Dual 13A or Single 26A DC/DC µModule Regulator

FEATURES

- **Complete Standalone Dual Output Power Supply**
- **Dual 13A or Single 26A Output**
- **Wide Input Voltage Range: 4.5V to 16V**
- **Output Voltage Range: 0.6V to 2.5V**
- **±1.5% Maximum Total DC Output Error**
- **Multiphase Current Sharing with Multiple LTM4620s Up to 100A**
- Differential Remote Sense Amplifier
- Current Mode Control/Fast Transient Response
- Adjustable Switching Frequency
- Overcurrent Foldback Protection
- Frequency Synchronization
- Internal Temperature Sensing Diode Output
- Output Overvoltage Protection
- Low Profile (15mm × 15mm × 4.41mm) LGA Package

APPLICATIONS

- Telecom and Networking Equipment
- Storage and ATCA Cards
- Industrial Equipment

VIDEO TechClip

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- **100A and 26A Thermal Performance**
- **Current Sharing**
- **Short-Circuit Protection**

DESCRIPTION

The LTM®4620 is a complete dual 13A output switching mode DC/DC power supply. Included in the package are the switching controller, power FETs, inductors, and all supporting components. Operating from an input voltage range of 4.5V to 16V, the LTM4620 supports two outputs each with an output voltage range of 0.6V to 2.5V, set by a single external resistor. Its high efficiency design delivers up to 13A continuous current for each output. Only a few input and output capacitors are needed.

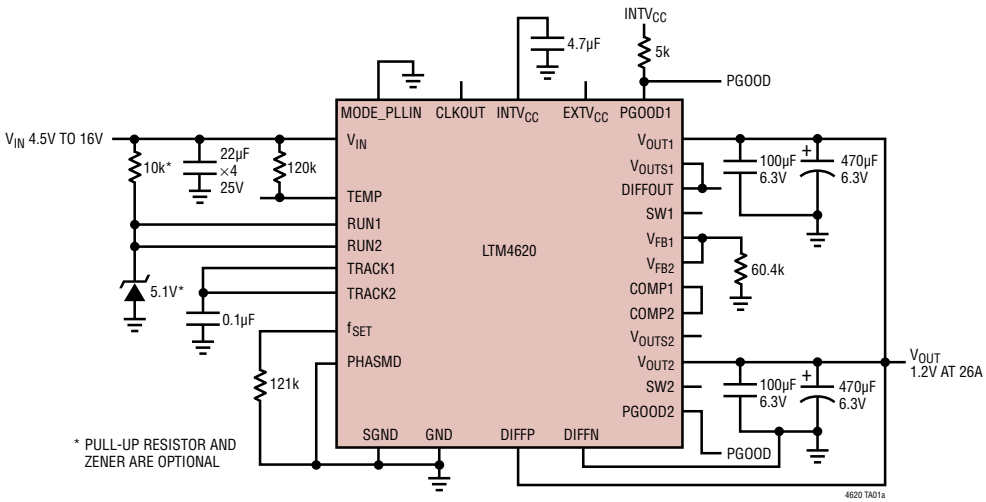
The device supports frequency synchronization, multiphase operation, Burst Mode operation and output voltage tracking for supply rail sequencing and has an onboard temperature diode for device temperature monitoring. High switching frequency and a current mode architecture enable a very fast transient response to line and load changes without sacrificing stability.

Fault protection features include overvoltage and overcurrent protection. The power module is offered in a proprietary space saving and thermally enhanced 15mm × 15mm × 4.41mm LGA package with integrated top-side heat sink. The LTM4620 is RoHS compliant with a PB-free finish.

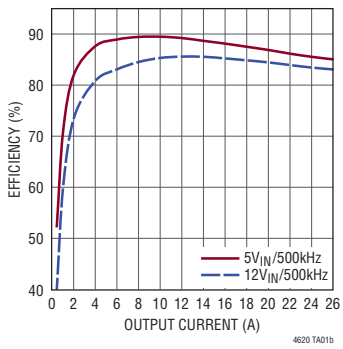
LT, LTC, LTM, Linear Technology, the Linear logo, µModule, Burst Mode and PolyPhase are registered trademarks and LTpowerCAD is a trademark of Linear Technology Corporation. All other trademarks are the property of their respective owners.

TYPICAL APPLICATION

26A, 1.2V Output DC/DC µModule® Regulator



1.2V Efficiency vs I_{OUT}

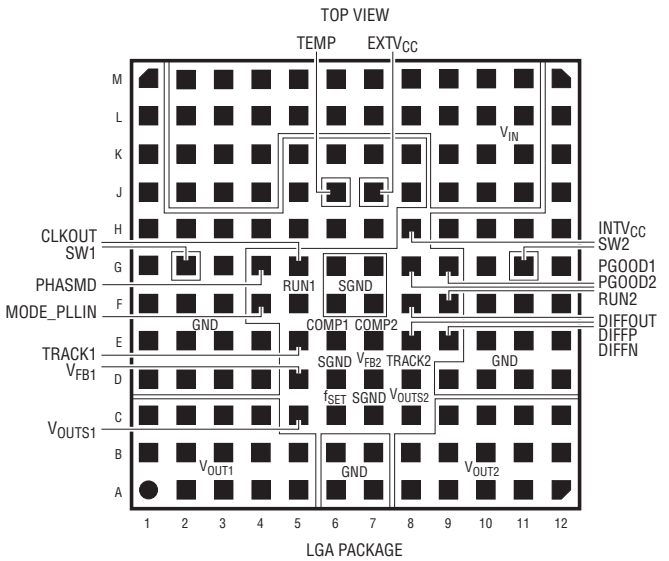


ABSOLUTE MAXIMUM RATINGS

(Note 1)

V_{IN} (Note 8) ..... –0.3V to 18V
V_{SW1}, V_{SW2} ..... –1V to 18V
PGOOD1, PGOOD2, RUN1, RUN2,
$INTV_{CC}$, $EXTV_{CC}$ ..... –0.3V to 6V
MODE_PLLIN, f_{SET}, TRACK1, TRACK2,
DIFFOUT, PHASMD..... –0.3V to $INTV_{CC}$
V_{OUT1}, V_{OUT2}, V_{OUTS1}, V_{OUTS2}..... –0.3V to 6V
DIFFP, DIFFN..... –0.3V to $INTV_{CC}$
COMP1, COMP2, V_{FB1}, V_{FB2} (Note 6) ..... –0.3V to 2.7V
$INTV_{CC}$ Peak Output Current 100mA
Internal Operating Temperature Range
(Note 2) .....–40°C to 125°C
Storage Temperature Range.....–55°C to 125°C
Peak Package Body Temperature ..... 250°C

PIN CONFIGURATION



LGA PACKAGE
144-LEAD (15mm × 15mm × 4.41mm)

T_{JMAX} = 125°C, Θ_{JA} = 7°C/W, $\Theta_{JCbottom}$ = 1.5°C/W,
Θ_{JCtop} = 3.7°C/W, Θ_{JB} + Θ_{BA} ≅ 7°C/W
Θ VALUES DEFINED PER JESD 51-12

ORDER INFORMATION

LEAD FREE FINISH	TRAY	PART MARKING*	PACKAGE DESCRIPTION	TEMPERATURE RANGE
LTM4620EV#PBF	LTM4620EV#PBF	LTM4620V	144-Lead (15mm × 15mm × 4.41mm) LGA	–40°C to 125°C
LTM4620IV#PBF	LTM4620IV#PBF	LTM4620V	144-Lead (15mm × 15mm × 4.41mm) LGA	–40°C to 125°C

Consult LTC Marketing for parts specified with wider operating temperature ranges. *The temperature grade is identified by a label on the shipping container.

For more information on lead free part marking, go to: http://www.linear.com/leadfree/
This product is only offered in trays. For more information go to: http://www.linear.com/packaging/

ELECTRICAL CHARACTERISTICS

The ● denotes the specifications which apply over the specified internal operating temperature range (Note 2). Specified as each individual output channel. T_A = 25°C, V_{IN} = 12V and V_{RUN1}, V_{RUN2} at 5V unless otherwise noted. Per the typical application in Figure 23.

SYMBOL	PARAMETER	CONDITIONS		MIN	TYP	MAX	UNITS
V_{IN}	Input DC Voltage		●	4.5		16	V
V_{OUT}	Output Voltage	(Note 8)	●	0.6		2.5	V
$V_{OUT1(DC)}$, $V_{OUT2(DC)}$	Output Voltage, Total Variation with Line and Load	C_{IN} = 22µF ×3, C_{OUT} = 100µF ×1 Ceramic, 470µF POSCAP, V_{OUT} = 1.5V	●	1.477	1.5	1.523	V
Input Specifications							
V_{RUN1}, V_{RUN2}	RUN Pin On/Off Threshold	RUN Rising		1.1	1.25	1.40	V
$V_{RUN1HYS}$, $V_{RUN2HYS}$	RUN Pin On Hysteresis				150		mV

ELECTRICAL CHARACTERISTICS

The ● denotes the specifications which apply over the specified internal operating temperature range (Note 2). Specified as each individual output channel. T_A = 25°C, V_{IN} = 12V and V_{RUN1}, V_{RUN2} at 5V unless otherwise noted. Per the typical application in Figure 23.

SYMBOL	PARAMETER	CONDITIONS		MIN	TYP	MAX	UNITS
$I_{INRUSH(VIN)}$	Input Inrush Current at Start-Up	I_{OUT} = 0A, C_{IN} = 22µF ×3, C_{SS} = 0.01µF, C_{OUT} = 100µF ×3, V_{OUT1} = 1.5V, V_{OUT2} = 1.5V, V_{IN} = 12V			1		A
$I_{Q(VIN)}$	Input Supply Bias Current	V_{IN} = 12V, V_{OUT} = 1.5V, Burst Mode Operation V_{IN} = 12V, V_{OUT} = 1.5V, Pulse-Skipping Mode V_{IN} = 12V, V_{OUT}= 1.5V, Switching Continuous Shutdown, RUN = 0, V_{IN} = 12V			5 15 65 50		mA mA mA µA
$I_{S(VIN)}$	Input Supply Current	V_{IN} = 5V, V_{OUT} = 1.5V, I_{OUT} = 13A V_{IN} = 12V, V_{OUT} = 1.5V, I_{OUT} = 13A			4.6 1.853		A A
Output Specifications							
$I_{OUT1(DC)}$, $I_{OUT2(DC)}$	Output Continuous Current Range	V_{IN} = 12V, V_{OUT} = 1.5V (Notes 7, 8)		0		13	A
$\Delta V_{OUT1(LINE)}/V_{OUT1}$ $\Delta V_{OUT2(LINE)}/V_{OUT2}$	Line Regulation Accuracy	V_{OUT} = 1.5V, V_{IN} from 4.5V to 16V I_{OUT} = 0A for Each Output,	●		0.01	0.025	%/V
$\Delta V_{OUT1}/V_{OUT1}$ $\Delta V_{OUT2}/V_{OUT2}$	Load Regulation Accuracy	For Each Output, V_{OUT} = 1.5V, 0A to 13A V_{IN} = 12V (Note 7)	●		0.5	0.75	%
$V_{OUT1(AC)}$, $V_{OUT2(AC)}$	Output Ripple Voltage	For Each Output, I_{OUT} = 0A, C_{OUT} = 100µF ×3/ X7R/Ceramic, 470µF POSCAP, V_{IN} = 12V, V_{OUT} = 1.5V, Frequency = 400kHz			15		mV_{P-P}
f_S (Each Channel)	Output Ripple Voltage Frequency	V_{IN} = 12V, V_{OUT} = 1.5V, f_{SET} = 1.25V (Note 4)			500		kHz
f_{SYNC} (Each Channel)	SYNC Capture Range			400		780	kHz
$\Delta V_{OUTSTART}$ (Each Channel)	Turn-On Overshoot	C_{OUT} = 100µF/X5R/Ceramic, 470µF POSCAP, V_{OUT} = 1.5V, I_{OUT} = 0A V_{IN} = 12V			10		mV
t_{START} (Each Channel)	Turn-On Time	C_{OUT} = 100µF/X5R/Ceramic, 470µF POSCAP, No Load, TRACK/SS with 0.01µF to GND, V_{IN} = 12V			5		ms
$\Delta V_{OUT(LS)}$ (Each Channel)	Peak Deviation for Dynamic Load	Load: 0% to 50% to 0% of Full Load C_{OUT} = 22µF ×3/X5R/Ceramic, 470µF POSCAP V_{IN} = 12V, V_{OUT} = 1.5V			30		mV
t_{SETTLE} (Each Channel)	Settling Time for Dynamic Load Step	Load: 0% to 50% to 0% of Full Load, V_{IN} = 12V, C_{OUT} = 100µF, 470µF POSCAP			20		µs
$I_{OUT(PK)}$ (Each Channel)	Output Current Limit	V_{IN} = 12V, V_{OUT} = 1.5V			20		A
Control Section							
V_{FB1}, V_{FB2}	Voltage at V_{FB} Pins	I_{OUT} = 0A, V_{OUT} = 1.5V	●	0.592	0.600	0.606	V
I_{FB1}, I_{FB2}		(Note 6)			–5	–20	nA
V_{OVL}	Feedback Overvoltage Lockout		●	0.64	0.66	0.68	V
TRACK1 (I), TRACK2 (I)	Track Pin Soft-Start Pull-Up Current	TRACK1 (I),TRACK2 (I) Start at 0V		1	1.25	1.5	µA
UVLO	Undervoltage Lockout	V_{IN} Falling V_{IN} Rising			3.3 3.9		V V
UVLO Hysteresis					0.6		V
$t_{ON(MIN)}$	Minimum On-Time	(Note 6)			90		ns
R_{FBHI1}, R_{FBHI2}	Resistor Between V_{OUTS1}, V_{OUTS2} and V_{FB1}, V_{FB2} Pins for Each Output			60.05	60.4	60.75	kΩ
V_{PGOOD1}, V_{PGOOD2} Low	PGOOD Voltage Low	I_{PGOOD} = 2mA			0.1	0.3	V
I_{PGOOD}	PGOOD Leakage Current	V_{PGOOD} = 5V				±5	µA

ELECTRICAL CHARACTERISTICS

The ● denotes the specifications which apply over the specified internal operating temperature range (Note 2). Specified as each individual output channel. T_A = 25°C, V_{IN} = 12V and VRUN1, VRUN2 at 5V unless otherwise noted. Per the typical application in Figure 23.

SYMBOL	PARAMETER	CONDITIONS		MIN	TYP	MAX	UNITS
V_{PGOOD}	PGOOD Trip Level	V_{FB} with Respect to Set Output Voltage V_{FB} Ramping Negative V_{FB} Ramping Positive			 –10 10		 % %
$INTV_{CC}$ Linear Regulator							
V_{INTVCC}	Internal V_{CC} Voltage	6V < V_{IN} < 16V		4.8	5	5.2	V
V_{INTVCC} Load Regulation	$INTV_{CC}$ Load Regulation	I_{CC} = 0mA to 50mA			0.5	2	%
V_{EXTVCC}	$EXTV_{CC}$ Switchover Voltage	$EXTV_{CC}$ Ramping Positive		4.5	4.7		V
$V_{EXTVCC(DROP)}$	$EXTV_{CC}$ Dropout	I_{CC} = 20mA, V_{EXTVCC} = 5V			50	100	mV
$V_{EXTVCC(HYST)}$	$EXTV_{CC}$ Hysteresis				200		mV
Oscillator and Phase-Locked Loop							
Frequency Nominal	Nominal Frequency	f_{SET} = 1.2V		450	500	550	kHz
Frequency Low	Lowest Frequency	f_{SET} = 0V (Note 5)		210	250	290	kHz
Frequency High	Highest Frequency	f_{SET} > 2.4V, Up to $INTV_{CC}$		700	780	860	kHz
f_{SET}	Frequency Set Current			9	10	11	µA
R_{MODE_PLLIN}	MODE_PLLIN Input Resistance				250		kΩ
CLKOUT	Phase (Relative to V_{OUT1})	PHASMD = GND PHASMD = Float PHASMD = $INTV_{CC}$			60 90 120		Deg Deg Deg
CLK High CLK Low	Clock High Output Voltage Clock Low Output Voltage			2		 0.2	V V
Differential Amplifier							
A_V Differential Amplifier	Gain				1		V/V
R_{IN}	Input Resistance	Measured at DIFFP Input			80		kΩ
V_{OS}	Input Offset Voltage	V_{DIFFP} = $V_{DIFFOUT}$ = 1.5V, $I_{DIFFOUT}$ = 100µA				3	mV
PSRR Differential Amplifier	Power Supply Rejection Ratio	5V < V_{IN} < 16V			90		dB
I_{CL}	Maximum Output Current				2		mA
$V_{OUT(MAX)}$	Maximum Output Voltage	$I_{DIFFOUT}$ = 300µA		$INTV_{CC}$ – 1.4			V
GBW	Gain Bandwidth Product				3		MHz
V_{TEMP} Temp Diode	Diode Connected PNP	I = 100µA			0.6		V
TC	Temperature Coefficient				–2.2		mV/°C

Note 1: Stresses beyond those listed under Absolute Maximum Ratings may cause permanent damage to the device. Exposure to any Absolute Maximum Rating condition for extended periods may affect device reliability and lifetime.

