V. The high side switch will stay on for the on-time, causing the FB voltage to rise above 1.225 V. After the on-time period, the high side switch will stay off until the FB voltage again falls below 1.225 V. During start up, the FB voltage will be below 1.225 V at the end of each on-time, causing the high side switch to turn on immediately after the minimum forced off-time of 144 ns. The high side switch can be turned off before the on-time is over if the peak current in the inductor reaches the current limit threshold.

7.3.4 Overvoltage Comparator

The feedback voltage at FB is compared to an internal 1.62-V reference. If the voltage at FB rises above 1.62 V the on-time pulse is immediately terminated. This condition can occur if the input voltage and/or the output load changes suddenly. The high side switch will not turn on again until the voltage at FB falls below 1.225 V.

7.3.5 On-Time Generator

The on-time for the LM25017 device is determined by the R_{ON} resistor and is inversely proportional to the input voltage (V_{IN}), resulting in a nearly constant frequency as V_{IN} is varied over the operating range. The on-time for the LM25017 can be calculated using Equation 3.

$$T_{ON} = \frac{10^{-10} \times R_{ON}}{V_{IN}} \tag{3}$$

See Figure 5. R_{ON} should be selected for a minimum on-time (at maximum V_{IN}) greater than 100 ns for proper operation. This requirement limits the maximum switching frequency for high V_{IN}.

7.3.6 Current Limit

The LM25017 device contains an intelligent current limit off-timer. If the current in the buck switch exceeds 1.02 A, the present cycle is immediately terminated, and a non-resetable off-timer is initiated. The length of the off-time is controlled by the FB voltage and the input voltage V_{IN}. As an example, when FB = 0 V and V_{IN} = 48 V, the maximum off-time is set to 16 µs. This condition occurs when the output is shorted and during the initial part of start-up. This V_{IN} dependent off-time ensures safe short circuit operation up to the maximum input voltage of 48 V.

In cases of overload where the FB voltage is above zero volts (not a short circuit) the current limit off-time is reduced. Reducing the off-time during less severe overloads reduces the amount of fold-back, recovery time, and start-up time. The off-time is calculated as shown in Equation 4.

$$T_{OFF(ILIM)} = \frac{0.07 \times V_{IN}}{V_{FB} + 0.2V} \ \mu s \tag{4}$$

The current limit protection feature is peak limited. The maximum average output current will be less than the peak.

7.3.7 N-Channel Buck Switch and Driver

The LM25017 device integrates an N-Channel Buck switch and associated floating high-voltage gate driver. The gate driver circuit works in conjunction with an external bootstrap capacitor and an internal high-voltage diode. A 0.01-uF ceramic capacitor connected between the BST pin and the SW pin provides the voltage to the driver during the on-time. During each off-time, the SW pin is at approximately 0 V, and the bootstrap capacitor charges from V_{CC} through the internal diode. The minimum off-timer, set to 144 ns, ensures a minimum time each cycle to recharge the bootstrap capacitor.

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Feature Description (continued)

7.3.8 Synchronous Rectifier

The LM25017 device provides an internal synchronous N-Channel MOSFET rectifier. This MOSFET provides a path for the inductor current to flow when the high-side MOSFET is turned off.

The synchronous rectifier has no diode emulation mode, and is designed to keep the regulator in continuous conduction mode even with light loads which would otherwise result in discontinuous operation.

7.3.9 Undervoltage Detector

The LM25017 device contains a dual-level undervoltage lockout (UVLO) circuit. A summary of threshold voltages and operational states is provided in *Device Functional Modes*. When the UVLO pin voltage is below 0.66 V, the regulator is in a low current shutdown mode. When the UVLO pin voltage is greater than 0.66 V but less than 1.225 V, the regulator is in standby mode. In standby mode the V_{CC} bias regulator is active while the regulator output is disabled. When the V_{CC} pin exceeds the V_{CC} undervoltage threshold and the UVLO pin voltage is greater than 1.225 V, normal operation begins. An external set-point voltage divider from V_{IN} to GND can be used to set the minimum operating voltage of the regulator.

UVLO hysteresis is accomplished with an internal 20-µA current source that is switched on or off into the impedance of the set-point divider. When the UVLO threshold is exceeded, the current source is activated to quickly raise the voltage at the UVLO pin. The hysteresis is equal to the value of this current times the resistance R_{UV2}.

If the UVLO pin is connected directly to the V_{IN} pin, the regulator will begin operation once the V_{CC} undervoltage is satisfied.

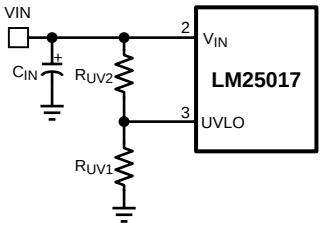


Figure 11. UVLO Resistor Setting

7.3.10 Thermal Protection

The LM25017 device should be operated so the junction temperature does not exceed 150°C during normal operation. An internal Thermal Shutdown circuit is provided to protect the LM25017 in the event of a higher than normal junction temperature. When activated, typically at 165°C, the regulator is forced into a low power reset state, disabling the buck switch and the V_{CC} regulator. This feature prevents catastrophic failures from accidental device overheating. When the junction temperature falls below 145°C (typical hysteresis = 20°C), the V_{CC} regulator is enabled, and normal operation is resumed.

7.3.11 Ripple Configuration

LM25017 uses Constant-On-Time (COT) control in which the on-time is terminated by an on-timer and the off-time is terminated by the feedback voltage (V_{FB}) falling below the reference voltage (V_{REF}). Therefore, for stable operation, the feedback voltage must decrease monotonically, in phase with the inductor current during the off-time. Furthermore, this change in feedback voltage (V_{FB}) during off-time must be larger than any noise component present at the feedback node.

Table 1 shows three different methods for generating appropriate voltage ripple at the feedback node. Type 1 and Type 2 ripple circuits couple the ripple at the output of the converter to the feedback node (FB). The output voltage ripple has two components:

1. Capacitive ripple caused by the inductor current ripple charging/discharging the output capacitor.
2. Resistive ripple caused by the inductor current ripple flowing through the ESR of the output capacitor.

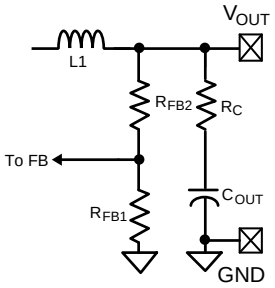
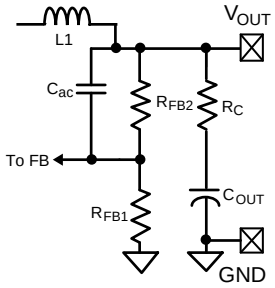
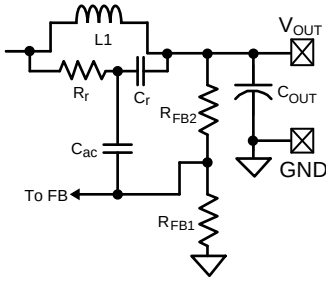
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Feature Description (continued)

The capacitive ripple is not in phase with the inductor current. As a result, the capacitive ripple does not decrease monotonically during the off-time. The resistive ripple is in phase with the inductor current and decreases monotonically during the off-time. The resistive ripple must exceed the capacitive ripple at the output node (V_{OUT}) for stable operation. If this condition is not satisfied unstable switching behavior is observed in COT converters, with multiple on-time bursts in close succession followed by a long off-time.

