TPS65262-2 4.5-V to 18-V Input Voltage, 3-A/1-A/1-A Output Current Triple Synchronous Step-Down Converter With Dual Adjustable 350-mA/150-mA LDOs

1 Features

- Operating input voltage range: 4.5 to 18 V
- Feedback reference voltage: 0.6 V ±1%
- Maximum continuous output current: 3 A/1 A/1 A
- Fixed 600-kHz switching frequency
- Integrated dual LDOs with input voltage range: 1.3 to 18 V and continuous output current: 350 mA/150 mA
- Programmable soft start time for Buck1
- Fixed 1-ms soft-start time for Buck2 and Buck3
- Internal loop compensation for Buck2 and Buck3
- Dedicated enable pins for each Buck
- Support pulse skipping mode (PSM) and forced continuous current mode (FCCM)
- Output voltage power-good indicator
- Thermal overloading protection
- 32-Pin VQFN (RHB) 5-mm × 5-mm package
- Overvoltage protection, overcurrent and short-circuit protection, and overtemperature protection

2 Applications

- DTV
- Set-top boxes
- Home gateway and access point networks
- Wireless routers
- Surveillance
- POS machine

3 Description

The TPS65262-2 is a monolithic triple synchronous step-down (buck) converter with 3-A/1-A/1-A output current. A wide 4.5- to 18-V input supply voltage range encompasses the most intermediate bus voltage operating off 5-, 9-, 12-, or 15-V power bus. The converter, with constant frequency peak current mode, is designed to simplify its application while giving designers options to optimize the system according to targeted applications. The device operates at 600-kHz fixed switching frequency. The loop compensations for buck 2 and buck3 have been integrated for less external components. The 180° out-of-phase operation between buck1 and buck2, 3 (buck2 and buck3 run in phase) minimizes the input filter requirements.

The TPS65262-2 operates in pulse skipping mode (PSM) with connecting MODE pin to GND and operates in force continuous current mode (FCC) with driving MODE pin to high or leaving float. PSM mode provides high efficiency by reducing switching losses at light load and FCC mode reduces noise susceptibility and RF interference.

Two low dropout voltage linear regulators (LDO) are also built in TPS65262-2 with input voltage range 1.3 to 18 V, continuous output current 350 mA/150 mA, independent enable and adjustable output voltage.

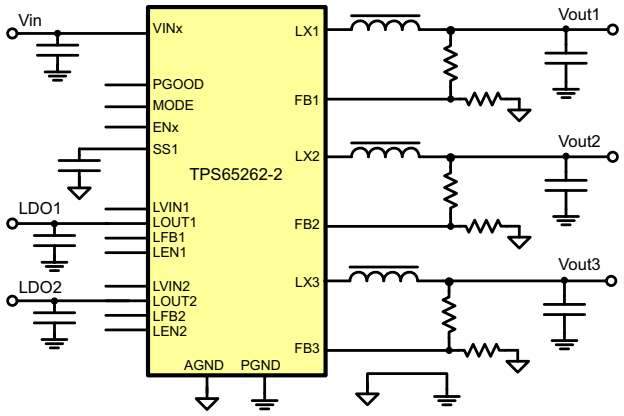
A power-good pin asserts when any output voltages are out of regulation.

Device Information(1)

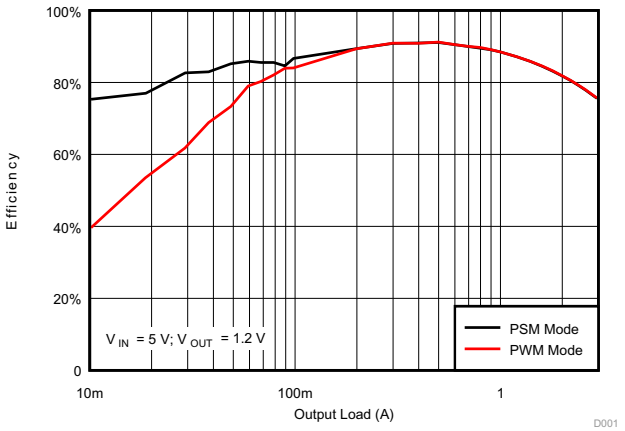
PART NUMBER	PACKAGE	BODY SIZE (NOM)
TPS65262-2	VQFN (32)	5.00 mm × 5.00 mm

(1) For all available packages, see the orderable addendum at the end of the data sheet.