Note 2: The LTM4620 is tested under pulsed load conditions such that $T_J \approx T_A$. The LTM4620E is guaranteed to meet specifications from 0°C to 125°C internal temperature. Specifications over the –40°C to 125°C internal operating temperature range are assured by design, characterization and correlation with statistical process controls. The LTM4620I is guaranteed over the full –40°C to 125°C internal operating temperature range. Note that the maximum ambient temperature consistent with these specifications is determined by specific operating conditions in conjunction with board layout, the rated package thermal impedance and other environmental factors.

Note 3: Two outputs are tested separately and the same testing condition is applied to each output.

Note 4: The switching frequency is programmable from 400kHz to 750kHz.

Note 5: LTM4620 device is designed to operate from 400kHz to 750kHz

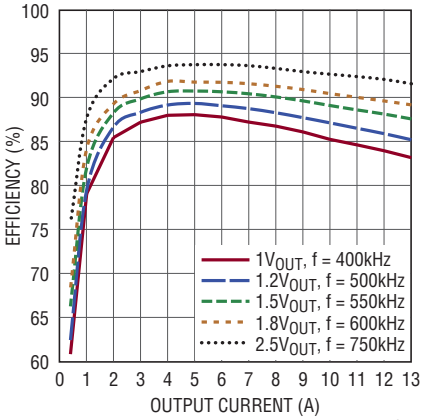
Note 6: These parameters are tested at wafer sort.

Note 7: See output current derating curves for different V_{IN}, V_{OUT} and T_A.

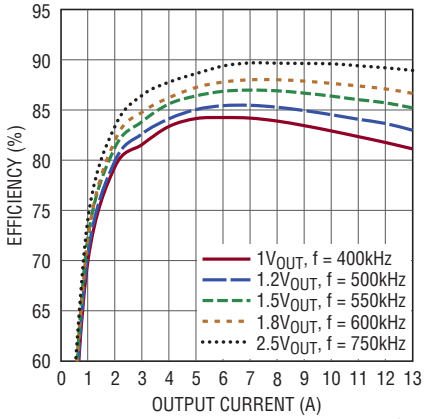
Note 8: Output current limitations. For 10V ≤ V_{IN} ≤ 16V, the 2.5V output current needs to be limited to 10A/channel, switching frequency = 750kHz. Derating curves apply. For 5V ≤ V_{IN} ≤ 9V, the 2.5V output current needs to be limited to 12A/channel, switching frequency = 750kHz. Derating curves apply. All other input and output combinations are 13A/channel with recommended switching frequency included in the efficiency graphs. Derating curves apply.

TYPICAL PERFORMANCE CHARACTERISTICS

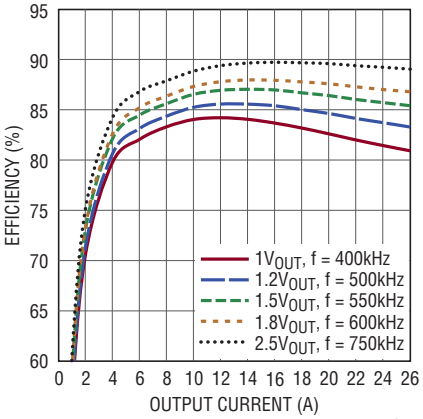
Efficiency vs Output Current, V_{IN} = 5V



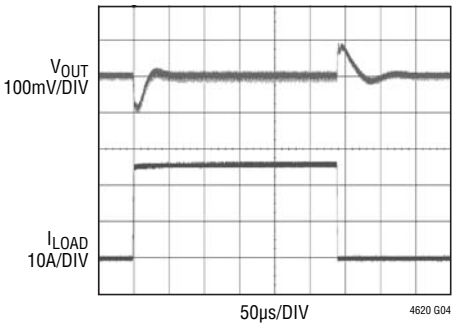
Efficiency vs Output Current, V_{IN} = 12V



Dual Phase Single Output Efficiency vs Output Current, V_{IN} = 12V

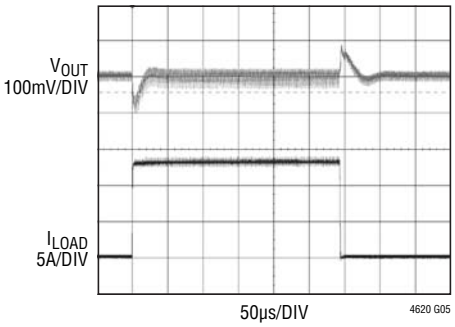


Dual Phase Single Output Load Transient Response



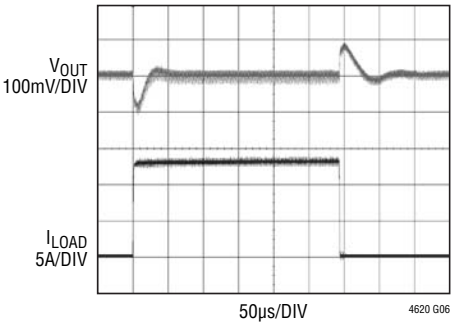
$12V_{IN}$, $1.5V_{OUT}$ AT 26A/µs LOAD STEP
C_{OUT} = 4× 470µF, 4V POSCAP AND
2× 100µF, 6.3V CERAMIC

Single Phase Single Output Load Transient Response



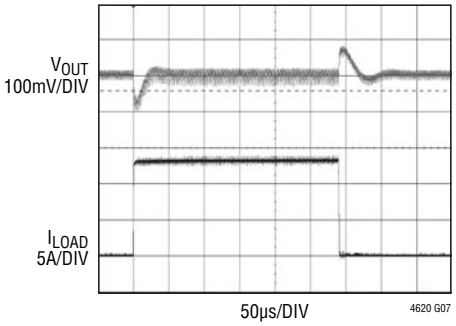
$12V_{IN}$, $1V_{OUT}$ AT 13A/µs LOAD STEP
C_{OUT} = 2× 470µF, 4V POSCAP AND
1× 100µF, 6.3V CERAMIC

Single Phase Single Output Load Transient Response



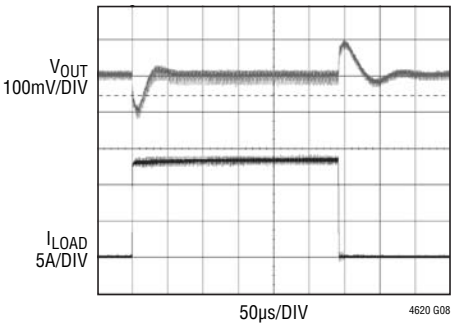
$12V_{IN}$, $1.2V_{OUT}$ AT 13A/µs LOAD STEP
C_{OUT} = 2× 470µF, 4V POSCAP AND
1× 100µF, 6.3V CERAMIC

Single Phase Single Output Load Transient Response



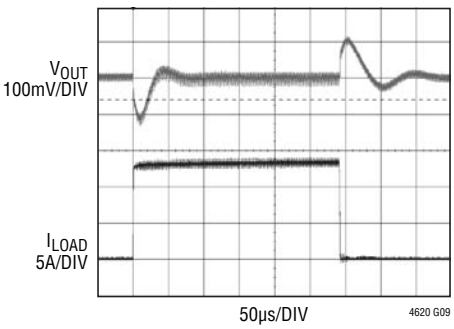
$12V_{IN}$, $1.5V_{OUT}$ AT 13A/µs LOAD STEP
C_{OUT} = 2× 470µF, 4V POSCAP AND
1× 100µF, 6.3V CERAMIC

Single Phase Single Output Load Transient Response



$12V_{IN}$, $1.8V_{OUT}$ AT 13A/µs LOAD STEP
C_{OUT} = 2× 470µF, 4V POSCAP AND
1× 100µF, 6.3V CERAMIC

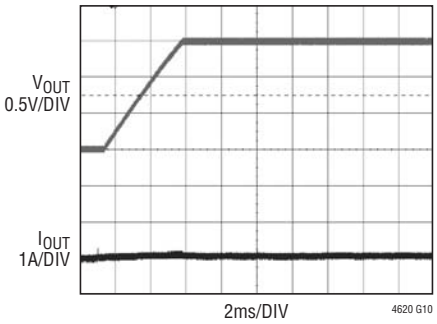
Single Phase Single Output Load Transient Response



$12V_{IN}$, $2.5V_{OUT}$ AT 13A/µs LOAD STEP
C_{OUT} = 2× 470µF, 4V POSCAP AND
1× 100µF, 6.3V CERAMIC

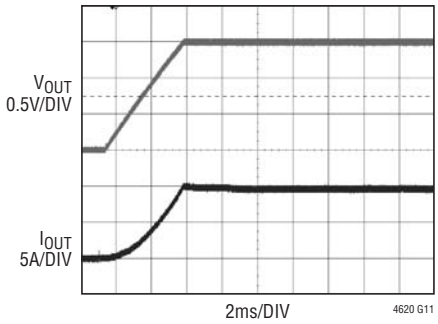
TYPICAL PERFORMANCE CHARACTERISTICS

Single Phase Single Output Start-Up



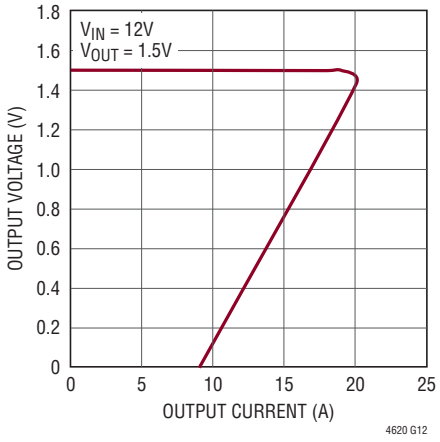
$12V_{IN}$, $1.5V_{OUT}$ AT NO LOAD
C_{OUT} = 2× 470µF, 4V SANYO POSCAP,
1× 100µF, 6.3V CERAMIC
SOFT-START CAPACITOR = 0.01µF
USE RUN PIN TO CONTROL START-UP

Single Phase Single Output Start-Up

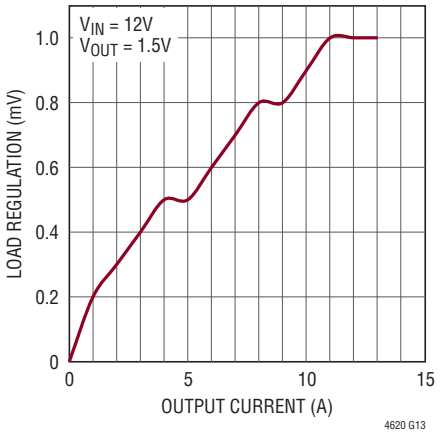


$12V_{IN}$, $1.5V_{OUT}$ AT 10A LOAD
C_{OUT} = 2× 470µF, 4V SANYO POSCAP,
1× 100µF, 6.3V X5R CERAMIC
SOFT-START CAPACITOR = 0.01µF
USE RUN PIN TO CONTROL START-UP

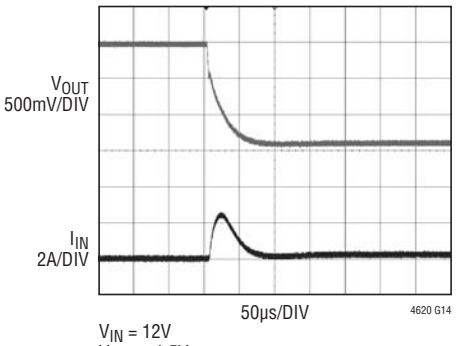
Current Limit and Current Foldback



Load Regulation vs Current

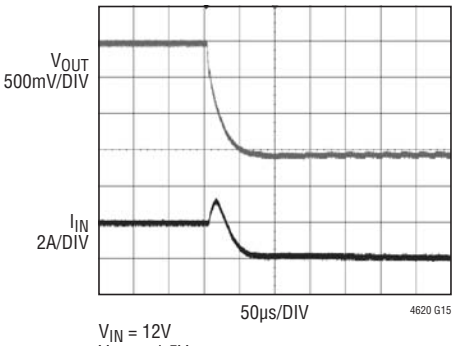


Short-Circuit Protection



V_{IN} = 12V
V_{OUT} = 1.5V
I_{OUT} = NO LOAD

Short-Circuit Protection



V_{IN} = 12V
V_{OUT} = 1.5V
I_{OUT} = 13A

PIN FUNCTIONS (Recommended to Use Test Points to Monitor Signal Pin Connections.)

V_{OUT1} (A1-A5, B1-B5, C1-C4): Power Output Pins. Apply output load between these pins and GND pins. Recommend placing output decoupling capacitance directly between these pins and GND pins. Review Table 4. See Note 8 in the Electrical Characteristics section for output current guideline.

GND (A6-A7, B6-B7, D1-D4, D9-D12, E1-E4, E10-E12, F1-F3, F10-F12, G1, G3, G10, G12, H1-H7, H9-H12, J1, J5, J8, J12, K1, K5-K8, K12, L1, L12, M1 , M12): Power Ground Pins for Both Input and Output Returns.

V_{OUT2} (A8-A12, B8-B12, C9-C12): Power Output Pins. Apply output load between these pins and GND pins. Recommend placing output decoupling capacitance directly between these pins and GND pins. Review Table 4. See Note 8 in the Electrical Characteristics section for output current guideline.

V_{OUTS1}, V_{OUTS2} (C5, C8): This pin is connected to the top of the internal top feedback resistor for each output. The pin can be directly connected to its specific output, or connected to DIFFOUT when the remote sense amplifier is used. In paralleling modules, one of the V_{OUTS} pins is connected to the DIFFOUT pin in remote sensing or directly to V_{OUT} with no remote sensing. It is very important to connect these pins to either the DIFFOUT or V_{OUT} since this is the feedback path, and cannot be left open. See the Applications Information section.

f_{SET} (C6): Frequency Set Pin. A 10µA current is sourced from this pin. A resistor from this pin to ground sets a voltage that in turn programs the operating frequency. Alternatively, this pin can be driven with a DC voltage that can set the operating frequency. See the Applications Information section.

SGND (C7, D6, G6-G7, F6-F7): Signal Ground Pin. Return ground path for all analog and low power circuitry. Tie a single connection to the output capacitor GND in the application. See layout guidelines in Figure 22.

V_{FB1}, V_{FB2} (D5, D7): The Negative Input of the Error Amplifier for Each Channel. Internally, this pin is connected to V_{OUTS1} or V_{OUTS2} with a 60.4kΩ precision resistor. Different output voltages can be programmed with an additional resistor between V_{FB} and GND pins. In PolyPhase® operation, tying the V_{FB} pins together allows for parallel operation. See the Applications Information section for details.

TRACK1, TRACK2 (E5, D8): Output Voltage Tracking Pin and Soft-Start Inputs. Each channel has a 1.3µA pull-up current source. When one channel is configured to be master of the two channels, then a capacitor from this pin to ground will set a soft-start ramp rate. The remaining channel can be set up as the slave, and have the master's output applied through a voltage divider to the slave output's track pin. This voltage divider is equal to the slave output's feedback divider for coincidental tracking. See the Applications Information section.

COMP1, COMP2 (E6, E7): Current control threshold and error amplifier compensation point for each channel. The current comparator threshold increases with this control voltage. Tie the COMP pins together for parallel operation. The device is internal compensated.

DIFFP (E8): Positive input of the remote sense amplifier. This pin is connected to the remote sense point of the output voltage. See the Applications Information section.

DIFFN (E9): Negative input of the remote sense amplifier. This pin is connected to the remote sense point of the output GND. See the Applications Information section.

MODE_PLLIN (F4): Force Continuous Mode, Burst Mode Operation, or Pulse-Skipping Mode Selection Pin and External Synchronization Input to Phase Detector Pin. Connect this pin to SGND to force both channels into force continuous mode of operation. Connect to $INTV_{CC}$ to enable pulse-skipping mode of operation. Leaving the pin floating will enable Burst Mode operation. A clock on the pin will force both channels into continuous mode of operation and synchronized to the external clock applied to this pin.