Type 3 ripple method uses R_r and C_r and the switch node (SW) voltage to generate a triangular ramp. This triangular ramp is ac coupled using C_{ac} to the feedback node (FB). Since this circuit does not use the output voltage ripple, it is ideally suited for applications where low output voltage ripple is required. See *AN-1481 Controlling Output Ripple and Achieving ESR Independence in Constant On-Time (COT) Regulator Designs* (SNVA166) for more details for each ripple generation method.

Table 1. Ripple Configuration

TYPE 1 LOWEST COST CONFIGURATION	TYPE 2 REDUCED RIPPLE CONFIGURATION	TYPE 3 MINIMUM RIPPLE CONFIGURATION
		
$R_C \geq \frac{25\ mV}{\Delta I_{L(MIN)}} \times \frac{V_{OUT}}{V_{REF}}$	$C \geq \frac{5}{f_{sw}(R_{FB2} \| R_{FB1})}$ $R_C \geq \frac{25\ mV}{\Delta I_{L(MIN)}}$	$C_r = 3300\ pF$ $C_{ac} = 100\ nF$ $R_r C_r \leq \frac{(V_{IN(MIN)} - V_{OUT}) \times T_{ON}}{25\ mV}$

7.3.12 Soft-Start

A soft-start feature can be implemented with the LM25017 device using an external circuit. As shown in Figure 12, the soft-start circuit consists of one capacitor, C_1, two resistors, R_1 and R_2, and a diode, D. During the initial start-up, the VCC voltage is established prior to the V_{OUT} voltage. Capacitor C_1 is discharged and diode D is thereby forward biased to pull up the FB pin voltage. The FB voltage exceeds the reference voltage (1.225 V) and switching is therefore disabled. As capacitor C_1 charges, the voltage at node B gradually decreases and switching commences. V_{OUT} will gradually rise to maintain the FB voltage at the reference voltage. Once the voltage at node B is less than a diode drop above the FB voltage, the soft-start sequence is finished and D is reverse biased.

During the initial part of the start-up, the FB voltage can be approximated as shown in Equation 5.

$$V_{FB} = (VCC - V_D) \times \frac{R_{FB1} \times R_{FB2}}{R_2 \times (R_{FB1} + R_{FB2}) + R_{FB1} \times R_{FB2}} \quad (5)$$

C1 is charged after the first start up. Diode D1 is optional and can be added to discharge C1 when the input voltage experiences a momentary drop to initialize the soft-start sequence.

To achieve the desired soft start, the following design guidance is recommended:

- R_2 is selected so that V_{FB} is higher than 1.225 V for a V_{CC} of 4.5 V, but is lower than 5 V when V_{CC} is 8.55 V. If an external V_{CC} is used, V_{FB} should not exceed 5 V at maximum V_{CC}.
- C_1 is selected to achieve the desired start-up time which can be determined from Equation 6.

$$t_S = C_1 \times \left(R_2 + \frac{R_{FB1} \times R_{FB2}}{R_{FB1} + R_{FB2}}\right) \quad (6)$$

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- R_1 is used to maintain the node B voltage at zero after the soft start is finished. A value larger than the feedback resistor divider is preferred. Note that the effect of resistor R1 is ignored in Equation 5.

Based on the schematic shown in Figure 12, selecting C_1 = 1 uF, R_2 = 1 kΩ, R_1 = 30 kΩ results in a soft-start time of about 2 ms.

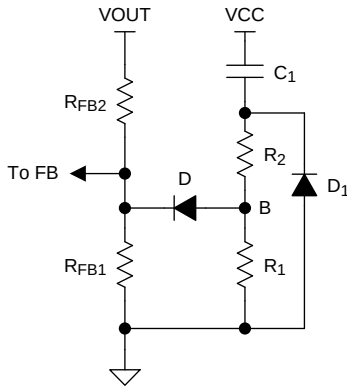


Figure 12. Soft-Start Circuit

7.4 Device Functional Modes

The UVLO pin controls the operating mode of the LM25017 device (see Table 2 for the detailed functional states).

Table 2. UVLO Mode

UVLO	V_{CC}	MODE	DESCRIPTION
< 0.66 V	Disabled	Shutdown	V_{CC} regulator disabled. Switching disabled.
0.66 V – 1.225 V	Enabled	Standby	V_{CC} regulator enabled Switching disabled.
> 1.225 V	V_{CC} < 4.5 V	Standby	V_{CC} regulator enabled. Switching disabled.
	V_{CC} > 4.5 V	Operating	V_{CC} enabled. Switching enabled.

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8 Application and Implementation

NOTE

Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes. Customers should validate and test their design implementation to confirm system functionality.

8.1 Application Information

The LM25017 device is step-down dc-to-dc converter. The device is typically used to convert a higher dc voltage to a lower dc voltage with a maximum available output current of 650 mA. Use the following design procedure to select component values for the LM25017 device. Alternately, use the WEBENCH® software to generate a complete design. The WEBENCH™ software uses an iterative design procedure and accesses a comprehensive database of components when generating a design. This section presents a simplified discussion of the design process.

8.2 Typical Application

8.2.1 Application Circuit: 12.5-V to 48-V Input and 10-V, 650-mA Output Buck Converter

The application schematic of a buck supply is shown in Figure 13. For output voltage (V_{OUT}) above the maximum regulation threshold of V_{CC} (8.55 V, see *Electrical Characteristics*), the V_{CC} pin can be connected to V_{OUT} through a diode (D2), for higher efficiency and lower power dissipation in the IC.

The design example shown in Figure 13 uses equations from the *Feature Description* section with component names provided in the *Typical Application Schematic*. Corresponding component designators from Figure 13 are also provided for each selected value.

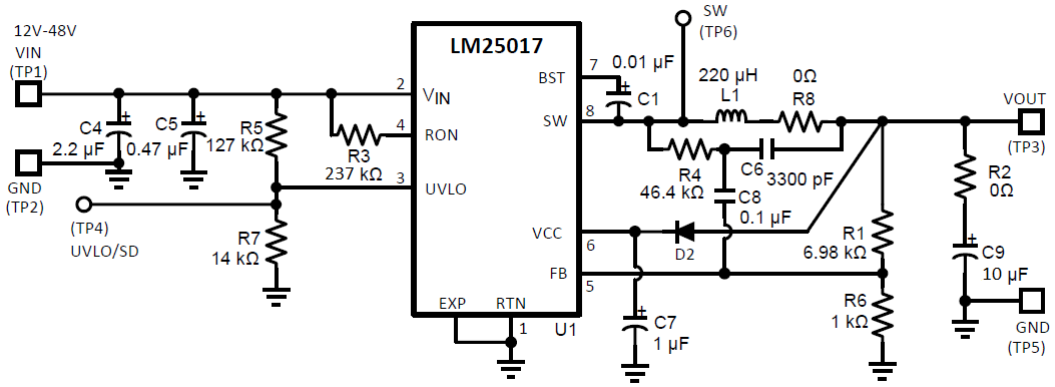


Figure 13. Final Schematic for 12.5-V to 48-V Input, and 10-V, 650-mA Output Buck Converter

8.2.1.1 Design Requirements

Selection of external components is illustrated through a design example. The design example specifications are shown in Table 3.