Application Schematic



Efficiency vs Output Load



An IMPORTANT NOTICE at the end of this data sheet addresses availability, warranty, changes, use in safety-critical applications, intellectual property matters and other important disclaimers. PRODUCTION DATA.

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4 Revision History

NOTE: Page numbers for previous revisions may differ from page numbers in the current version.

Changes from Revision A (December 2015) to Revision B **Page**

- Added T_J = 25°C temperature condition for LDO1 current limit in the *Electrical Characteristics* ... 7
- Added T_J = 25°C temperature condition for LDO2 current limit in the *Electrical Characteristics* ... 7

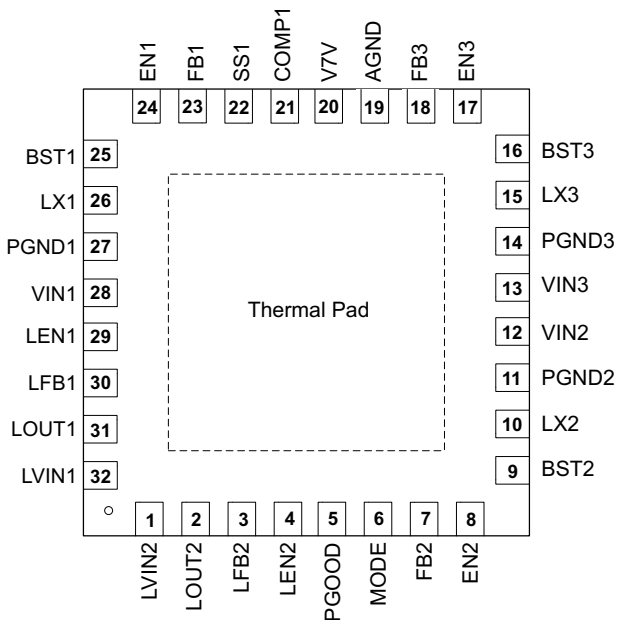
Changes from Original (December 2015) to Revision A **Page**

- Updated device status to production data ... 1

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5 Pin Configuration and Functions

32-Pin Plastic VQFN
RHB Package
Top View



(There is no electric signal down bonded to thermal pad inside IC. Exposed thermal pad must be soldered to PCB for optimal thermal performance.)

Pin Functions

PIN		DESCRIPTION
NAME	NO.	
LVIN2	1	Input power supply for LDO2. Connect LVIN2 pin as close as possible to the (+) terminal of an input ceramic capacitor (suggest 1 µF).
LOUT2	2	LDO2 output. Connect LOUT2 pin as close as possible to the (+) terminal of an output ceramic capacitor (suggest 1 µF).
LFB2	3	Feedback Kelvin sensing pin for LDO2 output voltage. Connect this pin to LDO2 resistor divider.
LEN2	4	Enable for LDO2. Float to enable.
PGOOD	5	An open-drain output, asserts low if output voltage of any buck is beyond regulation range due to thermal shutdown, overcurrent, undervoltage, or ENx shut down.
MODE	6	Switch FCC mode and PSM mode. Pull high or leave floating, FCC mode. Pull low, PSM mode.
FB2	7	Feedback Kelvin sensing pin for buck2 output voltage. Connect this pin to buck2 resistor divider.
EN2	8	Enable for buck2. Float to enable. Can use this pin to adjust the input undervoltage lockout of buck2 with a resistor divider.
BST2	9	Boot strapped supply to the high side floating gate driver in Buck2. Connect a capacitor (recommend 47 nF) from BST2 pin to LX2 pin.
LX2	10	Switching node connection to the inductor and bootstrap capacitor for Buck2. The voltage swing at this pin is from a diode voltage below the ground up to VIN2 voltage.
PGND2	11	Power ground connection of Buck2. Connect PGND2 pin as close as possible to the (–) terminal of VIN2 input ceramic capacitor.
VIN2	12	Input power supply for Buck2. Connect VIN2 pin as close as possible to the (+) terminal of an input ceramic capacitor (suggest 10 µF).
VIN3	13	Input power supply for Buck3. Connect VIN3 pin as close as possible to the (+) terminal of an input ceramic capacitor (suggest 10 µF).
PGND3	14	Power ground connection of Buck3. Connect PGND3 pin as close as possible to the (–) terminal of VIN3 input ceramic capacitor.
LX3	15	Switching node connection to the inductor and bootstrap capacitor for Buck3. The voltage swing at this pin is from a diode voltage below the ground up to VIN3 voltage.