Heat Sink (Top Exposed Metal): The top exposed metal is at ground potential.

PIN FUNCTIONS (Recommended to Use Test Points to Monitor Signal Pin Connections.)

RUN1, RUN2 (F5, F9): Run Control Pin. A voltage above 1.25V will turn on each channel in the module. A voltage below 1.25V on the RUN pin will turn off the related channel. Each RUN pin has a 1µA pull-up current, once the RUN pin reaches 1.2V an additional 4.5µA pull-up current is added to this pin.

DIFFOUT (F8): Internal Remote Sense Amplifier Output. Connect this pin to V_{OUTS1} or V_{OUTS2} depending on which output is using remote sense. In parallel operation connect one of the V_{OUTS} pin to DIFFOUT for remote sensing.

SW1, SW2 (G2, G11): Switching node of each channel that is used for testing purposes. Also an R-C snubber network can be applied to reduce or eliminate switch node ringing, or otherwise leave floating. See the Applications Information section.

PHASMD (G4): Connect this pin to SGND, $INTV_{CC}$, or floating this pin to select the phase of CLKOUT to 60 degrees, 120 degrees, and 90 degrees respectively.

CLKOUT (G5): Clock output with phase control using the PHASMD pin to enable multiphase operation between devices. See the Applications Information section.

PGOOD1, PGOOD2 (G9, G8): Output Voltage Power Good Indicator. Open drain logic output that is pulled to ground when the output voltage is not within ±10% of the regulation point.

$INTV_{CC}$ (H8): Internal 5V Regulator Output. The control circuits and internal gate drivers are powered from this voltage. Decouple this pin to PGND with a 4.7µF low ESR tantalum or ceramic. $INTV_{CC}$ is activated when either RUN1 or RUN2 is activated.

TEMP (J6): Onboard Temperature Diode for Monitoring the VBE Junction Voltage Change with Temperature. See the Applications Information section.

$EXTV_{CC}$ (J7): External power input that is enabled through a switch to $INTV_{CC}$ whenever $EXTV_{CC}$ is greater than 4.7V. Do not exceed 6V on this input, and connect this pin to V_{IN} when operating V_{IN} on 5V. An efficiency increase will occur that is a function of the (V_{IN} – $INTV_{CC}$) multiplied by power MOSFET driver current. Typical current requirement is 30mA. V_{IN} must be applied before $EXTV_{CC}$, and $EXTV_{CC}$ must be removed before V_{IN}.

V_{IN} (M2-M11, L2-L11, J2-J4, J9-J11, K2-K4, K9-K11): Power Input Pins. Apply input voltage between these pins and GND pins. Recommend placing input decoupling capacitance directly between V_{IN} pins and GND pins.

Top Heat Sink: Top heat sink is at ground potential.

SIMPLIFIED BLOCK DIAGRAM

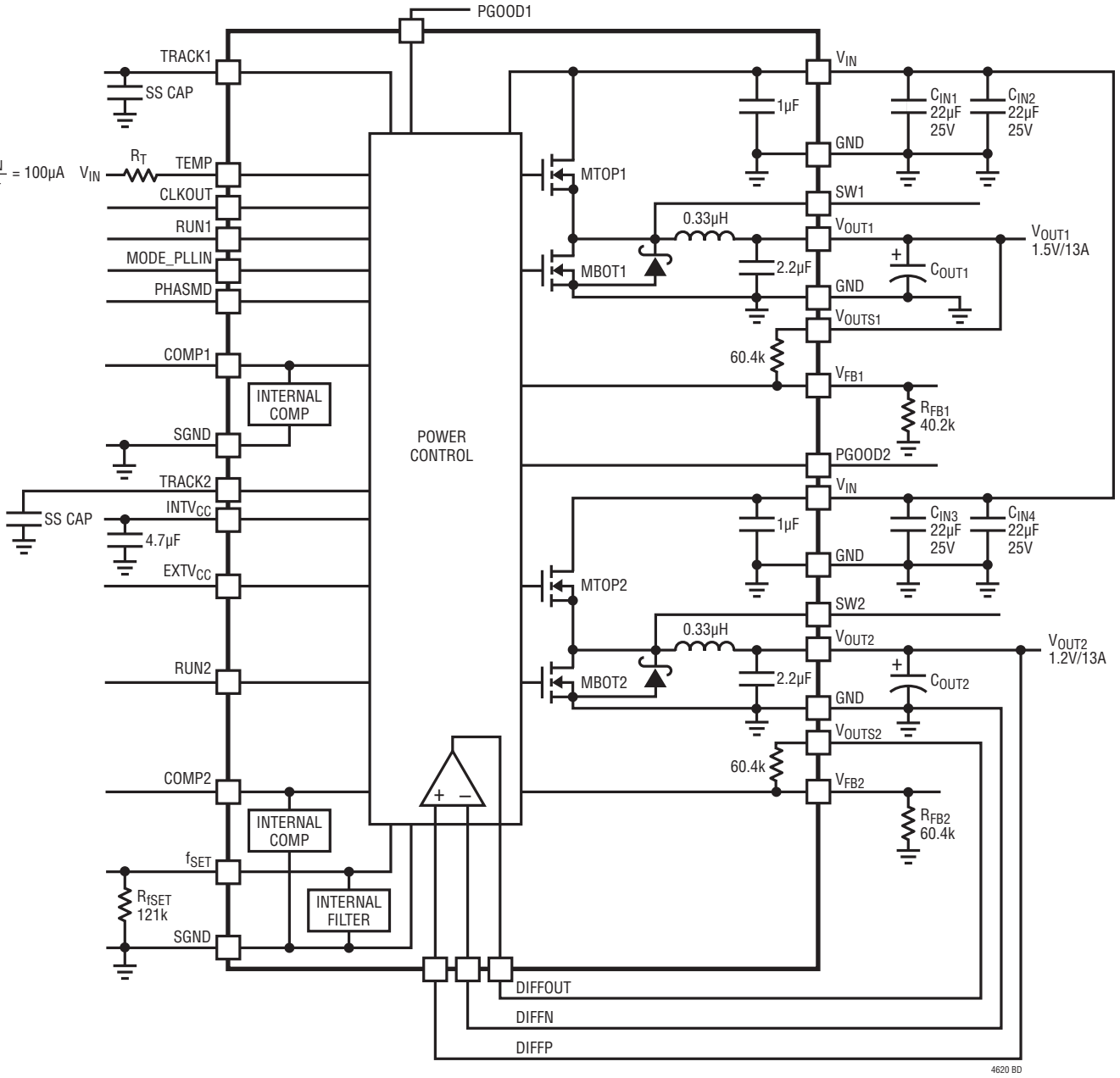


Figure 1. Simplified LTM4620 Block Diagram

DECOUPLING REQUIREMENTS

T_A = 25°C. Use Figure 1 configuration.

SYMBOL	PARAMETER	CONDITIONS		MIN	TYP	MAX	UNITS
C_{IN1}, C_{IN2} C_{IN3}, C_{IN4}	External Input Capacitor Requirement (V_{IN} = 4.5V to 16V, V_{OUT1} = 1.5V) (V_{IN} = 4.5V to 16V, V_{OUT2} = 1.2V)	 I_{OUT1} = 13A I_{OUT2} = 13A (Note 8)			22 22		µF µF
C_{OUT1} C_{OUT2}	External Output Capacitor Requirement (V_{IN} = 4.5V to 16V, V_{OUT1} = 1.5V) (V_{IN} = 4.5V to 16V, V_{OUT2} = 1.2V)	 I_{OUT1} = 13A I_{OUT2} = 13A (Note 8)			300 300		µF µF

OPERATION

Power Module Description

The LTM4620 is a dual-output standalone nonisolated switching mode DC/DC power supply. It can provide two 13A outputs with few external input and output capacitors and setup components. This module provides precisely regulated output voltages programmable via external resistors from $0.6V_{DC}$ to $2.5V_{DC}$ over 4.5V to 16V input voltages. The typical application schematic is shown in Figure 23. See Note 8 in the Electrical Characteristics section for output current guideline.

The LTM4620 has dual integrated constant-frequency current mode regulators and built-in power MOSFET devices with fast switching speed. The typical switching frequency is 500kHz. For switching-noise sensitive applications, it can be externally synchronized from 400kHz to 780kHz. A resistor can be used to program a free run frequency on the f_{SET} pin. See the Applications Information section.

With current mode control and internal feedback loop compensation, the LTM4620 module has sufficient stability margins and good transient performance with a wide range of output capacitors, even with all ceramic output capacitors.

Current mode control provides cycle-by-cycle fast current limit and foldback current limit in an overcurrent condition. Internal overvoltage and undervoltage comparators pull the open-drain PGOOD outputs low if the output feedback voltage exits a ±10% window around the regulation point. As the output voltage exceeds 10% above regulation, the bottom MOSFET will turn on to clamp the output voltage. The top MOSFET will be turned off. This overvoltage protect is feedback voltage referred.

Pulling the RUN pins below 1.1V forces the regulators into a shutdown state, by turning off both MOSFETs. The TRACK pins are used for programming the output voltage ramp and voltage tracking during start-up or used for soft-starting the regulator. See the Applications Information section.

The LTM4620 is internally compensated to be stable over all operating conditions. Table 4 provides a guide line for input and output capacitances for several operating conditions. The LTpowerCAD™ will be provided for transient and stability analysis. The V_{FB} pin is used to program the output voltage with a single external resistor to ground. A differential remote sense amplifier is available for sensing the output voltage accurately on one of the outputs at the load point, or in parallel operation sensing the output voltage at the load point.

Multiphase operation can be easily employed with the MODE_PLLIN, PHASMD, and CLKOUT pins. Up to 12 phases can be cascaded to run simultaneously with respect to each other by programming the PHASMD pin to different levels. See the Applications Information section.

High efficiency at light loads can be accomplished with selectable Burst Mode operation or pulse-skipping operation using the MODE_PLLIN pin. These light load features will accommodate battery operation. Efficiency graphs are provided for light load operation in the Typical Performance Characteristics section. See the Applications Information section for details.

A temperature diode is included inside the module to monitor the temperature of the module. See the Applications Information section for details.

The switching node pins are available for functional operation monitoring and a resistor-capacitor snubber circuit can be careful placed on the switching node pin to ground to dampen any high frequency ringing on the transition edges. See the Applications Information section for details.

APPLICATIONS INFORMATION

The typical LTM4620 application circuit is shown in Figure 23. External component selection is primarily determined by the maximum load current and output voltage. Refer to Table 4 for specific external capacitor requirements for particular applications.

V_{IN} to V_{OUT} Step-Down Ratios

There are restrictions in the maximum V_{IN} and V_{OUT} step-down ratio that can be achieved for a given input voltage. Each output of the LTM4620 is capable of 98% duty cycle, but the V_{IN} to V_{OUT} minimum dropout is still shown as a function of its load current and will limit output current capability related to high duty cycle on the top side switch. Minimum on-time $t_{ON(MIN)}$ is another consideration in operating at a specified duty cycle while operating at a certain frequency due to the fact that $t_{ON(MIN)} < D/f_{SW}$, where D is duty cycle and f_{SW} is the switching frequency. $t_{ON(MIN)}$ is specified in the electrical parameters as 90ns. See Note 8 in the Electrical Characteristics section for output current guideline.

Output Voltage Programming

The PWM controller has an internal 0.6V reference voltage. As shown in the Block Diagram, a 60.4kΩ internal feedback resistor connects between the V_{OUTS1} to V_{FB1} and V_{OUTS2} to V_{FB2}. It is very important that these pins be connected to their respective outputs for proper feedback regulation. Overvoltage can occur if these V_{OUTS1} and V_{OUTS2} pins are left floating when used as individual regulators, or at least one of them is used in paralleled regulators. The output voltage will default to 0.6V with no feedback resistor on either V_{FB1} or V_{FB2}. Adding a resistor R_{FB} from V_{FB} pin to GND programs the output voltage:

$$V_{OUT} = 0.6V \bullet \frac{60.4k + R_{FB}}{R_{FB}}$$

Table 1. V_{FB} Resistor Table vs Various Output Voltages

V_{OUT}	0.6V	1.0V	1.2V	1.5V	1.8V	2.5V
R_{FB}	Open	90.9k	60.4k	40.2k	30.2k	19.1k

For parallel operation of multiple channels the same feedback setting resistor can be used for the parallel design. This is done by connecting the V_{OUTS1} to the output as shown in Figure 2, thus tying one of the internal 60.4k resistors to the output. All of the V_{FB} pins tie together with one programming resistor as shown in Figure 2.

In parallel operation, the V_{FB} pins have an I_{FB} current of 20nA maximum each channel. To reduce output voltage error due to this current, an additional V_{OUTS} pin can be tied to V_{OUT}, and an additional R_{FB} resistor can be used to lower the total Thevenin equivalent resistance seen by this current. For example in Figure 2, the total Thevenin equivalent resistance of the V_{FB} pin is (60.4k//R_{FB}), which is 30.2k where R_{FB} is equal to 60.4k for a 1.2V output. Four phases connected in parallel equates to a worse case feedback current of 4 • I_{FB} = 80nA maximum. The voltage error is 80nA • 30.2k = 2.4mV. If V_{OUTS2} is connected, as shown in Figure 2, to V_{OUT}, and another 60.4k resistor is connected from V_{FB2} to ground, then the voltage error is reduced to 1.2mV. If the voltage error is acceptable then no additional connections are necessary. The onboard 60.4k resistor is 0.5% accurate and the V_{FB} resistor can be chosen by the user to be as accurate as needed. All COMP pins are tied together for current sharing between the phases. The TRACK pins can be tied together and a single soft-start capacitor can be used to soft-start the regulator. The soft-start equation will need to have the soft-start current parameter increased by the number of paralleled channels. See the Output Voltage Tracking section.

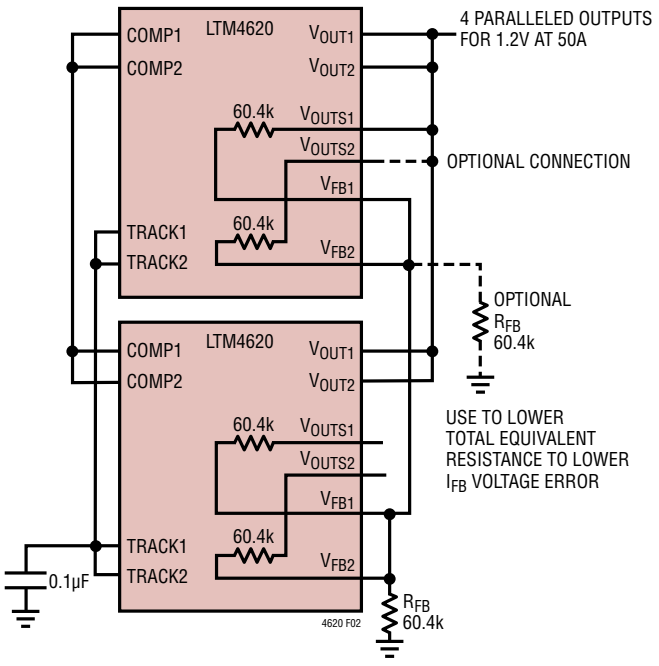


Figure 2. 4-Phase Parallel Configurations

APPLICATIONS INFORMATION

Input Capacitors

The LTM4620 module should be connected to a low ac-impedance DC source. For the regulator input four 22µF input ceramic capacitors are used for RMS ripple current. A 47µF to 100µF surface mount aluminum electrolytic bulk capacitor can be used for more input bulk capacitance. This bulk input capacitor is only needed if the input source impedance is compromised by long inductive leads, traces or not enough source capacitance. If low impedance power planes are used, then this bulk capacitor is not needed.

For a buck converter, the switching duty-cycle can be estimated as:

$$D = \frac{V_{OUT}}{V_{IN}}$$

Without considering the inductor current ripple, for each output, the RMS current of the input capacitor can be estimated as:

$$I_{CIN(RMS)} = \frac{I_{OUT(MAX)}}{\eta\%} \bullet \sqrt{D \bullet (1-D)}$$

In the above equation, η% is the estimated efficiency of the power module. The bulk capacitor can be a switcher-rated electrolytic aluminum capacitor, Polymer capacitor.