Table 3. Buck Converter Design Specifications

DESIGN PARAMETERS	VALUE
Input Range	12.5 V to 48 V
Output Voltage	10 V
Maximum Output Current	650 mA
Nominal Switching Frequency	≈ 480 kHz

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8.2.1.2 Detailed Design Procedure

8.2.1.2.1 RFB1, RFB2

$V_{OUT} = V_{FB}$ x (R_{FB2} / R_{FB1} + 1), and because V_{FB} = 1.225 V, the ratio of R_{FB2} to R_{FB1} calculates as 7:1. Standard values are chosen with R_{FB2} = R1 = 6.98 kΩ and R_{FB1} = R6 = 1.00 kΩ are chosen. Other values could be used as long as the 7:1 ratio is maintained.

8.2.1.2.2 Frequency Selection

At the minimum input voltage, the maximum switching frequency of LM25017 is restricted by the forced minimum off-time ($T_{OFF(MIN)}$) as shown in Equation 7.

$$f_{SW(MAX)} = \frac{1 - D_{MAX}}{T_{OFF(MIN)}} = \frac{1 - 10/12.5}{200\ ns} = 1\ MHz \quad (7)$$

Similarly, at maximum input voltage, the maximum switching frequency of LM25017 is restricted by the minimum T_{ON} as shown in Equation 8.

$$f_{SW(MAX)} = \frac{D_{MIN}}{T_{ON(MIN)}} = \frac{10/48}{100\ ns} = 2.1\ MHz \quad (8)$$

Resistor R_{ON} sets the nominal switching frequency based on Equation 9.

$$f_{SW} = \frac{V_{OUT}}{K \times R_{ON}}$$

where

- $K = 9 \times 10^{-11}$ (9)

Operation at high switching frequency results in lower efficiency while providing the smallest solution. For this example, 480 kHz was selected, resulting in R_{ON} = 231.5 kΩ. Selecting a standard value for R_{ON} = R3 = 237 kΩ.

8.2.1.2.3 Inductor Selection

The minimum inductance is selected to limit the output ripple to 15 to 40 percent of the maximum load current. In addition, the peak inductor current at maximum load should be smaller than the minimum current limit as given in *Electrical Characteristics*. The inductor current ripple is shown in Equation 10.

$$\Delta I_L = \frac{V_{IN} - V_{OUT}}{L1 \times f_{SW}} \times \frac{V_{OUT}}{V_{IN}} \quad (10)$$

The maximum ripple is observed at maximum input voltage. To achieve the required output current of 650 mA without exceeding the peak current limit threshold, low ripple current is required. Substituting V_{IN} = 48 V and Δ_{IL} = 15 percent x $I_{OUT\ (max)}$ results in L1 = 169 µH. The higher value of 220 µH is chosen. The peak-to-peak minimum and maximum inductor current ripples of 19 mA and 75 mA at the minimum and maximum input voltages respectively. The peak inductor and switch current is shown in Equation 11.

$$I_{LI}(peak) = I_{OUT} + \frac{\Delta I_L(max)}{2} = 688\,mA \quad (11)$$

688 mA is smaller than the minimum current limit threshold, which is 700 mA. The selected inductor should be able to operate at the maximum current limit of 1.3 A, during startup and overload conditions without saturating.

8.2.1.2.4 Output Capacitor

The output capacitor is selected to minimize the capacitive ripple across it. The maximum ripple is observed at maximum input voltage and is shown in Equation 12.

$$C_{OUT} = \frac{\Delta I_L}{8 \times f_{sw} \times \Delta V_{ripple}}$$

where

- ΔV_{ripple} is the voltage ripple across the capacitor. (12)

Substituting ΔV_{ripple} = 5 mV gives C_{OUT} = 3.9 µF. A 10-µF standard value is selected for C_{OUT} = C9. An X5R or X7R type capacitor with a voltage rating 16 V or higher should be selected.

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8.2.1.2.5 Type III Ripple Circuit

Type III ripple circuit as described in *Ripple Configuration* is chosen for this example. For a constant on time converter to be stable, the injected in-phase ripple should be larger than the capacitive ripple on C_{OUT}.

Using type III ripple circuit equations, the target ripple should be greater than the capacitive ripple generated at the primary output.

C_r = C6 = 3300 pF

C_{ac} = C8 = 100 nF

$$R_r \leq \frac{(V_{IN(MIN)} - V_{OUT}) \times T_{ON(VINMIN)}}{(25mV \times C_r)} \quad (13)$$

For T_{ON}, refer to Equation 3.

Ripple resistor R_r is calculated to be 57.6 kΩ. This value provides the minimum ripple for stable operation. A smaller resistance should be selected to allow for variations in T_{ON}, C_{OUT}, and other components. R_r = R4 = 46.4 kΩ is selected for this example application.

8.2.1.2.6 V_{CC} and Bootstrap Capacitor

The V_{CC} capacitor provides charge to bootstrap capacitor as well as internal circuitry and low side gate driver. The bootstrap capacitor provides charge to high side gate driver. The recommended value for CV_{CC} = C7 is 1 µF. A good value for C_{BST} = C1 is 0.01 µF.

8.2.1.2.7 Input Capacitor

The input capacitor should be large enough to limit the input voltage ripple and can be calculated using Equation 14.

$$C_{IN} \geq \frac{I_{OUT(MAX)}}{8 \times f_{SW} \times \Delta V_{IN}} \quad (14)$$

Choosing a ΔV_{IN} = 0.5 V gives a minimum C_{IN} = 0.34 µF. A standard value of 2.2 µF is selected for C_{IN} = C4. The input capacitor should be rated for the maximum input voltage under all conditions. A 50-V, X7R dielectric should be selected for this design.

The input capacitor should be placed directly across V_{IN} and RTN (pin 2 and 1) of the IC. If it is not possible to place all of the input capacitor close to the IC, a 0.47-µF capacitor should be placed near the IC to provide a bypass path for the high-frequency component of the switching current. This helps limit the switching noise.

8.2.1.2.8 UVLO Resistors

The UVLO resistors R_{FB1} and R_{FB2} set the UVLO threshold and hysteresis according to the following relationship between Equation 15 and Equation 16.

$$V_{IN}(HYS) = I_{HYS} \times R_{UV2} \quad (15)$$

$$V_{IN}(UVLO,rising) = 1.225V \times \left(\frac{R_{UV2}}{R_{UV1}} + 1\right)$$

where

- I_{HYS} = 20 µA (16)

Setting UVLO hysteresis of 2.5 V and UVLO rising threshold of 12 V results in R_{UV1} = 14.53 kΩ and R_{UV2} = 125 kΩ. Selecting a standard value of R_{UV1} = R7 = 14 kΩ and R_{UV2} = R5 = 127 kΩ results in UVLO thresholds and hysteresis of 12.5 V to 2.5 V respectively.