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Pin Functions (continued)

PIN		DESCRIPTION
NAME	NO.	
BST3	16	Boot strapped supply to the high side floating gate driver in Buck3. Connect a capacitor (recommend 47 nF) from BST3 pin to LX3 pin.
EN3	17	Enable for Buck3. Float to enable. Can use this pin to adjust the input undervoltage lockout of Buck3 with a resistor divider.
FB3	18	Feedback Kelvin sensing pin for buck3 output voltage. Connect this pin to Buck3 resistor divider.
AGND	19	Analog ground common to buck controllers and other analog circuits. It must be routed separately from high current power grounds to the (-) terminal of bypass capacitor of input voltage VIN.
V7V	20	Internal LDO for gate driver and internal controller. Connect a 1-µF capacitor from the pin to power ground
COMP1	21	Error amplifier output and loop compensation pin for Buck1. Connect a series resistor and capacitor to compensate the control loop of buck1 with peak current PWM mode.
SS1	22	Soft-start and tracking input for Buck1. An internal 5-µA pullup current source is connected to this pin. The soft-start time can be programmed by connecting a capacitor between this pin and ground.
FB1	23	Feedback Kelvin sensing pin for Buck1 output voltage. Connect this pin to Buck1 resistor divider.
EN1	24	Enable for Buck1. Float to enable. Can use this pin to adjust the input undervoltage lockout of Buck1 with a resistor divider.
BST1	25	Boot strapped supply to the high side floating gate driver in buck1. Connect a capacitor (recommend 47 nF) from BST1 pin to LX1 pin.
LX1	26	Switching node connection to the inductor and bootstrap capacitor for buck1. The voltage swing at this pin is from a diode voltage below the ground up to VIN1 voltage.
PGND1	27	Power ground connection of buck1. Connect PGND1 pin as close as possible to the (–) terminal of VIN1 input ceramic capacitor.
VIN1	28	Input power supply for buck1. Connect VIN1 pin as close as possible to the (+) terminal of an input ceramic capacitor (suggest 10 µF).
LEN1	29	Enable for LDO1. Float to enable.
LFB1	30	Feedback Kelvin sensing pin for LDO1 output voltage. Connect this pin to LDO1 resistor divider.
LOUT1	31	LDO1 output. Connect LOUT1 pin as close as possible to the (+) terminal of an output ceramic capacitor (suggest 1 µF).
LVIN1	32	Input power supply for LDO1. Connect LVIN1 pin as close as possible to the (+) terminal of an input ceramic capacitor (suggest 1 µF).
PAD	—	There is no electric signal down bonded to thermal pad inside IC. Exposed thermal pad must be soldered to PCB for optimal thermal performance.

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6 Specifications

6.1 Absolute Maximum Ratings

over operating free-air temperature range (unless otherwise noted) (operating in a typical application circuit)(1)

		MIN	MAX	UNIT
Voltage	VIN1, VIN2, VIN3, LVIN1, LVIN2	–0.3	20	V
	LX1, LX2, LX3 (Maximum withstand voltage transient <20 ns)	–1.0	20	
	BST1, BST2, BST3 referenced to LX1, LX2, LX3 pins respectively	–0.3	7	
	MODE, LEN1, LEN2, EN1, EN2, EN3, PGOOD, V7V	–0.3	7	
	LOUT1, LOUT2	–0.3	7	
	FB1, FB2, FB3, LFB1, LFB2, COMP1 , SS1	–0.3	3.6	
	AGND, PGND1, PGND2, PGND3	–0.3	0.3	
T_J	Operating junction temperature	–40	125	°C
T_{stg}	Storage temperature	–55	150	°C

(1) Stresses beyond those listed under *Absolute Maximum Ratings* may cause permanent damage to the device. These are stress ratings only and functional operation of the device at these or any other conditions beyond those indicated under *recommended operating conditions* is not implied. Exposure to absolute-maximum-rated conditions for extended periods may affect device reliability.