Output Capacitors

The LTM4620 is designed for low output voltage ripple noise and good transient response. The bulk output capacitors defined as C_{OUT} are chosen with low enough effective series resistance (ESR) to meet the output voltage ripple and transient requirements. C_{OUT} can be a low ESR tantalum capacitor, the low ESR polymer capacitor or ceramic capacitor. The typical output capacitance range for each output is from 200µF to 470µF. Additional output filtering may be required by the system designer, if further reduction of output ripples or dynamic transient spikes is required. Table 4 shows a matrix of different output voltages and output capacitors to minimize the voltage droop and overshoot during a 7A/µs transient. The table optimizes total equivalent ESR and total bulk capacitance to optimize the transient performance. Stability criteria are considered in the Table 4 matrix, and LTpowerCAD will be provided for stability analysis. Multiphase operation will reduce effective output ripple as a function of the number of phases. Application Note 77 discusses this noise reduction versus output ripple current cancellation, but the output capacitance should be considered carefully as a function of stability and transient response. LTpowerCAD can calculate the output ripple reduction as the number of implemented phases increases by N times. A small value 10Ω to 50Ω resistor can be placed in series from V_{OUT} to the V_{OUTS} pin to allow for a bode plot analyzer to inject a signal into the control loop and validate the regulator stability. The same resistor could be placed in series from V_{OUT} to DIFFP and a bode plot analyzer could inject a signal into the control loop and validate the regulator stability.

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Burst Mode Operation

The LTM4620 is capable of Burst Mode operation on each regulator in which the power MOSFETs operate intermittently based on load demand, thus saving quiescent current. For applications where maximizing the efficiency at very light loads is a high priority, Burst Mode operation should be applied. Burst Mode operation is enabled with the MODE_PLLIN pin floating. During this operation, the peak current of the inductor is set to approximately one third of the maximum peak current value in normal operation even though the voltage at the COMP pin indicates a lower value. The voltage at the COMP pin drops when the inductor's average current is greater than the load requirement. As the COMP voltage drops below 0.5V, the burst comparator trips, causing the internal sleep line to go high and turn off both power MOSFETs.

In sleep mode, the internal circuitry is partially turned off, reducing the quiescent current to about 450µA for each output. The load current is now being supplied from the output capacitors. When the output voltage drops, causing COMP to rise above 0.5V, the internal sleep line goes low, and the LTM4620 resumes normal operation. The next oscillator cycle will turn on the top power MOSFET and the switching cycle repeats. Either regulator can be configured for Burst Mode operation.

Pulse-Skipping Mode Operation

In applications where low output ripple and high efficiency at intermediate currents are desired, pulse-skipping mode should be used. Pulse-skipping operation allows the LTM4620 to skip cycles at low output loads, thus increasing efficiency by reducing switching loss. Tying the MODE_PLLIN pin to $INTV_{CC}$ enables pulse-skipping operation. At light loads the internal current comparator may remain tripped for several cycles and force the top MOSFET to stay off for several cycles, thus skipping cycles. The inductor current does not reverse in this mode. This mode will maintain higher effective frequencies thus lower output ripple and lower noise than Burst Mode operation. Either regulator can be configured for pulse-skipping mode.

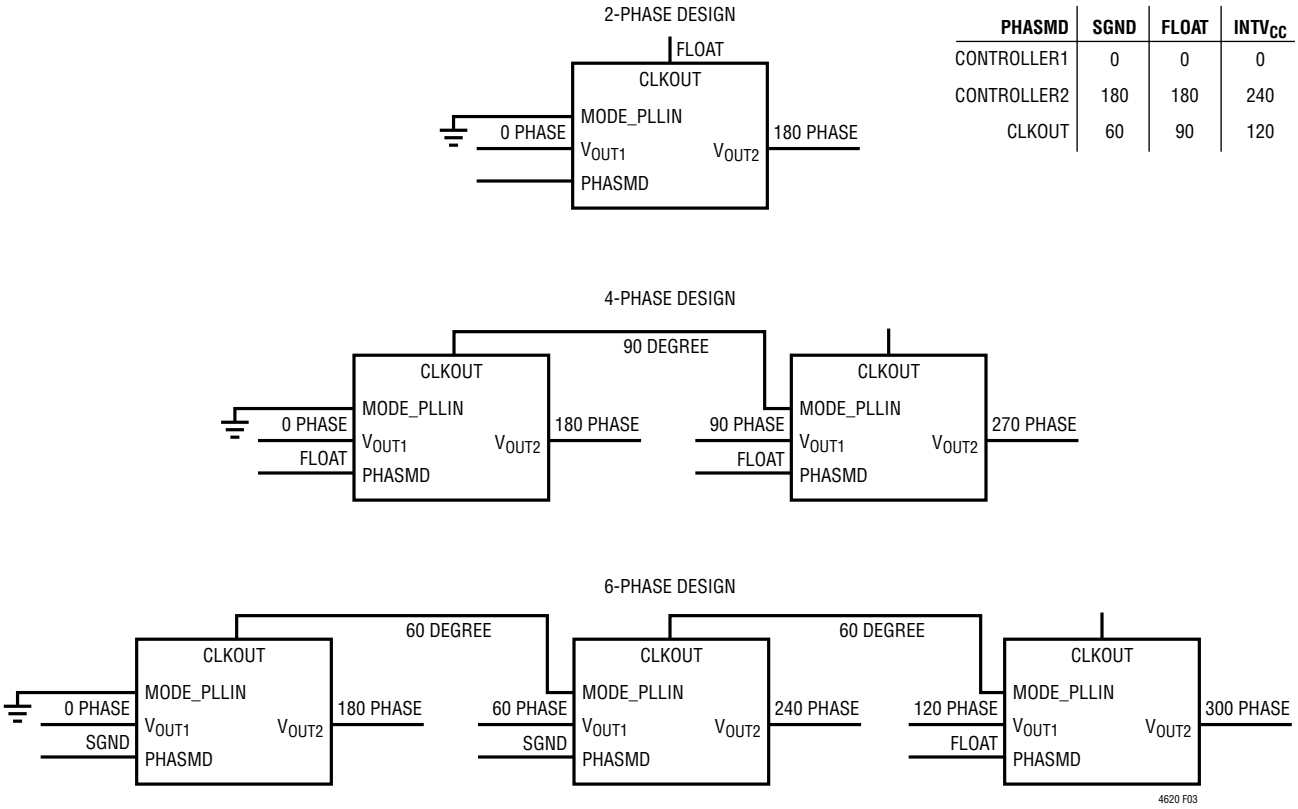
Forced Continuous Operation

In applications where fixed frequency operation is more critical than low current efficiency, and where the lowest output ripple is desired, forced continuous operation should be used. Forced continuous operation can be enabled by tying the MODE_PLLIN pin to GND. In this mode, inductor current is allowed to reverse during low output loads, the COMP voltage is in control of the current comparator threshold throughout, and the top MOSFET always turns on with each oscillator pulse. During start-up, forced continuous mode is disabled and inductor current is prevented from reversing until the LTM4620's output voltage is in regulation. Either regulator can be configured for forced continuous mode.

Multiphase Operation

For output loads that demand more than 13A of current, two outputs in LTM4620 or even multiple LTM4620s can be paralleled to run out of phase to provide more output current without increasing input and output voltage ripple. The MODE_PLLIN pin allows the LTM4620 to synchronize to an external clock (between 400kHz and 780kHz) and the internal phase-locked loop allows the LTM4620 to lock onto an incoming clock phase as well. The CLKOUT signal can be connected to the MODE_PLLIN pin of the following stage to line up both the frequency and the phase of the entire system. Tying the PHASMD pin to $INTV_{CC}$, SGND, or (floating) generates a phase difference (between MODE_PLLIN and CLKOUT) of 120 degrees, 60 degrees, or 90 degrees respectively. A total of 12 phases can be cascaded to run simultaneously with respect to each other by programming the PHASMD pin of each LTM4620 channel to different levels. Figure 3 shows a 2-phase design, 4-phase design and a 6-phase design example for clock phasing with the PHASMD table.

APPLICATIONS INFORMATION



PHASMD	SGND	FLOAT	$INTV_{CC}$
CONTROLLER1	0	0	0
CONTROLLER2	180	180	240
CLKOUT	60	90	120

Figure 3. Examples of 2-Phase, 4-Phase, and 6-Phase Operation with PHASMD Table

A multiphase power supply significantly reduces the amount of ripple current in both the input and output capacitors. The RMS input ripple current is reduced by, and the effective ripple frequency is multiplied by, the number of phases used (assuming that the input voltage is greater than the number of phases used times the output voltage). The output ripple amplitude is also reduced by the number of phases used when all of the outputs are tied together to achieve a single high output current design.

The LTM4620 device is an inherently current mode controlled device, so parallel modules will have very good current sharing. This will balance the thermals on the design. Figure 26 shows an example of parallel operation and pin connection.

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Input RMS Ripple Current Cancellation

Application Note 77 provides a detailed explanation of multiphase operation. The input RMS ripple current cancellation mathematical derivations are presented, and a graph is displayed representing the RMS ripple current reduction as a function of the number of interleaved phases. Figure 4 shows this graph.

Frequency Selection and Phase-Locked Loop (MODE_PLLIN and f_{SET} Pins)

The LTM4620 device is operated over a range of frequencies to improve power conversion efficiency. It is recommended to operate the lower output voltages or lower duty cycle conversions at lower frequencies to improve efficiency by lowering power MOSFET switching losses. Higher output voltages or higher duty cycle conversions can be operated at higher frequencies to limit inductor ripple current. The efficiency graphs will show an operating frequency chosen for that condition.

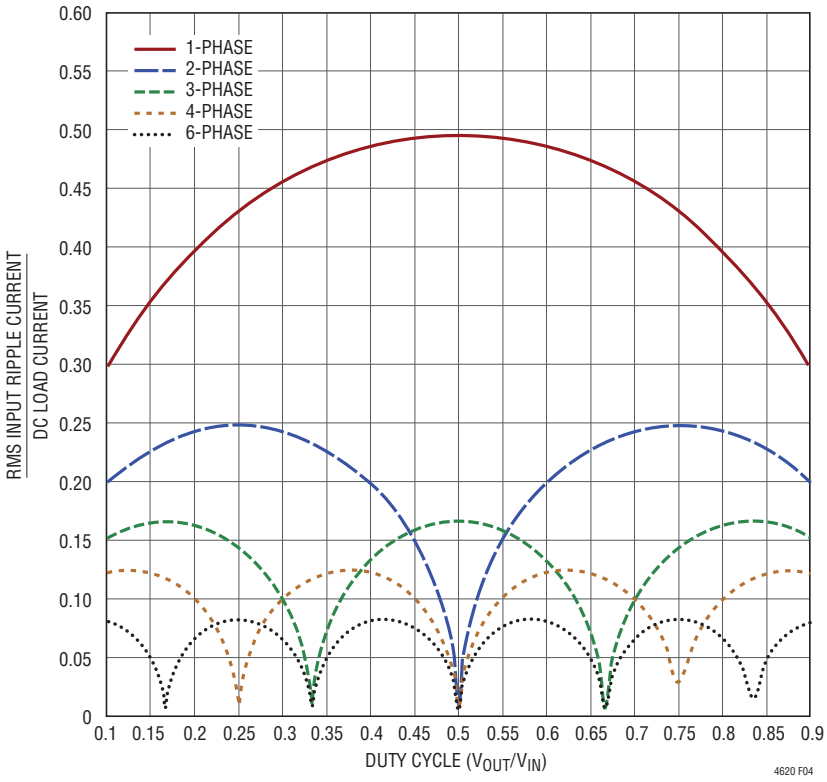

Figure 4. Input RMS Current Ratios to DC Load Current as a Function of Duty Cycle

APPLICATIONS INFORMATION

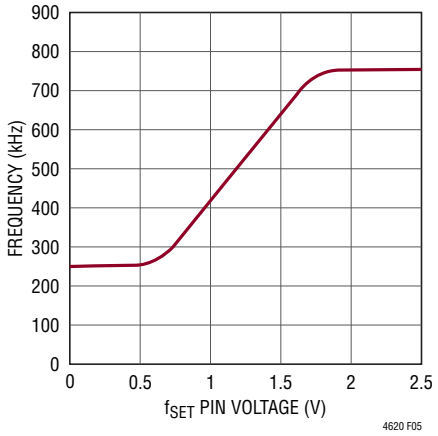

Figure 5. Operating Frequency vs f_{SET} Pin Voltage

The LTM4620 switching frequency can be set with an external resistor from the f_{SET} pin to SGND. An accurate 10µA current source into the resistor will set a voltage that programs the frequency or a DC voltage can be applied. Figure 5 shows a graph of frequency setting verses programming voltage. An external clock can be applied to the MODE_PLLIN pin from 0V to $INTV_{CC}$ over a frequency range of 400kHz to 780kHz. The clock input high threshold is 1.6V and the clock input low threshold is 1V. The LTM4620 has the PLL loop filter components on board. The frequency setting resistor should always be present to set the initial switching frequency before locking to an external clock. Both regulators will operate in continuous mode while being externally clocked.

The output of the PLL phase detector has a pair of complementary current sources that charge and discharge the internal filter network. When the external clock is applied, the f_{SET} frequency resistor is disconnected with an internal switch, and the current sources control the frequency adjustment to lock to the incoming external clock. When no external clock is applied, then the internal switch is on, thus connecting the external f_{SET} frequency set resistor for free run operation.

Minimum On-Time

Minimum on-time t_{ON} is the smallest time duration that the LTM4620 is capable of turning on the top MOSFET on either channel. It is determined by internal timing delays, and the gate charge required to turn on the top MOSFET. Low duty cycle applications may approach this minimum on-time limit and care should be taken to ensure that:

$$\frac{V_{OUT}}{V_{IN} \bullet FREQ} > t_{ON(MIN)}$$

If the duty cycle falls below what can be accommodated by the minimum on-time, the controller will begin to skip cycles. The output voltage will continue to be regulated, but the output ripple will increase. The on-time can be increased by lowering the switching frequency. A good rule of thumb is to keep on-time longer than 110ns.

Output Voltage Tracking

Output voltage tracking can be programmed externally using the TRACK pins. The output can be tracked up and down with another regulator. The master regulator's output is divided down with an external resistor divider that is the same as the slave regulator's feedback divider to implement coincident tracking. The LTM4620 uses an accurate 60.4k resistor internally for the top feedback resistor for each channel. Figure 6 shows an example of coincident tracking.

$$SLAVE = \left(1 + \frac{60.4k}{R_{TA}}\right) \bullet V_{TRACK}$$

V_{TRACK} is the track ramp applied to the slave's track pin. V_{TRACK} has a control range of 0V to 0.6V, or the internal reference voltage. When the master's output is divided down with the same resistor values used to set the slave's output, then the slave will coincident track with the master until it reaches its final value. The master will continue to its final value from the slave's regulation point. Voltage tracking is disabled when V_{TRACK} is more than 0.6V. R_{TA} in Figure 6 will be equal to the R_{FB} for coincident tracking. Figure 7 shows the coincident tracking waveforms.