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8.2.1.3 Application Curves

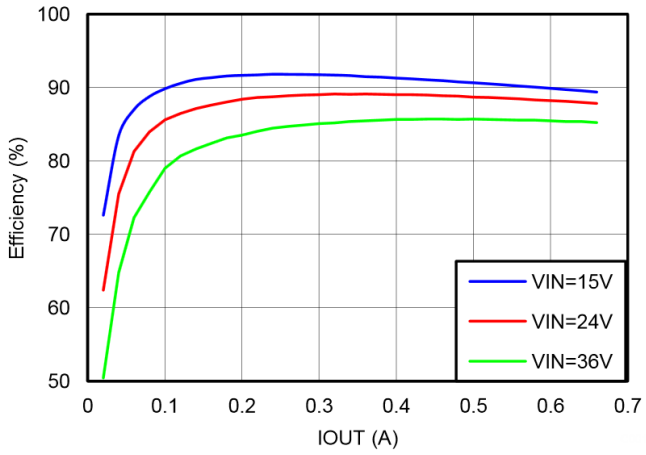


Figure 14. Efficiency vs Load Current

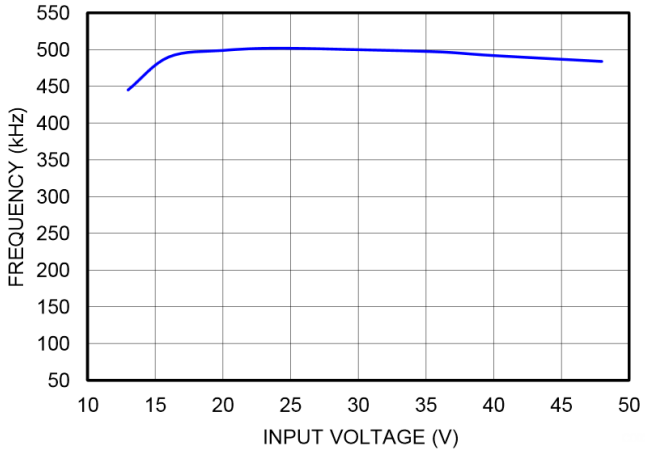


Figure 15. Frequency vs Input Voltage

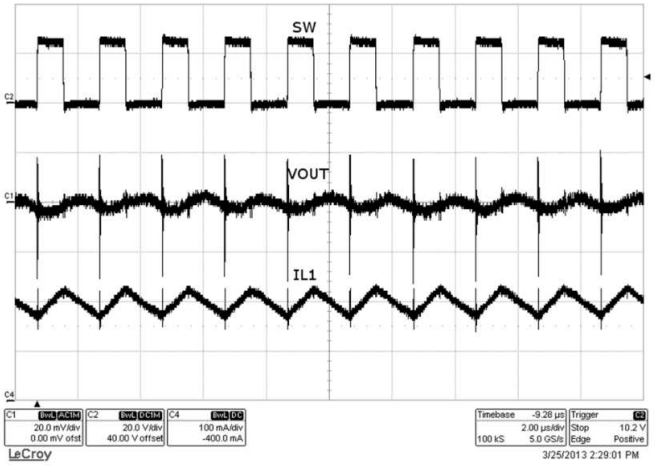


Figure 16. Typical Switching Waveform (V_{IN} = 24 V, I_{OUT} = 200 mA

8.2.2 Typical Isolated DC-DC Converter Using LM25017

An isolated supply using LM25017 is shown in Figure 17. Inductor (L) in a typical buck circuit is replaced with a coupled inductor (X1). A diode (D1) is used to rectify the voltage on a secondary output. The nominal voltage at the secondary output (V_{OUT2}) is given by Equation 17.

$$V_{OUT2} = V_{OUT1} \times \frac{N_S}{N_P} - V_F \quad (17)$$

where

- V_F is the forward voltage drop of D1
- N_P and N_S are the number of turns on the primary and secondary of coupled inductor X1.

For output voltage (V_{OUT1}) more than one diode drop above the maximum V_{CC} (8.55 V), the V_{CC} pin can be diode connected to V_{OUT1} for higher efficiency and low dissipation in the IC. See *AN-2292 Designing an Isolated Buck (Flyback) Converter* (SNVA674) for a complete isolated bias design using the Fly-Buck topology.

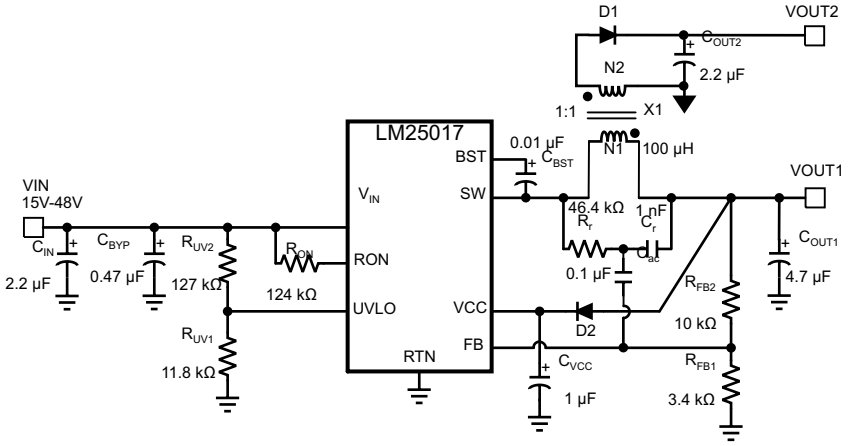


Figure 17. Typical Isolated Application Schematic

8.2.2.1 Design Requirements

Selection of external components is illustrated through a design example. The design example specifications are shown in Table 4.

Table 4. Buck Converter Design Specifications

DESIGN PARAMETERS	VALUE
Input Range	15 V to 48 V
Primary Output Voltage	5 V
Secondary (Isolated) Output Voltage	4.5 V
Maximum Output Current (Primary + Secondary)	600 mA
Maximum Power Output	3 W
Nominal Switching Frequency	500 kHz

8.2.2.2 Detailed Design Procedure

8.2.2.2.1 Transformer Turns Ratio

The transformer turns ratio is selected based on the ratio of the primary output voltage to the secondary (isolated) output voltage. In this design example, the two outputs are nearly equal and a 1:1 turns ratio transformer is selected. Therefore, N2 / N1 = 1.

If the secondary (isolated) output voltage is significantly higher or lower than the primary output voltage, a turns ratio less than or greater than 1 is recommended. The primary output voltage is normally selected based on the input voltage range such that the duty cycle of the converter does not exceed 50% at the minimum input voltage. This condition is satisfied if VOUT1 < V_{IN_MIN} / 2.

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8.2.2.2.2 Total IOUT

The total primary referred load current is calculated by multiplying the isolated output load(s) by the turns ratio of the transformer as shown in Equation 18.

$$I_{OUT(MAX)} = I_{OUT1} + I_{OUT2} \times \frac{N2}{N1} = 0.6\,A \tag{18}$$

8.2.2.2.3 RFB1, RFB2

The feedback resistors are selected to set the primary output voltage. The selected value for R_{FB1} is 3.4 kΩ. R_{FB2} can be calculated using the following equations to set V_{OUT1} to the specified value of 5 V. A standard resistor value of 10.0 kΩ is selected for R_{FB2}.

$$V_{OUT1} = 1.225V \text{ x } (1+ \frac{R_{FB2}}{R_{FB1}}) \tag{19}$$

$$\rightarrow R_{FB2} = (\frac{V_{OUT1}}{1.225} - 1) \times R_{FB1} = 10.4k\Omega \tag{20}$$

8.2.2.2.4 Frequency Selection

Equation 21 is used to calculate the value of R_{ON} required to achieve the desired switching frequency.

$$f_{SW} = \frac{V_{OUT1}}{K \text{ x } R_{ON}} \tag{21}$$

Where $K = 9 \times 10^{-11}$

For V_{OUT1} of 5 V and f_{SW} of 500 kHz, the calculated value of R_{ON} is 111 kΩ. A standard value of 124 kΩ is selected for this design to allow for second order effects at high switching frequency that are not included in Equation 21.

8.2.2.2.5 Transformer Selection

A coupled inductor or a flyback-type transformer is required for this topology. Energy is transferred from primary to secondary when the low-side synchronous switch of the buck converter is conducting.

The maximum inductor primary ripple current that can be tolerated without exceeding the buck switch peak current limit threshold (0.7 A minimum) is given by Equation 22.

$$\Delta I_{L1} = \left(0.7 - I_{OUT1} - I_{OUT2} \times \frac{N2}{N1}\right) \times 2 = 0.2\,A \tag{22}$$

Using the maximum peak-to-peak inductor ripple current ΔI_{L1} from Equation 22, the minimum inductor value is given by Equation 23.

$$L1 = \frac{V_{IN(MAX)} - V_{OUT}}{\Delta I_{L1} \times f_{SW}} \times \frac{V_{OUT}}{V_{IN(MAX)}} = 44.4\,\mu H \tag{23}$$

A higher value of 100 µH is selected to insure the high-side switch current does not exceed the minimum peak current limit threshold. With this inductance, the inductor current ripple is ΔI_{L1}= 90 mA at the maximum V_{IN}.

8.2.2.2.6 Primary Output Capacitor

In a conventional buck converter the output ripple voltage is calculated as shown in Equation 24.

$$\Delta V_{OUT} = \frac{\Delta I_{L1}}{8 \text{ x } f \text{ x } C_{OUT1}} \tag{24}$$

To limit the primary output ripple voltage ΔV_{OUT1} to approximately 25 mV, an output capcitor C_{OUT1} of 0.9 µF would be required for a conventional buck.

Figure 18 shows the primary winding current waveform (I_{L1}) of a Fly-Buck™ converter. The reflected secondary winding current adds to the primary winding current during the buck switch off-time. Because of this increased current, the output voltage ripple is not the same as in conventional buck converter. The output capacitor value calculated in Equation 24 should be used as the starting point. Optimization of output capacitance over the entire line and load range must be done experimentally. If the majority of the load current is drawn from the secondary isolated output, a better approximation of the primary output voltage ripple is given by Equation 25.

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$$\Delta V_{OUT1} = \frac{(I_{OUT2} \times \frac{N2}{N1}) \times T_{ON(MAX)}}{C_{OUT1}} \quad (25)$$

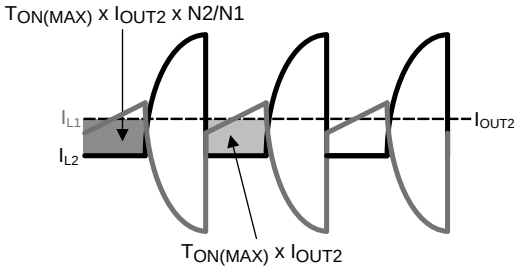


Figure 18. Current Waveforms for C_{OUT1} Ripple Calculation

To limit the primary output ripple voltage to approximately 100 mV, an output capacitor of 4 µF is required. A standard 4.7-µF, 16 V capacitor is selected for this design. If lower output voltage ripple is required, a higher value should be selected for C_{OUT1} and/or C_{OUT2}.

8.2.2.2.7 Secondary Output Capacitor

A simplified waveform for secondary output current (I_{OUT2}) is shown in Figure 19.

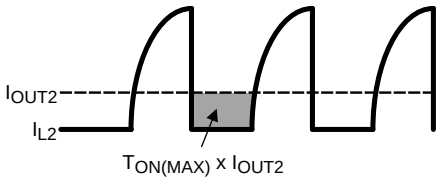


Figure 19. Secondary Current Waveforms for C_{OUT2} Ripple Calculation

The secondary output current (I_{OUT2}) is sourced by C_{OUT2} during on-time of the buck switch, T_{ON}. Ignoring the current transition times in the secondary winding, the secondary output capacitor ripple voltage can be calculated using Equation 26.

$$\Delta V_{OUT2} = \frac{I_{OUT2} \text{ x } T_{ON\ (MAX)}}{C_{OUT2}} \quad (26)$$

For a 1:1 transformer turns ratio, the primary and secondary voltage ripple equations are identical. A C_{OUT2} value of 2.2 µF is chosen for this design.

If lower output voltage ripple is required, a higher value should be selected for C_{OUT1} and/or C_{OUT2}.

8.2.2.2.8 Type III Feedback Ripple Circuit

Type III ripple circuit as described in is required for the Fly-Buck topology. Type I and Type II ripple circuits use series resistance and the triangular inductor ripple current to generate ripple at V_{OUT} and the FB pin. The primary ripple current of a Fly-Buck is the combination or primary and reflected secondary currents as illustrated in Figure 18. In the Fly-Buck topology, Type I and Type II ripple circuits suffer from large jitter as the reflected load current affects the feedback ripple.

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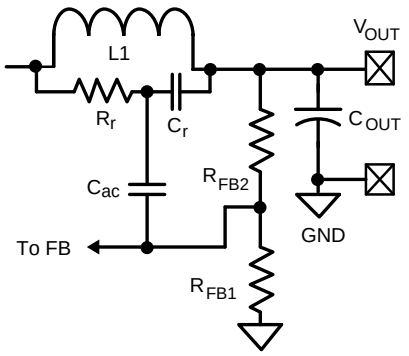


Figure 20. Type III Ripple Circuit

Selecting the Type III ripple components using the equations from will ensure that the FB pin ripple is greater than the capacitive ripple from the primary output capacitor C_{OUT1}. The feedback ripple component values are chosen as shown in Equation 27.

$$C_r = 1000 \text{ pF}$$

$$C_{ac} = 0.1 \ \mu\text{F}$$

$$R_r C_r \le \frac{(V_{IN(MIN)} - V_{OUT}) \times T_{ON}}{100 \text{ mV}} \tag{27}$$

The calculated value for Rr is 66 kΩ. This value provides the minimum ripple for stable operation. A smaller resistance should be selected to allow for variations in T_{ON}, C_{OUT1} and other components. For this design, Rr value of 46.4 kΩ is selected.

8.2.2.2.9 Secondary Diode

The reverse voltage across secondary-rectifier diode D1 when the high-side buck switch is off can be calculated using Equation 28.

$$V_{D1} = \frac{N2}{N1} V_{IN} \tag{28}$$

For a V_{IN_MAX} of 48 V and the 1:1 turns ratio of this design, a 60 V Schottky is selected.