APPLICATIONS INFORMATION

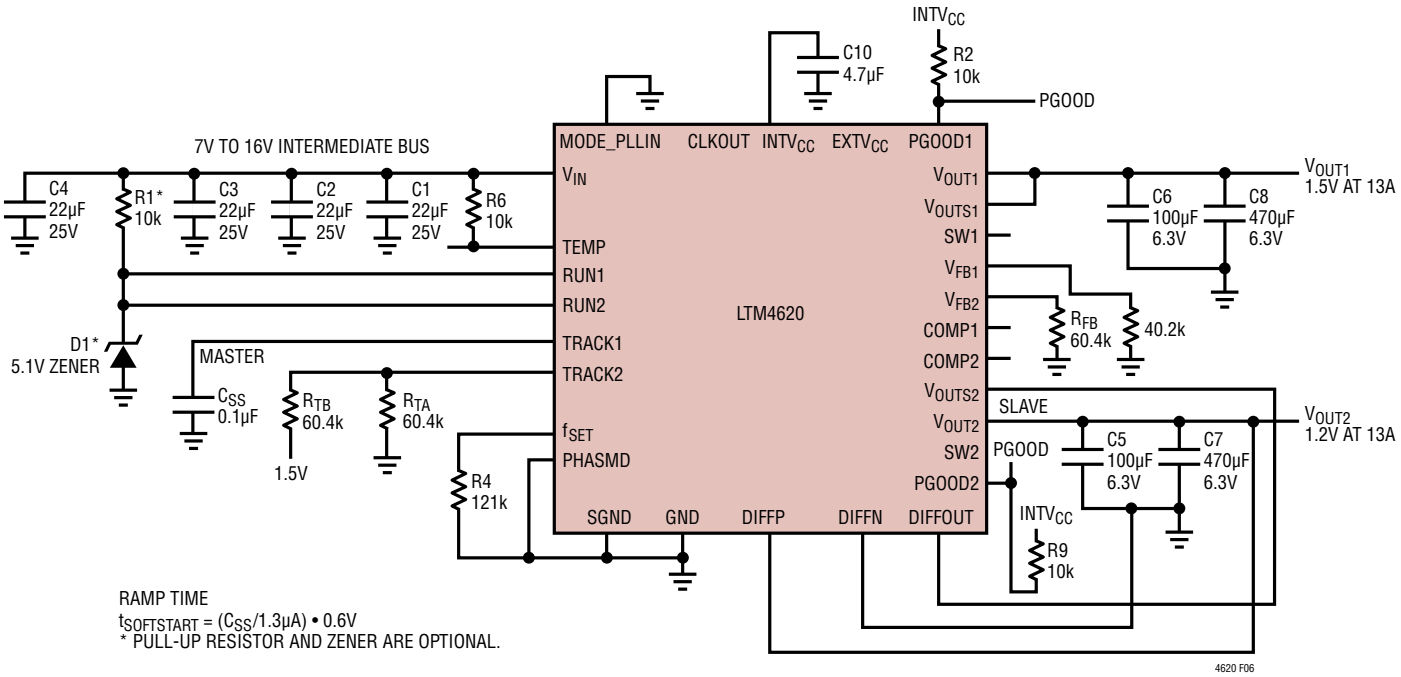

Figure 6. Example of Output Tracking Application Circuit

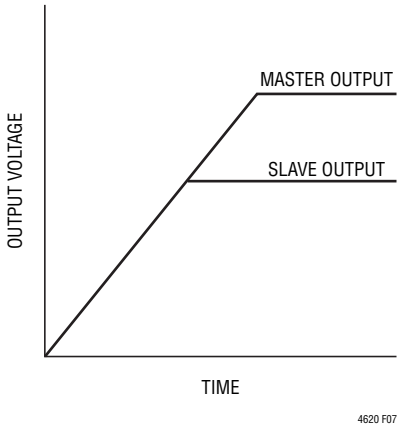

Figure 7. Output Coincident Tracking Waveform

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The TRACK pin can be controlled by a capacitor placed on the regulator TRACK pin to ground. A 1.3µA current source will charge the TRACK pin up to the reference voltage and then proceed up to $INTV_{CC}$. After the 0.6V ramp, the TRACK pin will no longer be in control, and the internal voltage reference will control output regulation from the feedback divider. Foldback current limit is disabled during this sequence of turn-on during tracking or soft-starting. The TRACK pins are pulled low when the RUN pin is below 1.2V. The total soft-start time can be calculated as:

$$t_{SOFT\text{-}START} = \left(\frac{C_{SS}}{1.3\mu A}\right) \bullet 0.6V$$

Regardless of the mode selected by the MODE_PLLIN pin, the regulator channels will always start in pulse-skipping mode up to TRACK = 0.5V. Between TRACK = 0.5V and 0.54V, it will operate in forced continuous mode and revert to the selected mode once TRACK > 0.54V. In order to track with another channel once in steady state operation, the LTM4620 is forced into continuous mode operation as soon as V_{FB} is below 0.54V regardless of the setting on the MODE_PLLIN pin.

Ratiometric tracking can be achieved by a few simple calculations and the slew rate value applied to the master's TRACK pin. As mentioned above, the TRACK pin has a control range from 0 to 0.6V. The master's TRACK pin slew rate is directly equal to the master's output slew rate in Volts/Time. The equation:

$$\frac{MR}{SR} \bullet 60.4k = R_{TB}$$

where MR is the master's output slew rate and SR is the slave's output slew rate in Volts/Time. When coincident tracking is desired, then MR and SR are equal, thus R_{TB} is equal the 60.4k. R_{TA} is derived from equation:

$$R_{TA} = \frac{0.6V}{\frac{V_{FB}}{60.4k} + \frac{V_{FB}}{R_{FB}} - \frac{V_{TRACK}}{R_{TB}}}$$

where V_{FB} is the feedback voltage reference of the regulator, and V_{TRACK} is 0.6V. Since R_{TB} is equal to the 60.4k top feedback resistor of the slave regulator in equal slew rate or coincident tracking, then R_{TA} is equal to R_{FB} with $V_{FB} = V_{TRACK}$. Therefore R_{TB} = 60.4k, and R_{TA} = 60.4k in Figure 6.

In ratiometric tracking, a different slew rate maybe desired for the slave regulator. R_{TB} can be solved for when SR is slower than MR. Make sure that the slave supply slew rate is chosen to be fast enough so that the slave output voltage will reach it final value before the master output.

For example, MR = 1.5V/1ms, and SR = 1.2V/1ms. Then R_{TB} = 76.8k. Solve for R_{TA} to equal to 49.9k.

Each of the TRACK pins will have the 1.3µA current source on when a resistive divider is used to implement tracking on that specific channel. This will impose an offset on the TRACK pin input. Smaller values resistors with the same ratios as the resistor values calculated from the above equation can be used. For example, where the 60.4k is used then a 6.04k can be used to reduce the TRACK pin offset to a negligible value.

Power Good

The PGOOD pins are open drain pins that can be used to monitor valid output voltage regulation. This pin monitors a ±10% window around the regulation point. A resistor can be pulled up to a particular supply voltage no greater than 6V maximum for monitoring.

Stability Compensation

The module has already been internally compensated for all output voltages. Table 4 is provided for most application requirements. LTpowerCAD will be provided for other control loop optimization.

Run Enable

The RUN pins have an enable threshold of 1.4V maximum, typically 1.25V with 150mV of hysteresis. They control the turn on each of the channels and $INTV_{CC}$. These pins can be pulled up to V_{IN} for 5V operation, or a 5V Zener diode can be placed on the pins and a 10k to 100k resistor can be placed up to higher than 5V input for enabling the channels. The RUN pins can also be used for output voltage sequencing. In parallel operation the RUN pins can be tie together and

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controlled from a single control. See the Typical Application circuits in Figure 23.

$INTV_{CC}$ and $EXTV_{CC}$

The LTM4620 module has an internal 5V low dropout regulator that is derived from the input voltage. This regulator is used to power the control circuitry and the power MOSFET drivers. This regulator can source up to 70mA, and typically uses ~30mA for powering the device at the maximum frequency. This internal 5V supply is enabled by either RUN1 or RUN2.

$EXTV_{CC}$ allows an external 5V supply to power the LTM4620 and reduce power dissipation from the internal low dropout 5V regulator. The power loss savings can be calculated by:

$$(V_{IN} – 5V) \bullet 30mA = PLOSS$$

$EXTV_{CC}$ has a threshold of 4.7V for activation, and a maximum rating of 6V. When using a 5V input, connect this 5V input to $EXTV_{CC}$ also to maintain a 5V gate drive level. $EXTV_{CC}$ must sequence on after V_{IN}, and $EXTV_{CC}$ must sequence off before V_{IN}.

Differential Remote Sense Amplifier

An accurate differential remote sense amplifier is provided to sense low output voltages accurately at the remote load points. This is especially true for high current loads. The amplifier can be used on one of the two channels, or on a single parallel output. It is very important that the DIFFP and DIFFN are connected properly at the output, and DIFFOUT is connected to either V_{OUTS1} or V_{OUTS2}. In parallel operation, the DIFFP and DIFFN are connected properly at the output, and DIFFOUT is connected to one of the V_{OUTS} pins. Review the parallel schematics in Figure 24 and review Figure 2.

SW Pins

The SW pins are generally for testing purposes by monitoring these pins. These pins can also be used to dampen out switch node ringing caused by LC parasitic in the switched current paths. Usually a series R-C combination is used called a snubber circuit. The resistor will dampen the resonance and the capacitor is chosen to only affect the high frequency ringing across the resistor. If the stray inductance or capacitance can be measured or approximated then a somewhat analytical technique can be used to select the snubber values. The inductance is usually easier to predict. It combines the power path board inductance in combination with the MOSFET interconnect bond wire inductance.

First the SW pin can be monitored with a wide bandwidth scope with a high frequency scope probe. The ring frequency can be measured for its value. The impedance Z can be calculated:

$$Z_{(L)} = 2\pi fL,$$

where f is the resonant frequency of the ring, and L is the total parasitic inductance in the switch path. If a resistor is selected that is equal to Z, then the ringing should be dampened. The snubber capacitor value is chosen so that its impedance is equal to the resistor at the ring frequency. Calculated by: $Z_{(C)} = 1/(2\pi fC)$. These values are a good place to start with. Modification to these components should be made to attenuate the ringing with the least amount of power loss.

Temperature Monitoring

Measuring the absolute temperature of a diode is possible due to the relationship between current, voltage and temperature described by the classic diode equation:

$$I_D = I_S \bullet e\left(\frac{V_D}{\eta \bullet V_T}\right)$$

or

$$V_D = \eta \bullet V_T \bullet \ln\frac{I_D}{I_S}$$

where I_D is the diode current, V_D is the diode voltage, η is the ideality factor (typically close to 1.0) and I_S (saturation current) is a process dependent parameter. V_T can be broken out to:

$$V_T = \frac{k \bullet T}{q}$$

where T is the diode junction temperature in Kelvin, q is the electron charge and k is Boltzmann's constant. V_T is approximately 26mV at room temperature (298K) and scales linearly with Kelvin temperature. It is this linear

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temperature relationship that makes diodes suitable temperature sensors. The I_S term in the equation above is the extrapolated current through a diode junction when the diode has zero volts across the terminals. The I_S term varies from process to process, varies with temperature, and by definition must always be less than I_D. Combining all of the constants into one term:

$$K_D = \frac{\eta \bullet k}{q}$$

where $K_D = 8.62 \bullet 10^{-5}$, and knowing $\ln(I_D/I_S)$ is always positive because I_D is always greater than I_S, leaves us with the equation that:

$$V_D = T(KELVIN) \bullet K_D \bullet \ln\frac{I_D}{I_S}$$

where V_D appears to increase with temperature. It is common knowledge that a silicon diode biased with a current source has an approximately –2mV/°C temperature relationship (Figure 8), which is at odds with the equation. In fact, the I_S term increases with temperature, reducing the $\ln(I_D/I_S)$ absolute value yielding an approximately –2mV/°C composite diode voltage slope.

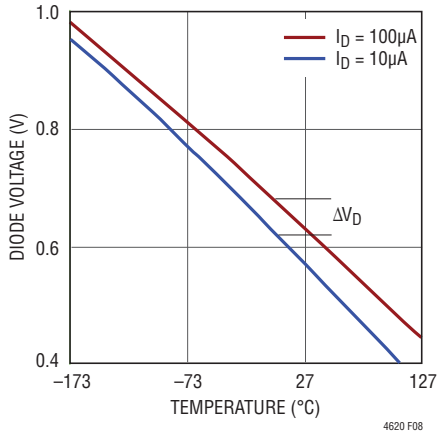

Figure 8. Diode Voltage V_D vs Temperature T(°C) for Different Bias Currents

To obtain a linear voltage proportional to temperature we cancel the I_S variable in the natural logarithm term to remove the I_S dependency from the following equation. This is accomplished by measuring the diode voltage at two currents I_1, and I_2, where $I_1 = 10 \bullet I_2$),

Subtracting we get:

$$\Delta V_D = T(KELVIN) \bullet K_D \bullet \ln\frac{I_1}{I_S} - T(KELVIN) \bullet K_D \bullet \ln\frac{I_2}{I_S}$$

Combining like terms, then simplifying the natural log terms yields:

$$\Delta V_D = T(KELVIN) \bullet K_D \bullet \ln(10)$$

and redefining constant

$$K'_D = K_D \bullet \ln(10) = 198\mu V/k$$

yields

$$\Delta V_D = K'_D \bullet T(KELVIN)$$

Solving for temperature:

$$T(KELVIN) = \frac{\Delta V_D}{K'_D},$$

$$T(KELVIN) = [°C] + 273.15,$$

$$[°C] = T(KELVIN) - 273.15$$

means that is we take the difference in voltage across the diode measured at two currents with a ratio of 10, the resulting voltage is 198µV per Kelvin of the junction with a zero intercept at 0 Kelvin.

The diode connected PNP transistor can be pulled up to V_{IN} with a resistor to set the current to 100µA for using this diode connected transistor as a general temperature monitor by monitoring the diode voltage drop with temperature, or a specific temperature monitor can be used that injects two currents that are at a 10:1 ratio for very accurate temperature monitoring. See Figure 24 for an example.

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Thermal Considerations and Output Current Derating

The thermal resistances reported in the Pin Configuration section of the data sheet are consistent with those parameters defined by JESD 51-12 and are intended for use with finite element analysis (FEA) software modeling tools that leverage the outcome of thermal modeling, simulation, and correlation to hardware evaluation performed on a µModule package mounted to a hardware test board defined by JESD 51-9 ("Test Boards for Area Array Surface Mount Package Thermal Measurements"). The motivation for providing these thermal coefficients is found in JESD 51-12 ("Guidelines for Reporting and Using Electronic Package Thermal Information").

Many designers may opt to use laboratory equipment and a test vehicle such as the demo board to anticipate the µModule regulator's thermal performance in their application at various electrical and environmental operating conditions to compliment any FEA activities. Without FEA software, the thermal resistances reported in the Pin Configuration section are in-and-of themselves not relevant to providing guidance of thermal performance; instead, the derating curves provided in the data sheet can be used in a manner that yields insight and guidance pertaining to one's application-usage, and can be adapted to correlate thermal performance to one's own application.

The Pin Configuration section gives four thermal coefficients explicitly defined in JESD 51-12; these coefficients are quoted or paraphrased below:

1. θ_{JA}, the thermal resistance from junction to ambient, is the natural convection junction-to-ambient air thermal resistance measured in a one cubic foot sealed enclosure. This environment is sometimes referred to as "still air" although natural convection causes the air to move. This value is determined with the part mounted to a JESD 51-9 defined test board, which does not reflect an actual application or viable operating condition.
2. $\theta_{JCbottom}$, the thermal resistance from junction to the bottom of the product case, is determined with all of the component power dissipation flowing through the bottom of the package. In the typical µModule, the bulk of the heat flows out the bottom of the package, but there is always heat flow out into the ambient environment. As a result, this thermal resistance value may be useful for comparing packages but the test conditions don't generally match the user's application.
3. θ_{JCtop}, the thermal resistance from junction to top of the product case, is determined with nearly all of the component power dissipation flowing through the top of the package. As the electrical connections of the typical µModule are on the bottom of the package, it is rare for an application to operate such that most of the heat flows from the junction to the top of the part. As in the case of $\theta_{JCbottom}$, this value may be useful for comparing packages but the test conditions don't generally match the user's application.
4. θ_{JB}, the thermal resistance from junction to the printed circuit board, is the junction-to-board thermal resistance where almost all of the heat flows through the bottom of the µModule and into the board, and is really the sum of the $\theta_{JCbottom}$ and the thermal resistance of the bottom of the part through the solder joints and through a portion of the board. The board temperature is measured a specified distance from the package, using a two sided, two layer board. This board is described in JESD 51-9.

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A graphical representation of the aforementioned thermal resistances is given in Figure 9; blue resistances are contained within the µModule regulator, whereas green resistances are external to the µModule package.

As a practical matter, it should be clear to the reader that no individual or sub-group of the four thermal resistance parameters defined by JESD 51-12 or provided in the Pin Configuration section replicates or conveys normal operating conditions of a µModule regulator. For example, in normal board-mounted applications, never does 100% of the device's total power loss (heat) thermally conduct exclusively through the top or exclusively through bottom of the µModule package—as the standard defines for θ_{JCtop} and $\theta_{JCbottom}$, respectively. In practice, power loss is thermally dissipated in both directions away from the package—granted, in the absence of a heat sink and airflow, a majority of the heat flow is into the board.