8.2.2.2.10 V_{CC} and Bootstrap Capacitor

A 1-µF capacitor of 16 V or higher rating is recommended for the V_{CC} regulator bypass capacitor.

A good value for the BST pin bootstrap capacitor is 0.01-µF with a 16 V or higher rating.

8.2.2.2.11 Input Capacitor

The input capacitor is typically a combination of a smaller bypass capacitor located near the regulator IC and a larger bulk capacitor. The total input capacitance should be large enough to limit the input voltage ripple to a desired amplitude. For input ripple voltage ΔV_{IN}, C_{IN} can be calculated using Equation 29.

$$C_{IN} \ge \frac{I_{OUT(MAX)}}{4 \times f \times \Delta V_{IN}} \tag{29}$$

Choosing a ΔV_{IN} of 0.5 V gives a minimum C_{IN} of 0.6 µF. A standard value of 0.47 µF is selected for C_{BYP} in this design. A bulk capacitor of higher value reduces voltage spikes due to parasitic inductance between the power source to the converter. A standard value of 2.2 µF is selected for for C_{IN} in this design. The voltage ratings of the two input capacitors should be greater than the maximum input voltage under all conditions.

8.2.2.2.12 UVLO Resistors

UVLO resistors R_{UV1} and R_{UV2} set the undervoltage lockout threshold and hysteresis according to Equation 30 and Equation 31.

$$V_{IN\ (HYS)} = I_{HYS} \times R_{UV2} \tag{30}$$

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$$V_{IN}(\text{UVLO, rising}) = 1.225V \times \left(\frac{R_{UV2}}{R_{UV1}} + 1\right)$$

where

- I_{HYS} = 20 µA, typical. (31)

For a UVLO hysteresis of 2.5 V and UVLO rising threshold of 15 V, Equation 30 and Equation 31 require R_{UV1} of 11.8 kΩ and R_{UV2} of 127 kΩ and these values are selected for this design example.

8.2.2.2.13 V_{CC} Diode

Diode D2 is an optional diode connected between V_{OUT1} and the V_{CC} regulator output pin. When V_{OUT1} is more than one diode drop greater than the V_{CC} voltage, the V_{CC} bias current is supplied from V_{OUT1}. This results in reduced power losses in the internal V_{CC} regulator which improves converter efficiency. V_{OUT1} must be set to a voltage at least one diode drop higher than 8.55 V (the maximum V_{CC} voltage) if D2 is used to supply bias current.

8.2.2.3 Application Curves

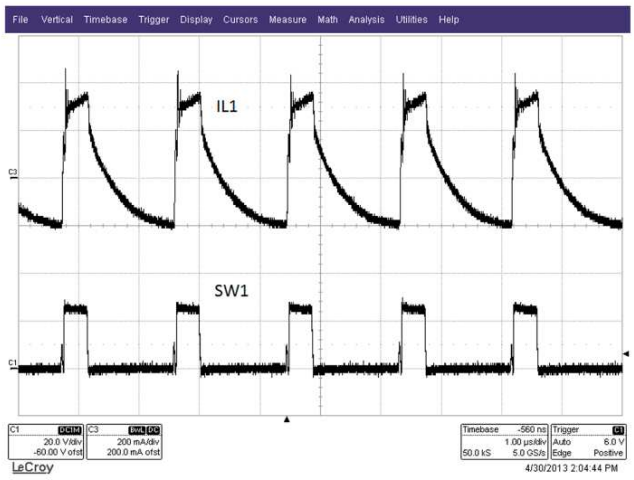


Figure 21. Steady State Waveform
(V_{IN} = 24 V, I_{OUT1} = 100 mA, I_{OUT2} = 200 mA)

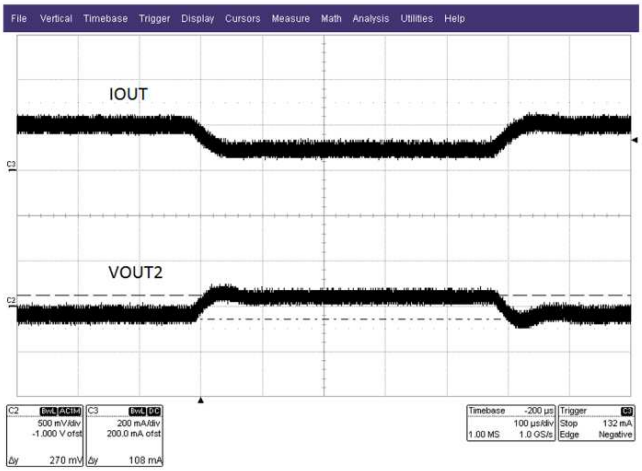


Figure 22. Step Load Response
(V_{IN} = 24 V, I_{OUT1} = 0, Step Load on I_{OUT2} = 100 mA to 200 mA)

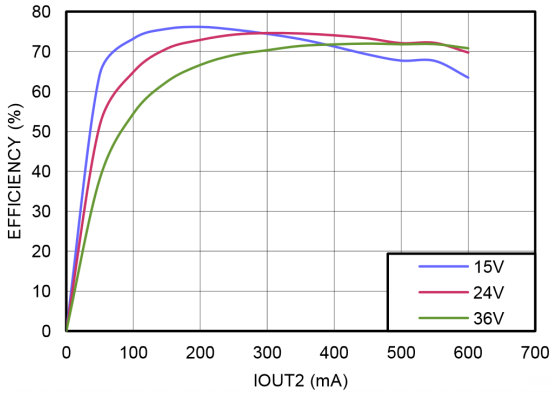


Figure 23. Efficiency at 500 kHz, V_{OUT1} = 5 V, V_{OUT2} = 4.5 V

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9 Power Supply Recommendations

LM25017 is a power management device. The power supply for the device is any dc voltage source within the specified input range.

10 Layout

10.1 Layout Guidelines

A proper layout is essential for optimum performance of the circuit. In particular, the following guidelines should be observed:

- C_{IN}: The loop consisting of input capacitor (C_{IN}), V_{IN} pin, and RTN pin carries switching currents. Therefore, the input capacitor should be placed close to the IC, directly across V_{IN} and RTN pins and the connections to these two pins should be direct to minimize the loop area. In general it is not possible to accommodate all of input capacitance near the IC. A good practice is to use a 0.1-µF or 0.47-µF capacitor directly across the V_{IN} and RTN pins close to the IC, and the remaining bulk capacitor as close as possible (see Figure 24).
- C_{VCC} and C_{BST}: The V_{CC} and bootstrap (BST) bypass capacitors supply switching currents to the high and low side gate drivers. These two capacitors should also be placed as close to the IC as possible, and the connecting trace length and loop area should be minimized (see Figure 24).
- The Feedback trace carries the output voltage information and a small ripple component that is necessary for proper operation of LM25017 device. Therefore, care should be taken while routing the feedback trace to avoid coupling any noise to this pin. In particular, feedback trace should not run close to magnetic components, or parallel to any other switching trace.
- SW trace: The SW node switches rapidly between V_{IN} and GND every cycle and is therefore a possible source of noise. The SW node area should be minimized. In particular, the SW node should not be inadvertently connected to a copper plane or pour.