Within the LTM4620, be aware there are multiple power devices and components dissipating power, with a consequence that the thermal resistances relative to different junctions of components or die are not exactly linear with respect to total package power loss. To reconcile this complication without sacrificing modeling simplicity—but also, not ignoring practical realities—an approach has been taken using FEA software modeling along with laboratory testing in a controlled-environment chamber to reasonably define and correlate the thermal resistance values supplied in this data sheet: (1) Initially, FEA software is used to accurately build the mechanical geometry of the LTM4620 and the specified PCB with all of the correct material coefficients along with accurate power loss source definitions; (2) this model simulates a software-defined JEDEC environment consistent with JESD 51-12 to predict power loss heat flow and temperature readings at different interfaces that enable the calculation of the JEDEC-defined thermal resistance values; (3) the model and FEA software is used to evaluate the LTM4620 with heat sink and airflow; (4) having solved for and analyzed these thermal resistance values and simulated various operating conditions in the software model, a thorough laboratory evaluation replicates the simulated conditions with thermocouples within a controlled-environment chamber while operating the device at the same power loss as that which was simulated. An outcome of this process and due diligence yields a set of derating curves provided in other sections of this data sheet. After these laboratory tests have been performed, then the θ_{JB} and θ_{BA} are summed together to correlate quite well with the LTM4620 model with no airflow or heat sinking in a properly define chamber. This $\theta_{JB} + \theta_{BA}$ value is shown in the Pin Configuration section and should accurately equal the θ_{JA} value because approximately 100% of power loss flows from the junction through the board into ambient with no airflow or top mounted heat sink. Each system has its own thermal characteristics, therefore thermal analysis must be performed by the user in a particular system.

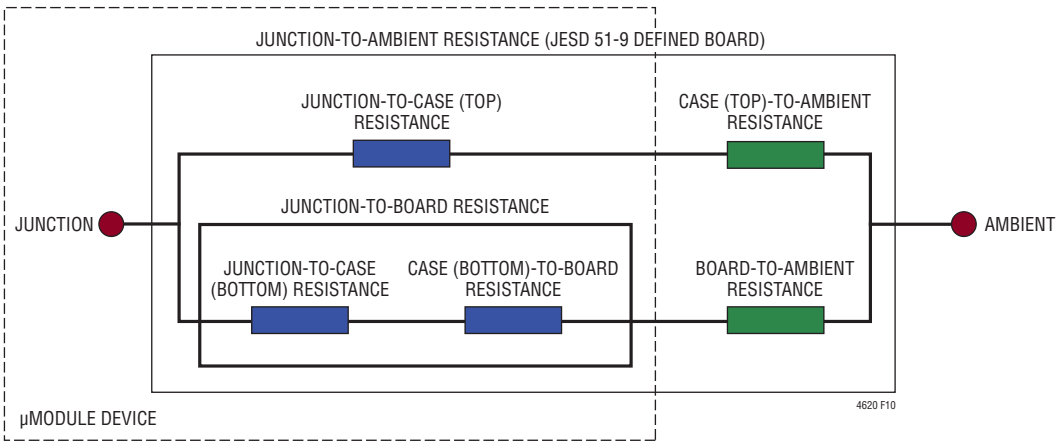

Figure 9. Graphical Representation of JESD51-12 Thermal Coefficients

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The LTM4620 has been designed to effectively remove heat from both the top and bottom of the package. The bottom substrate material has very low thermal resistance to the printed circuit board and the exposed top metal is thermally connected to the power devices and the power inductors. An external heat sink can be applied to the top of the device for excellent heat sinking with airflow. Basically all power dissipating devices are mounted directly to the substrate and the top exposed metal. This provides two low thermal resistance paths to remove heat.

Figure 10 shows a modeled temperature plot of the LTM4620 with BGA heat sink and 200LFM airflow with 4.7W of internal dissipation.

Figure 11 shows a modeled temperature plot of the LTM4620 with no heat sink and 200LFM airflow with 4.7W of internal dissipation.

These plots equate to a paralleled 1.2V at 26A design operating at 86% efficiency.

Safety Considerations

The LTM4620 modules do not provide isolation from V_{IN} to V_{OUT}. There is no internal fuse. If required, a slow blow fuse with a rating twice the maximum input current needs to be provided to protect each unit from catastrophic failure.

The fuse or circuit breaker should be selected to limit the current to the regulator during overvoltage in case of an internal top MOSFET fault. If the internal top MOSFET fails, then turning it off will not resolve the overvoltage, thus the internal bottom MOSFET will turn on indefinitely trying to protect the load. Under this fault condition, the input voltage will source very large currents to ground through the failed internal top MOSFET and enabled internal bottom MOSFET. This can cause excessive heat and board damage depending on how much power the input voltage can deliver to this system. A fuse or circuit breaker can be used as a secondary fault protector in this situation.

The device does support over current protection. A temperature diode is provided for monitoring internal temperature, and can be used to detect the need for thermal shutdown that can be done by controlling the RUN pin.

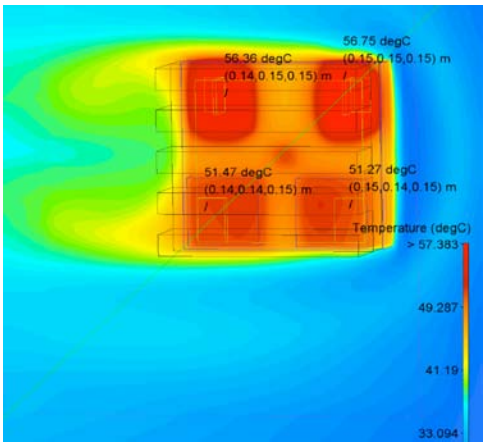

Figure 10. LTM4620 12V to 1.2V at 26A with 200LFM, External Heat Sink

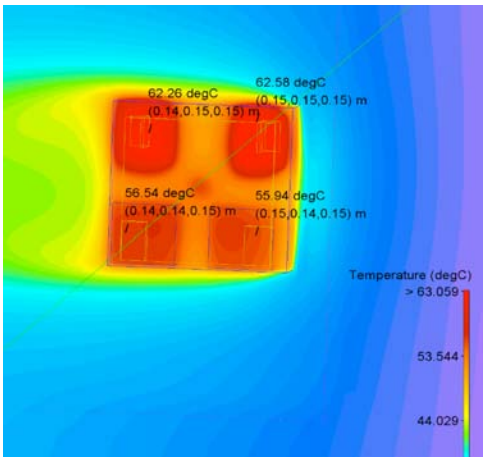

Figure 11. LTM4620 12V to 1.2V at 26A with 200LFM, No External Heat Sink

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Power Derating

The 1.0V and 2.5V power loss curves in Figures 12 and 13 can be used in coordination with the load current derating curves in Figures 14 to 21 for calculating an approximate Θ_{JA} thermal resistance for the LTM4620 with various heat sinking and airflow conditions. The power loss curves are taken at room temperature, and are increased with a 1.35 to 1.4 multiplicative factor at 125°C. These factors come from the fact that the power loss of the regulator increases about 45% from 25°C to 150°C, thus a 50% spread over 125°C delta equates to ~0.35%/°C loss increase. A 125°C maximum junction minus 25°C room temperature equates to a 100°C increase. This 100°C increase multiplied by 0.35%/°C equals a 35% power loss increase at the 125°C junction, thus the 1.35 multiplier.

The derating curves are plotted with V_{OUT1} and V_{OUT2} in parallel single output operation starting at 26A of load with low ambient temperature. The output voltages are 1.0V and 2.5V. These are chosen to include the lower and higher output voltage ranges for correlating the thermal resistance. Thermal models are derived from several temperature measurements in a controlled temperature chamber along with thermal modeling analysis.

The junction temperatures are monitored while ambient temperature is increased with and without airflow. The power loss increase with ambient temperature change is factored into the derating curves. The junctions are maintained at ~120°C maximum while lowering output current or power while increasing ambient temperature. The decreased output current will decrease the internal module loss as ambient temperature is increased.

The monitored junction temperature of 120°C minus the ambient operating temperature specifies how much temperature rise can be allowed. As an example in Figure 14, the load current is derated to ~19A at ~80°C with no air or heat sink and the power loss for the 12V to 1.0V at 19A output is a ~5.1W loss. The 5.1W loss is calculated with the ~3.75W room temperature loss from the 12V to 1.0V power loss curve at 19A, and the 1.35 multiplying factor at 125°C ambient. If the 80°C ambient temperature is subtracted from the 120°C junction temperature, then the difference of 40°C divided by 5.1W equals a 7.8°C/W Θ_{JA} thermal resistance. Table 2 specifies a 6.5 to 7°C/W value which is pretty close. The airflow graphs are more accurate due to the fact that the ambient temperature environment is controlled better with airflow. As an example in Figure 15, the load current is derated to ~22A at ~90°C with 200LFM of airflow and the power loss for the 12V to 1.0V at 22A output is a ~5.94W loss.

The 5.94W loss is calculated with the ~4.4W room temperature loss from the 12V to 1.0V power loss curve at 22A, and the 1.35 multiplying factor at 125°C ambient. If the 90°C ambient temperature is subtracted from the 120°C junction temperature, then the difference of 30°C divided by 5.94W equals a 5.1°C/W Θ_{JA} thermal resistance. Table 2 specifies a 5.5°C/W value which is pretty close. Tables 2 and 3 provide equivalent thermal resistances for 1.0V and 2.5V outputs with and without airflow and heat sinking.

The derived thermal resistances in Tables 2 and 3 for the various conditions can be multiplied by the calculated power loss as a function of ambient temperature to derive temperature rise above ambient, thus maximum junction temperature. Room temperature power loss can be derived from the efficiency curves and adjusted with the above ambient temperature multiplicative factors. The printed circuit board is a 1.6mm thick four layer board with two ounce copper for the two outer layers and one ounce copper for the two inner layers. The PCB dimensions are 101mm × 114mm. The BGA heat sinks are listed in Table 3.

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Table 2. 1.0V Output

DERATING CURVE	V_{IN} (V)	POWER LOSS CURVE	AIRFLOW (LFM)	HEAT SINK	Θ_{JA} (°C/W)
Figures 14, 15	5, 12	Figure 12	0	None	6.5 to 7
Figures 14, 15	5, 12	Figure 12	200	None	5.5
Figures 14, 15	5, 12	Figure 12	400	None	5
Figures 16, 17	5, 12	Figure 12	0	BGA Heat Sink	6.5
Figures 16, 17	5, 12	Figure 12	200	BGA Heat Sink	5
Figures 16, 17	5, 12	Figure 12	400	BGA Heat Sink	4

Table 3. 2.5V Output

DERATING CURVE	V_{IN} (V)	POWER LOSS CURVE	AIRFLOW (LFM)	HEAT SINK	Θ_{JA} (°C/W)
Figures 18, 19	5, 12	Figure 13	0	None	6.5 to 7
Figures 18, 19	5, 12	Figure 13	200	None	5.5 to 6
Figures 18, 19	5, 12	Figure 13	400	None	4.5
Figures 20, 21	5, 12	Figure 13	0	BGA Heat Sink	6.5 to 7
Figures 20, 21	5, 12	Figure 13	200	BGA Heat Sink	4
Figures 20, 21	5, 12	Figure 13	400	BGA Heat Sink	3.5

HEAT SINK MANUFACTURER	PART NUMBER	WEBSITE
Aavid Thermalloy	375424B00034G	www.aavid.com
Cool Innovations	4-050503P to 4-050508P	www.coolinnovations.com

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Table 4. Output Voltage Response vs Component Matrix (Refer to Figure 23) 0A to 7A Load Step Typical Measured Values

VENDORS	VALUE	PART NUMBER
TDK, C_{OUT1} Ceramic	100µF 6.3V	C4532X5R0J107MZ
Murata, C_{OUT1} Ceramic	100µF 6.3V	GRM32ER60J107M
AVX, C_{OUT1} Ceramic	100µF 6.3V	18126D107MAT
Sanyo POSCAP, C_{OUT2} Bulk	470µF 4V	4TPF470ML
Sanyo POSCAP, C_{OUT2} Bulk	470µF 6.3V	6TPD470M
Sanyo, C_{IN} Bulk	56µF 25V	25SVP56M

V_{OUT} (V)	C_{IN} (CERAMIC)	C_{IN} (BULK)**	C_{OUT1} (CERAMIC)	C_{OUT2} (BULK)	C_{FF} (pF)	C_{BOT} (pF)	C_{COMP} (pF)	V_{IN} (V)	DROOP (mV)	P-P DEVIATION AT 7A LOAD STEP (mV)	RECOVERY TIME (µs)	LOAD STEP (A/µs)	R_{FB} (kΩ)	FREQ
1	22µF × 3	56µF	100µF	470µF × 2	100	None	None	5	65	130	30	7	90.9	400
1	22µF × 3	56µF	100µF	470µF × 2	100	None	None	12	65	130	30	7	90.9	400
1	22µF × 3	56µF	100µF × 3	470µF × 2	100	None	None	5	60	120	30	7	90.9	400
1	22µF × 3	56µF	100µF × 3	470µF × 2	100	None	None	12	60	120	30	7	90.9	400
1.2	22µF × 3	56µF	100µF × 3	470µF × 2	100	None	None	5	65	130	30	7	60.4	500
1.2	22µF × 3	56µF	100µF × 3	470µF × 2	100	None	None	12	65	130	30	7	60.4	500
1.2	22µF × 3	56µF	100µF	470µF × 2	100	None	None	5	68	136	35	7	60.4	500
1.2	22µF × 3	56µF	100µF	470µF × 2	100	None	None	12	68	136	30	7	60.4	500
1.5	22µF × 3	56µF	100µF	470µF × 2	100	None	None	5	70	140	35	7	40.2	550
1.5	22µF × 3	56µF	100µF	470µF × 2	100	None	None	12	70	140	30	7	40.2	550
1.8	22µF × 3	56µF	100µF	470µF	100	None	None	5	75	150	30	7	30.2	600
1.8	22µF × 3	56µF	100µF	470µF	100	None	None	12	75	150	30	7	30.2	600
1.8	22µF × 3	56µF	100µF × 3	None	150	None	None	5	100	200	15	7	30.2	600
1.8	22µF × 3	56µF	100µF × 3	None	150	None	None	12	100	200	18	7	30.2	600
2.5	22µF × 3	56µF	100µF × 3	None	220	None	None	5	100	200	20	7	19.1	750
2.5	22µF × 3	56µF	100µF × 3	None	220	None	None	12	100	200	20	7	19.1	750
2.5	22µF × 3	56µF	100µF	470µF	150	None	None	5	85	170	30	7	19.1	750
2.5	22µF × 3	56µF	100µF	470µF	150	None	None	12	85	170	30	7	19.1	750

**Bulk capacitance is optional if V_{IN} has very low input impedance.

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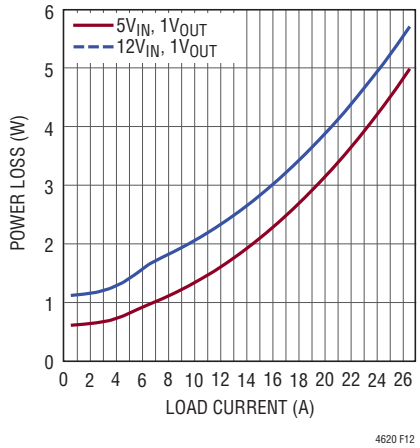