10.2 Layout Example

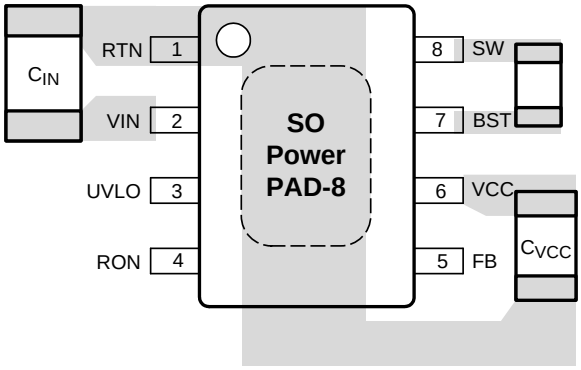


Figure 24. Placement of Bypass Capacitors

11 Device and Documentation Support

11.1 Documentation Support

11.1.1 Related Documentation

- AN-1481 *Controlling Output Ripple and Achieving ESR Independence in Constant On-Time (COT) Regulator Designs* (SNVA166)
- AN-2292 *Designing an Isolated Buck (Flybuck) Converter* (SNVA674)
- *LM25017 Evaluation Board* (SNVU228)
- *LM25017 Isolated Buck (FlyBuck) User's Guide* (SNVU264)

11.2 Trademarks

Fly-Buck is a trademark of Texas Instruments.
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11.3 Electrostatic Discharge Caution



These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

11.4 Glossary

SLYZ022 — *TI Glossary*.

This glossary lists and explains terms, acronyms, and definitions.

12 Mechanical, Packaging, and Orderable Information

The following pages include mechanical, packaging, and orderable information. This information is the most current data available for the designated devices. This data is subject to change without notice and revision of this document. For browser-based versions of this data sheet, refer to the left-hand navigation.

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PACKAGING INFORMATION

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead/Ball Finish (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
LM25017MR/NOPB	ACTIVE	SO PowerPAD	DDA	8	95	Green (RoHS & no Sb/Br)	CU SN	Level-3-260C-168 HR	-40 to 125	L25017 MR	Samples
LM25017MRE/NOPB	ACTIVE	SO PowerPAD	DDA	8	250	Green (RoHS & no Sb/Br)	CU SN	Level-3-260C-168 HR	-40 to 125	L25017 MR	Samples
LM25017MRX/NOPB	ACTIVE	SO PowerPAD	DDA	8	2500	Green (RoHS & no Sb/Br)	CU SN	Level-3-260C-168 HR	-40 to 125	L25017 MR	Samples
LM25017SD/NOPB	ACTIVE	WSON	NGU	8	1000	Green (RoHS & no Sb/Br)	CU SN	Level-1-260C-UNLIM	-40 to 125	L25017	Samples
LM25017SDE/NOPB	ACTIVE	WSON	NGU	8	250	Green (RoHS & no Sb/Br)	CU SN	Level-1-260C-UNLIM	-40 to 125	L25017	Samples
LM25017SDX/NOPB	ACTIVE	WSON	NGU	8	4500	Green (RoHS & no Sb/Br)	CU SN	Level-1-260C-UNLIM	-40 to 125	L25017	Samples

(1) The marketing status values are defined as follows:
ACTIVE: Product device recommended for new designs.
LIFEBUY: TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.
NRND: Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.
PREVIEW: Device has been announced but is not in production. Samples may or may not be available.
OBSOLETE: TI has discontinued the production of the device.

(2) Eco Plan - The planned eco-friendly classification: Pb-Free (RoHS), Pb-Free (RoHS Exempt), or Green (RoHS & no Sb/Br) - please check http://www.ti.com/productcontent for the latest availability information and additional product content details.
TBD: The Pb-Free/Green conversion plan has not been defined.
Pb-Free (RoHS): TI's terms "Lead-Free" or "Pb-Free" mean semiconductor products that are compatible with the current RoHS requirements for all 6 substances, including the requirement that lead not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, TI Pb-Free products are suitable for use in specified lead-free processes.
Pb-Free (RoHS Exempt): This component has a RoHS exemption for either 1) lead-based flip-chip solder bumps used between the die and package, or 2) lead-based die adhesive used between the die and leadframe. The component is otherwise considered Pb-Free (RoHS compatible) as defined above.
Green (RoHS & no Sb/Br): TI defines "Green" to mean Pb-Free (RoHS compatible), and free of Bromine (Br) and Antimony (Sb) based flame retardants (Br or Sb do not exceed 0.1% by weight in homogeneous material)

(3) MSL, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "~" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.

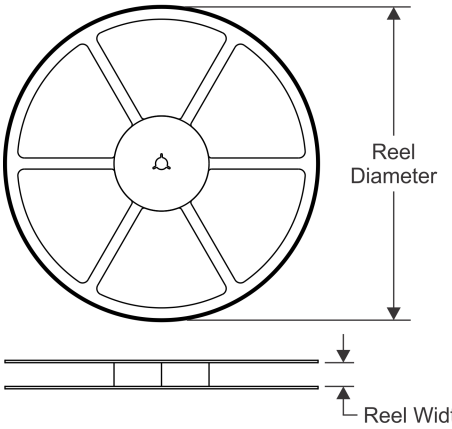
(6) Lead/Ball Finish - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead/Ball Finish values may wrap to two lines if the finish value exceeds the maximum column width.

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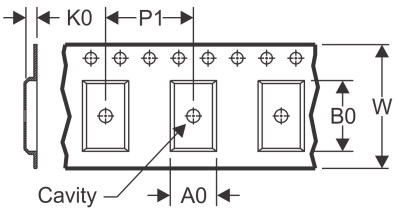
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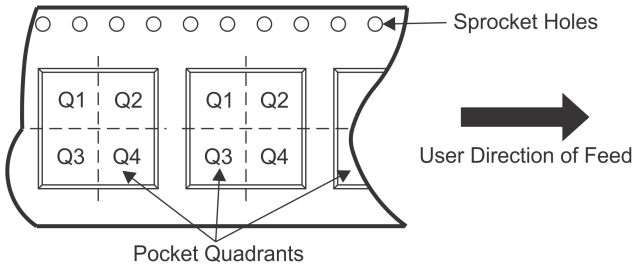


TAPE DIMENSIONS



A0	Dimension designed to accommodate the component width
B0	Dimension designed to accommodate the component length
K0	Dimension designed to accommodate the component thickness
W	Overall width of the carrier tape
P1	Pitch between successive cavity centers

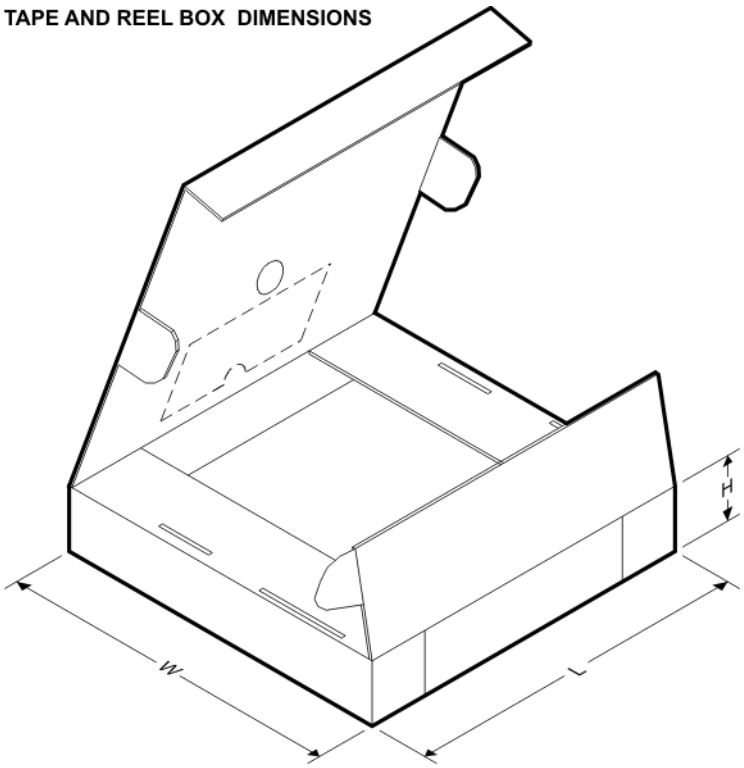
QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE



*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
LM25017MRE/NOPB	SO Power PAD	DDA	8	250	178.0	12.4	6.5	5.4	2.0	8.0	12.0	Q1
LM25017MRX/NOPB	SO Power PAD	DDA	8	2500	330.0	12.4	6.5	5.4	2.0	8.0	12.0	Q1
LM25017SD/NOPB	WSON	NGU	8	1000	178.0	12.4	4.3	4.3	1.3	8.0	12.0	Q1
LM25017SDE/NOPB	WSON	NGU	8	250	178.0	12.4	4.3	4.3	1.3	8.0	12.0	Q1
LM25017SDX/NOPB	WSON	NGU	8	4500	330.0	12.4	4.3	4.3	1.3	8.0	12.0	Q1

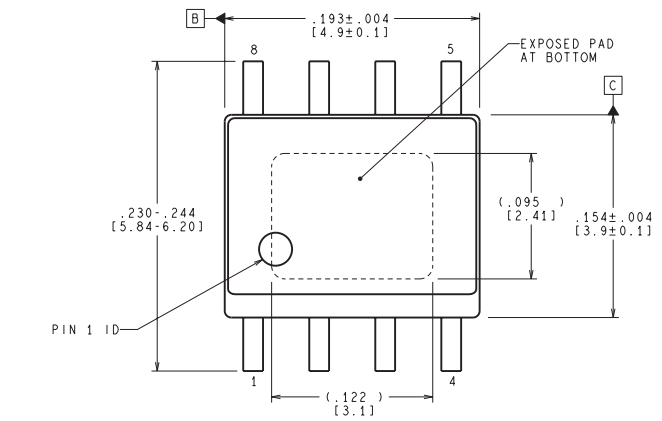
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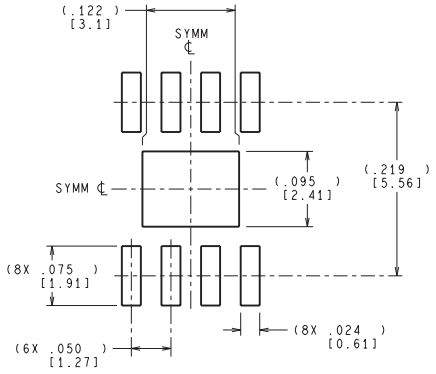


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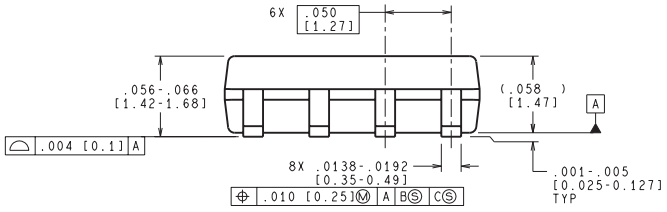
Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
LM25017MRE/NOPB	SO PowerPAD	DDA	8	250	213.0	191.0	55.0
LM25017MRX/NOPB	SO PowerPAD	DDA	8	2500	367.0	367.0	35.0
LM25017SD/NOPB	WSON	NGU	8	1000	210.0	185.0	35.0
LM25017SDE/NOPB	WSON	NGU	8	250	210.0	185.0	35.0
LM25017SDX/NOPB	WSON	NGU	8	4500	367.0	367.0	35.0

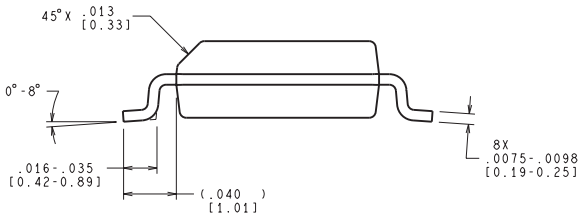
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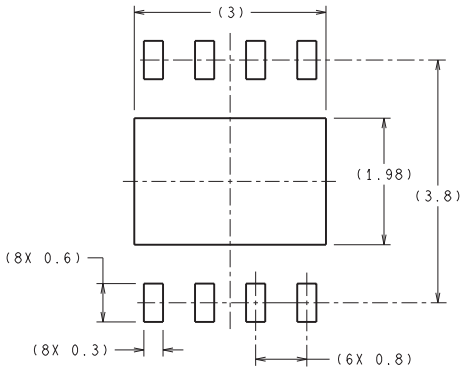




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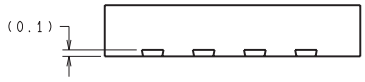
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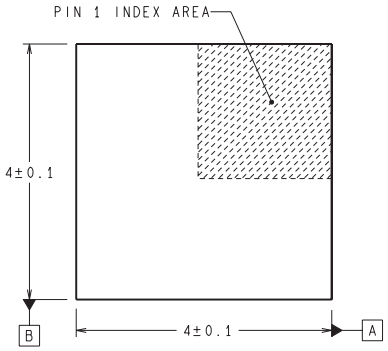
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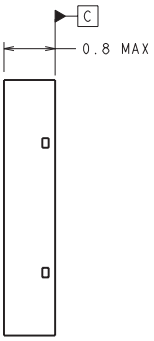


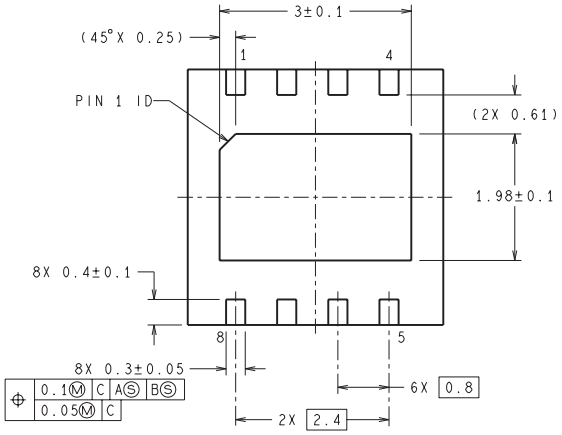
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