Figure 12. 1.0V Power Loss Curve

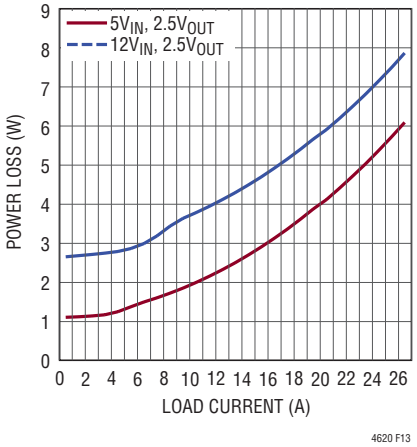

Figure 13. 2.5V Power Loss Curve

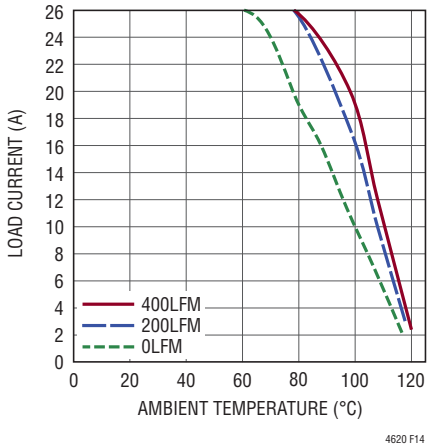

Figure 14. 12V to 1V Derating Curve, No Heat Sink

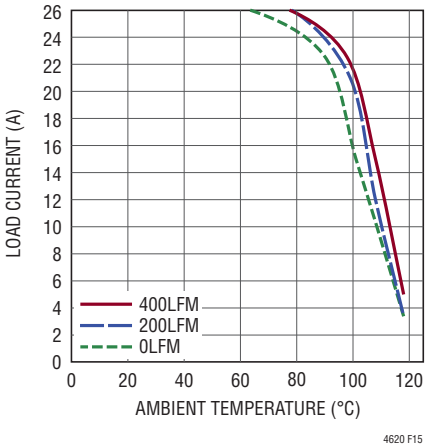

Figure 15. 5V to 1V Derating Curve, No Heat Sink

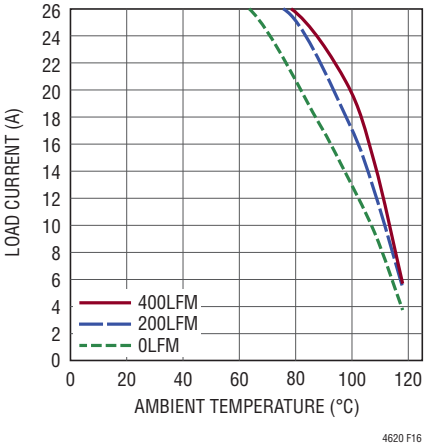

Figure 16. 12V to 1V Derating Curve, BGA Heat Sink

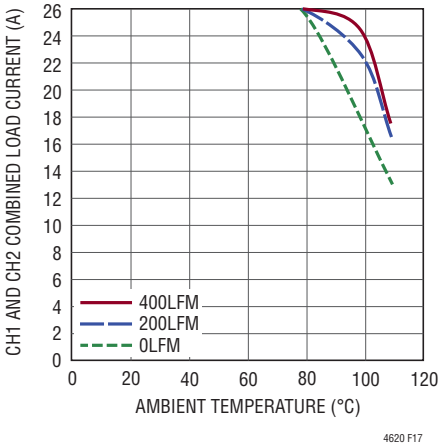

Figure 17. 5V to 1V Derating Curve, BGA Heat Sink

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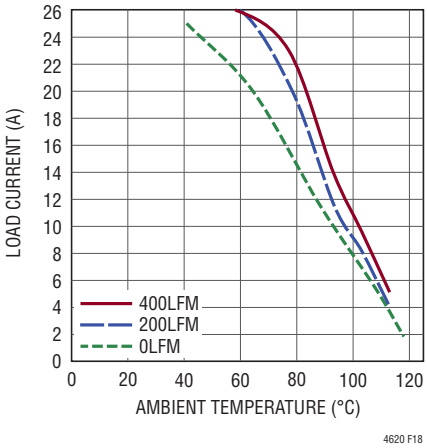


Figure 18. 12V to 2.5V Derating Curve, No Heat Sink

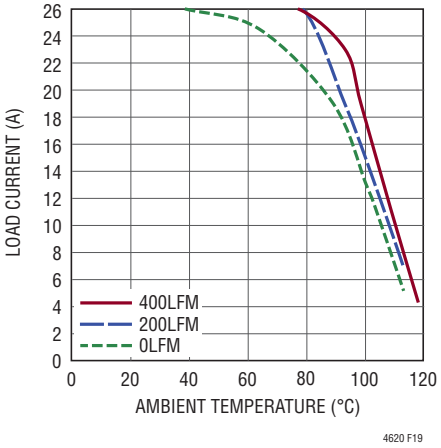


Figure 19. 5V to 2.5V Derating Curve, No Heat Sink

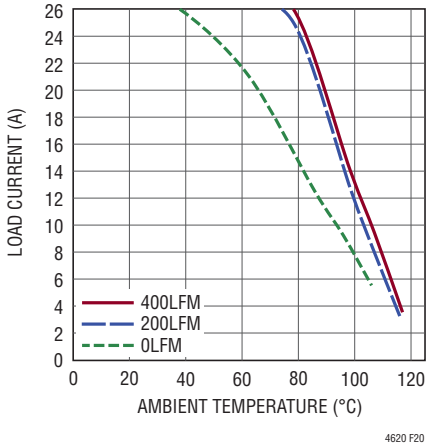


Figure 20. 12V to 2.5V Derating Curve, BGA Heat Sink

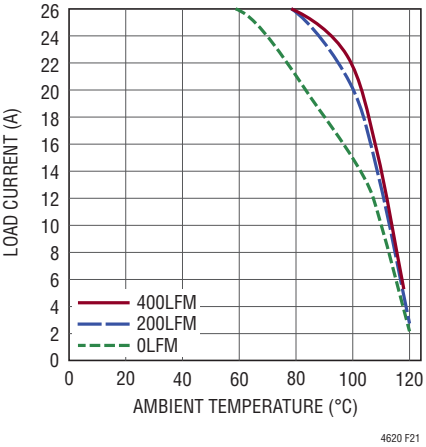


Figure 21. 5V to 2.5V Derating Curve, BGA Heat Sink

APPLICATIONS INFORMATION

Layout Checklist/Example

The high integration of LTM4620 makes the PCB board layout very simple and easy. However, to optimize its electrical and thermal performance, some layout considerations are still necessary.

- Use large PCB copper areas for high current paths, including V_{IN}, GND, V_{OUT1} and V_{OUT2}. It helps to minimize the PCB conduction loss and thermal stress.
- Place high frequency ceramic input and output capacitors next to the V_{IN}, PGND and V_{OUT} pins to minimize high frequency noise.
- Place a dedicated power ground layer underneath the unit.
- To minimize the via conduction loss and reduce module thermal stress, use multiple vias for interconnection between top layer and other power layers.
- Do not put via directly on the pad, unless they are capped or plated over.
- Use a separated SGND ground copper area for components connected to signal pins. Connect the SGND to GND underneath the unit.
- For parallel modules, tie the V_{OUT}, V_{FB}, and COMP pins together. Use an internal layer to closely connect these pins together. The TRACK pin can be tied a common capacitor for regulator soft-start.
- Bring out test points on the signal pins for monitoring.

Figure 22 gives a good example of the recommended layout.

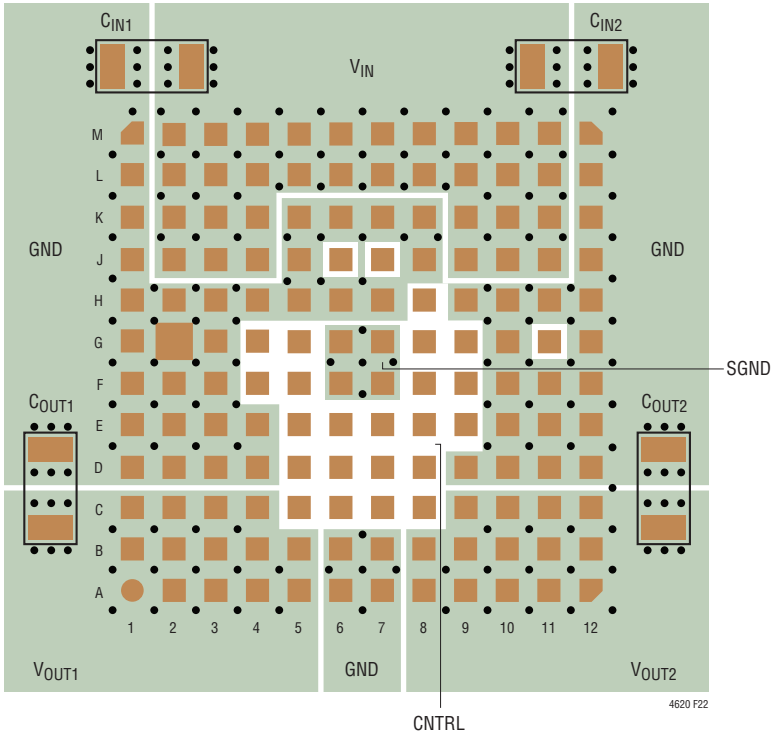


Figure 22. Recommended PCB Layout

TYPICAL APPLICATIONS

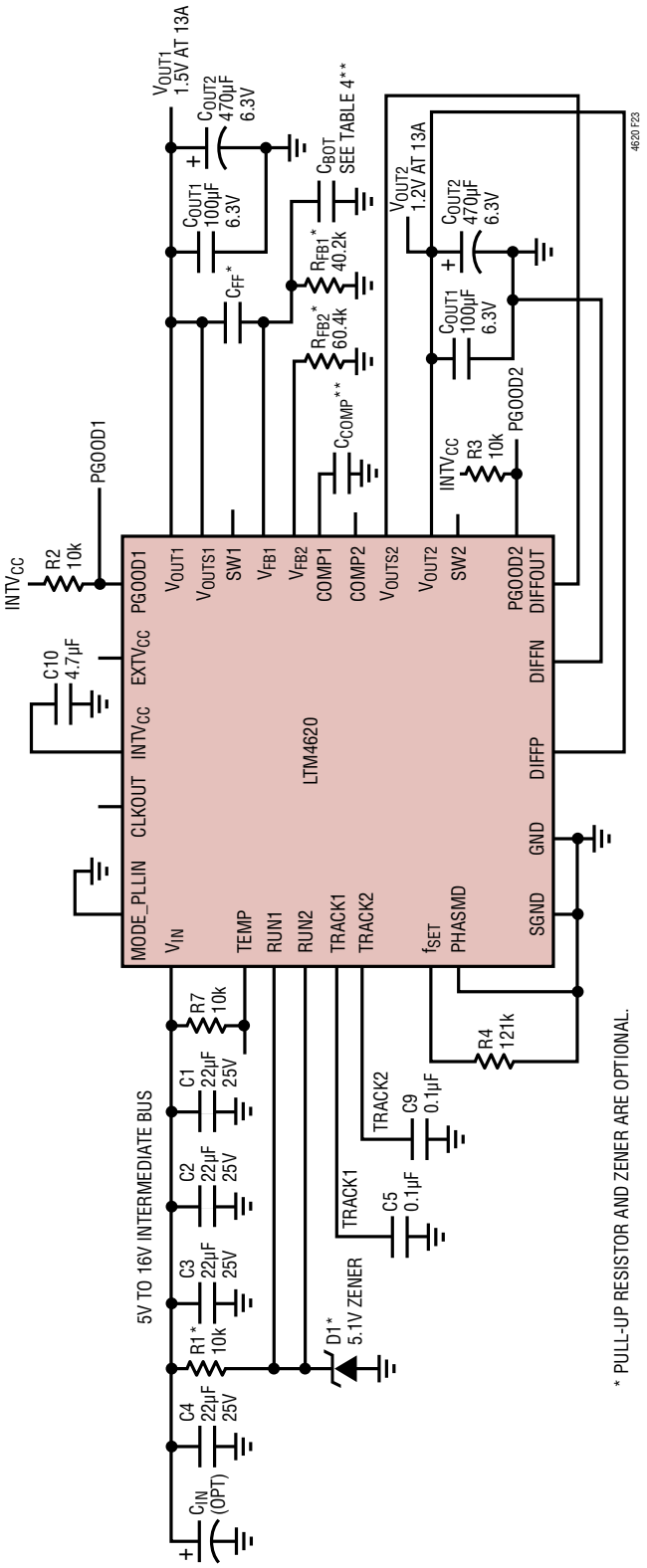


Figure 23. Typical $5V_{IN}$ to $16V_{IN}$, 1.5V and 1.2V Outputs

TYPICAL APPLICATIONS

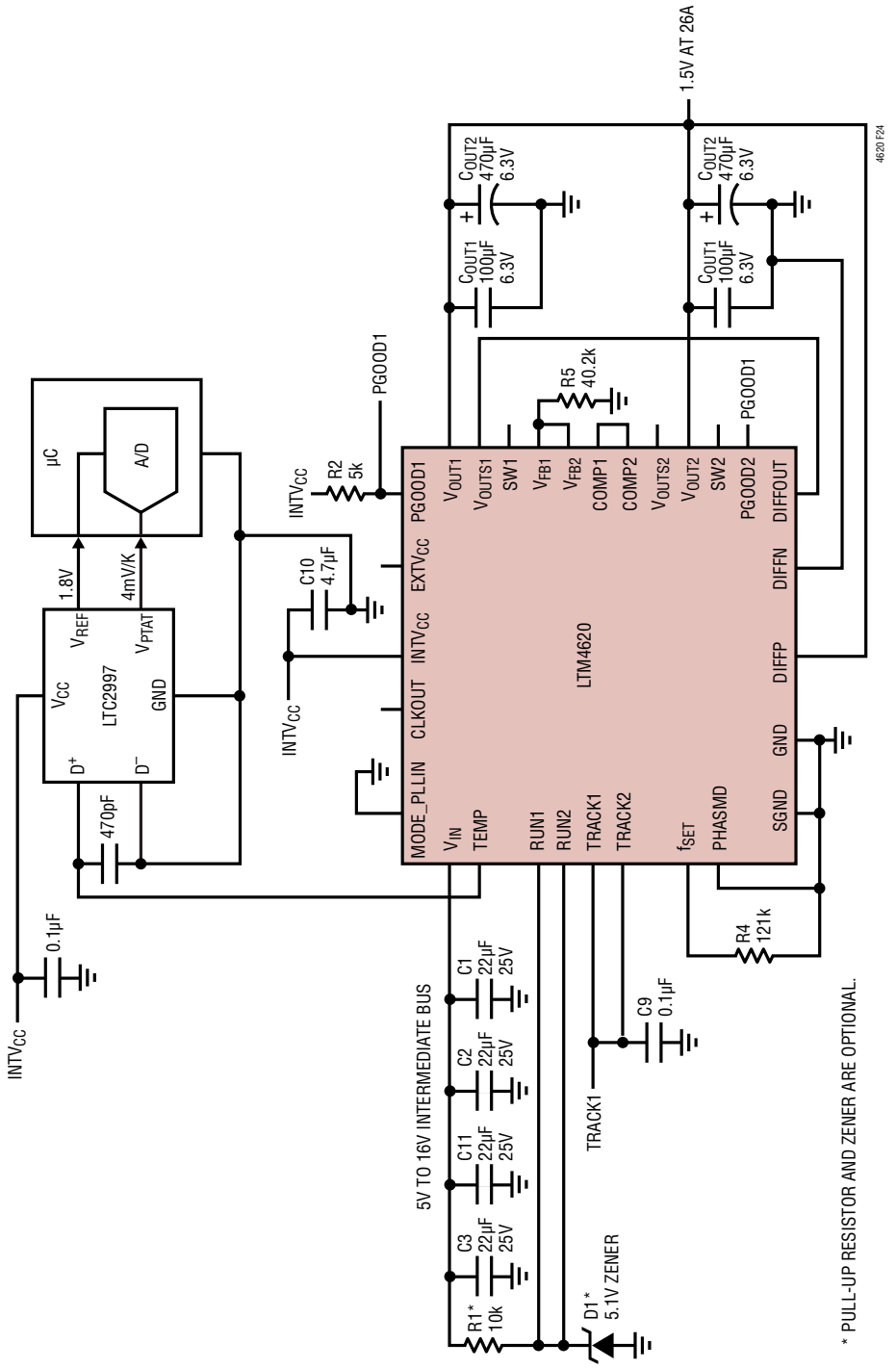


Figure 24. LTM4620 2-Phase, 1.5V at 26A Design with Temperature Monitoring

TYPICAL APPLICATIONS

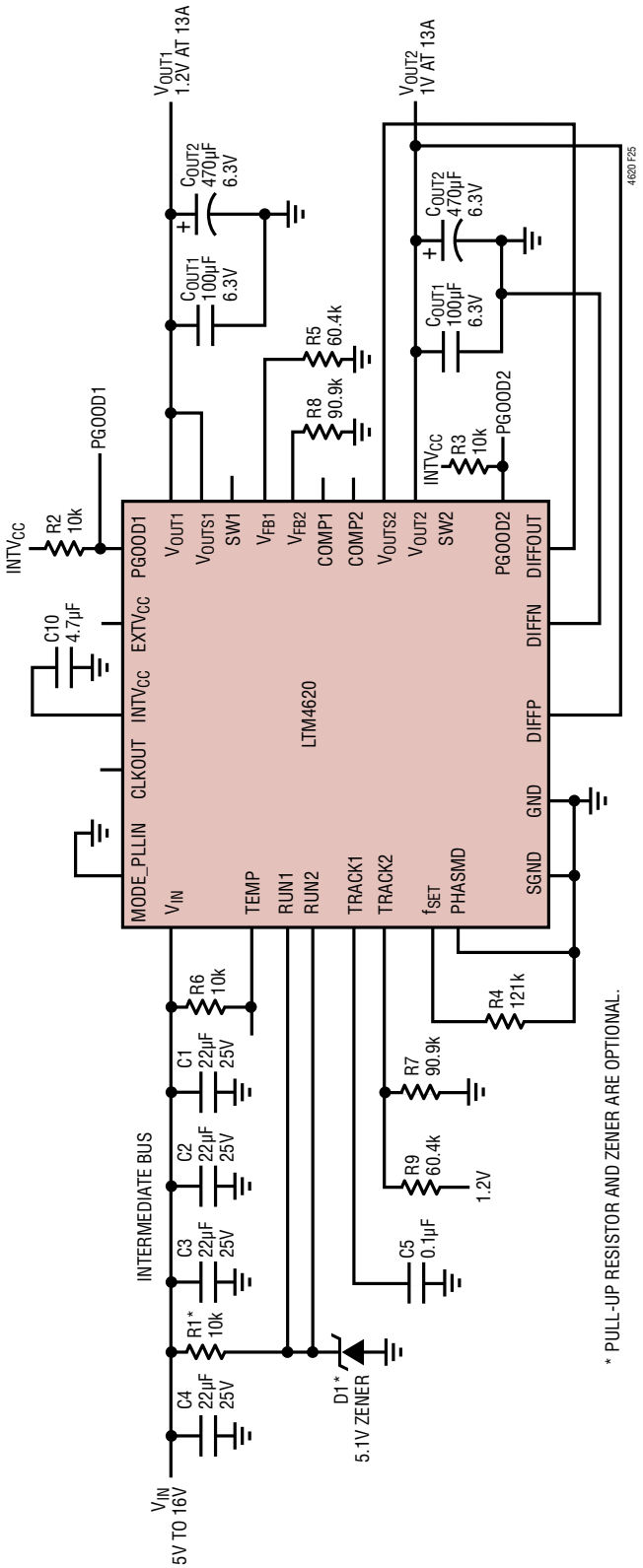


Figure 25. LTM4620 1.2V and 1V Output Tracking

TYPICAL APPLICATIONS

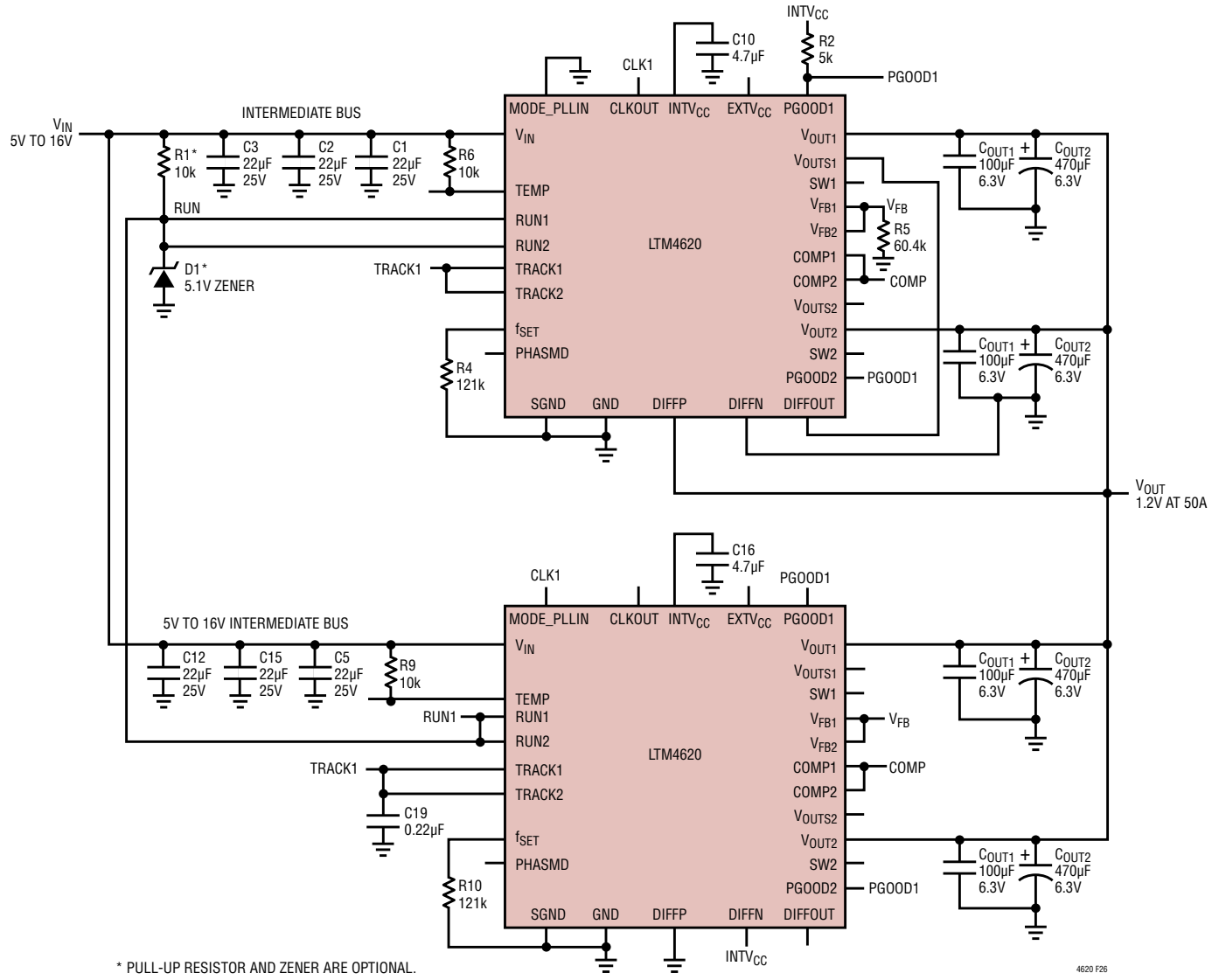


Figure 26. 4-Phase, 1.2V at 50A

PACKAGE DESCRIPTION

LTM4620 Component LGA Pinout

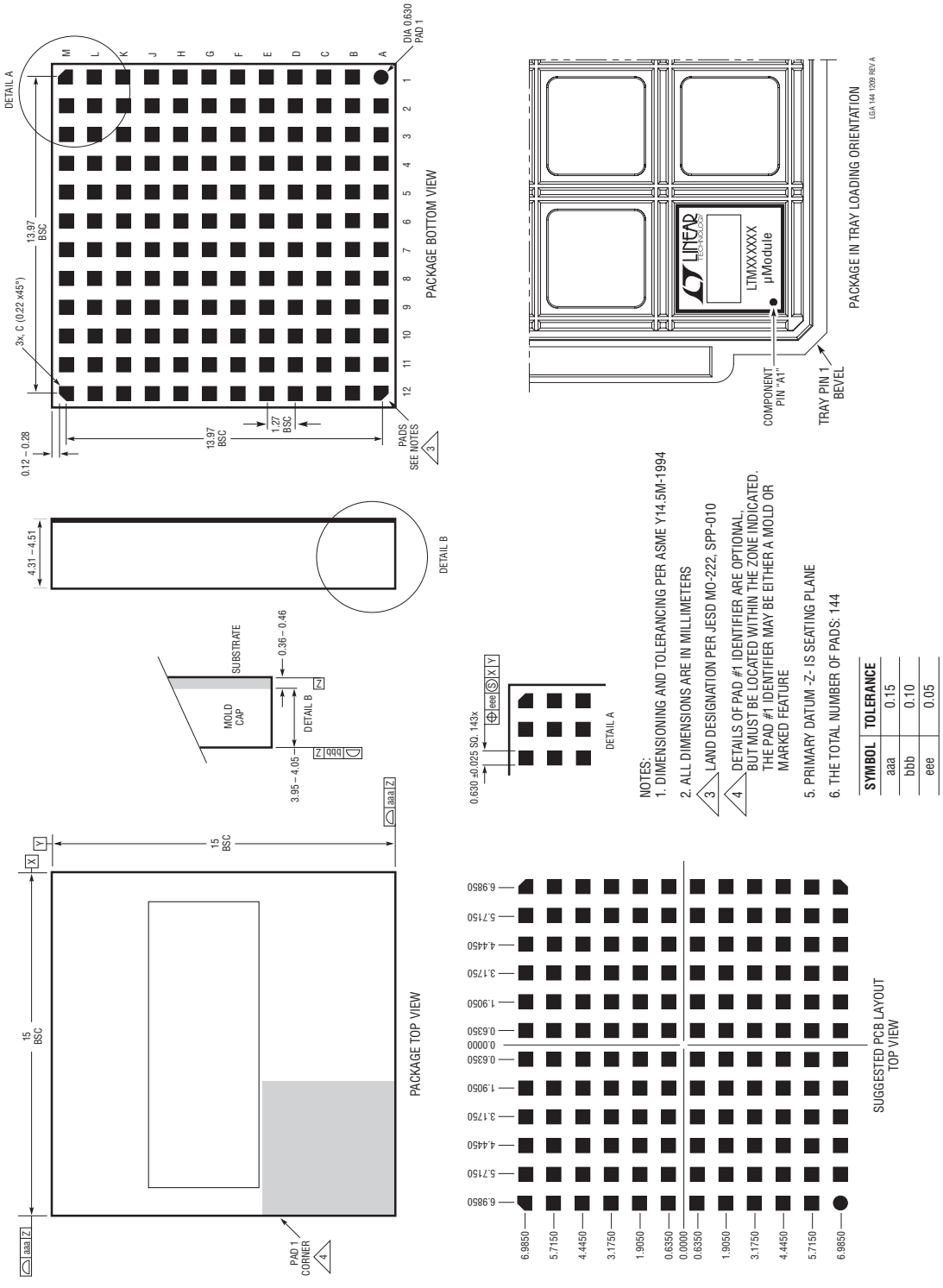
PIN ID	FUNCTION	PIN ID	FUNCTION	PIN ID	FUNCTION	PIN ID	FUNCTION	PIN ID	FUNCTION	PIN ID	FUNCTION
A1	VOUT1	B1	VOUT1	C1	VOUT1	D1	GND	E1	GND	F1	GND
A2	VOUT1	B2	VOUT1	C2	VOUT1	D2	GND	E2	GND	F2	GND
A3	VOUT1	B3	VOUT1	C3	VOUT1	D3	GND	E3	GND	F3	GND
A4	VOUT1	B4	VOUT1	C4	VOUT1	D4	GND	E4	GND	F4	MODE_PLLIN
A5	VOUT1	B5	VOUT1	C5	VOUT1S	D5	VFB1	E5	TRACK1	F5	RUN1
A6	GND	B6	GND	C6	f_{SET}	D6	SGND	E6	COMP1	F6	SGND
A7	GND	B7	GND	C7	SGND	D7	VFB2	E7	COMP2	F7	SGND
A8	VOUT2	B8	VOUT2	C8	VOUT2S	D8	TRACK2	E8	DIFFP	F8	DIFFOUT
A9	VOUT2	B9	VOUT2	C9	VOUT2	D9	GND	E9	DIFFN	F9	RUN2
A10	VOUT2	B10	VOUT2	C10	VOUT2	D10	GND	E10	GND	F10	GND
A11	VOUT2	B11	VOUT2	C11	VOUT2	D11	GND	E11	GND	F11	GND
A12	VOUT2	B12	VOUT2	C12	VOUT2	D12	GND	E12	GND	F12	GND

PIN ID	FUNCTION	PIN ID	FUNCTION	PIN ID	FUNCTION	PIN ID	FUNCTION	PIN ID	FUNCTION	PIN ID	FUNCTION
G1	GND	H1	GND	J1	GND	K1	GND	L1	GND	M1	GND
G2	SW1	H2	GND	J2	VIN	K2	VIN	L2	VIN	M2	VIN
G3	GND	H3	GND	J3	VIN	K3	VIN	L3	VIN	M3	VIN
G4	PHASMD	H4	GND	J4	VIN	K4	VIN	L4	VIN	M4	VIN
G5	CLKOUT	H5	GND	J5	GND	K5	GND	L5	VIN	M5	VIN
G6	SGND	H6	GND	J6	TEMP	K6	GND	L6	VIN	M6	VIN
G7	SGND	H7	GND	J7	EXTVCC	K7	GND	L7	VIN	M7	VIN
G8	PGOOD2	H8	INTVCC	J8	GND	K8	GND	L8	VIN	M8	VIN
G9	PGOOD1	H9	GND	J9	VIN	K9	VIN	L9	VIN	M9	VIN
G10	GND	H10	GND	J10	VIN	K10	VIN	L10	VIN	M10	VIN
G11	SW2	H11	GND	J11	VIN	K11	VIN	L11	VIN	M11	VIN
G12	GND	H12	GND	J12	GND	K12	GND	L12	GND	M12	GND

PACKAGE DESCRIPTION

Please refer to http://www.linear.com/designtools/packaging/ for the most recent package drawings.

LGA Package
144-Lead (15mm × 15mm × 4.41mm)
(Reference LTC DWG # 05-08-1844 Rev A)



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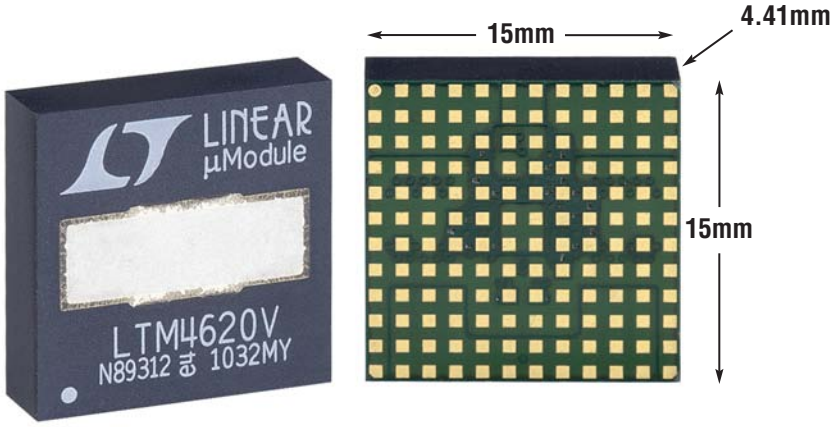
PACKAGE PHOTO



RELATED PARTS

PART NUMBER	DESCRIPTION	COMMENTS
LTM4628	Dual 8A, Single 16A µModule Regulator	Pin Compatible with LTM4620; 4.5V ≤ V_{IN} ≤ 26.5V, 0.6V ≤ V_{OUT} ≤ 5.5V, 15mm × 15mm × 4.32mm
LTM4627	15A µModule Regulator	4.5V ≤ V_{IN} ≤ 20V, 0.6V ≤ V_{OUT} ≤ 5.5V, 15mm × 15mm × 4.32mm
LTM4611	Ultralow V_{IN}, 15A µModule Regulator	1.5V ≤ V_{IN} ≤ 5.5V, 0.8V ≤ V_{OUT} ≤ 5V, 15mm × 15mm × 4.32mm
LTM4619	Dual 26V_{IN}, 4A DC/DC µModule Regulator	4.5V ≤ V_{IN} ≤ 26.5V; 0.8V ≤ V_{OUT} ≤ 5V
LTM4615	Triple Low V_{IN}, 4A DC/DC µModule Regulator	2.375 ≤ V_{IN} ≤ 5.5V; Two 4A and One 1.5A Output
LTM4616	Dual 8A, Low V_{IN}, DC/DC µModule Regulator	2.7V ≤ V_{IN} ≤ 5.5V; 0.6V ≤ V_{OUT} ≤ 5V
LTM4627	15A DC/DC µModule Regulator	4.5V ≤ V_{IN} ≤ 20V; 0.6V ≤ V_{OUT} ≤ 5V
LTM8062/ LTM8062A	32V_{IN}, 2A µModule Battery Charger with Maximum Peak Power Tracking (MPPT)	Adjustable V_{BATT} Up to 14.4V (18.8V for the LTM8062A), C/10 or Timer Termination, 9mm × 15mm × 4.32mm LGA Package
LTM8027	60V_{IN}, 4A DC/DC Step-Down µModule Regulator	4.5V ≤ V_{IN} ≤ 60V, 2.5V ≤ V_{OUT} ≤ 24V, 15mm × 15mm × 4.32mm LGA Package
LTM4613	EN55022B Compliant 36V_{IN}, 8A Step-Down µModule Regulator	5V ≤ V_{IN} ≤ 36V, 3.3V ≤ V_{OUT} ≤ 15V, Synchronizable, Parallelable, 15mm × 15mm × 4.32mm LGA Package

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