6.2 ESD Ratings

			VALUE	UNIT
$V_{(ESD)}$	Electrostatic discharge	Human body model (HBM), per ANSI/ESDA/JEDEC JS-001, all pins(1)	±2000	V
		Charged device model (CDM), per JEDEC specification JESD22-C101, all pins(2)	±500	

(1) JEDEC document JEP155 states that 500-V HBM allows safe manufacturing with a standard ESD control process. *Pins listed as 1 kV may actually have higher performance.*
(2) JEDEC document JEP157 states that 250-V CDM allows safe manufacturing with a standard ESD control process. *Pins listed as 250 V may actually have higher performance.*

6.3 Recommended Operating Conditions

over operating free-air temperature range (unless otherwise noted)

		MIN	MAX	UNIT
Voltage	VIN1, VIN2, VIN3, LVIN1, LVIN2	4.5	18	V
	LX1, LX2, LX3 (maximum withstand voltage transient <20 ns)	–0.8	18	
	BST1, BST2, BST3 referenced to LX1, LX2, LX3 pins respectively	–0.1	6.8	
	MODE, LEN1, LEN2, EN1, EN2, EN3, PGOOD, V7V	–0.1	6.3	
	FB1, FB2, FB3, LFB1, LFB2, COMP1 , SS1	–0.1	3	
	LOUT1, LOUT2	–0.1	5.5	
T_J	Operating junction temperature	–40	125	°C

6.4 Thermal Information

THERMAL METRIC(1)		TPS65262-2 RHB (VQFN) 32 PINS	UNIT
$R_{\theta JA}$	Junction-to-ambient thermal resistance	32	°C/W
$R_{\theta JC(top)}$	Junction-to-case (top) thermal resistance	24.2	°C/W
$R_{\theta JB}$	Junction-to-board thermal resistance	6.4	°C/W
ψ_{JT}	Junction-to-top characterization parameter	0.2	°C/W
ψ_{JB}	Junction-to-board characterization parameter	6.4	°C/W
$R_{\theta Jc(bot)}$	Junction-to-case (bottom) thermal resistance	1.3	°C/W

(1) For more information about traditional and new thermal metrics, see the *Semiconductor and IC Package Thermal Metrics* application report, SPRA953.

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6.5 Electrical Characteristics

T_J = –40°C to 125°C, typical values are at T_J = 25°C (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
INPUT SUPPLY VOLTAGE						
VIN	Input voltage range		4.5		18	V
UVLO	VIN undervoltage lockout	VIN rising	4	4.25	4.5	V
		VIN falling	3.5	3.75	4	
		Hysteresis		500		mV
IDD_{SDN}	Shutdown supply current	EN1 = EN2 = EN3 = MODE = LEN1 = LEN2 = 0 V		12		µA
IDD_{Q_NSW}	Input quiescent current without buck1/2/3 switching	EN1 = EN2 = EN3 = 5V, FB1 = FB2 = FB3 = 0.8 V, LEN1 = LEN2 = 0 V		790		µA
IDD_{Q_NSW1}		EN1 = 5 V, EN2 = EN3 = 0 V, FB1 = 0.8 V, LEN1 = LEN2 = 0 V		340		µA
IDD_{Q_NSW2}		EN2 = 5 V, EN1 = EN3 = 0V, FB2 = 0.8 V, LEN1 = LEN2 = 0 V		370		µA
IDD_{Q_NSW3}		EN3 = 5 V, EN1 = EN2 = 0 V, FB3 = 0.8 V, LEN1 = LEN2 = 0 V		370		µA
IDD_{Q_LDO1}	LDO input quiescent current	EN1 = EN2 = EN3 = LEN2 = 0 V, LFB1 = 0.8 V, LEN1 = 5 V		190		µA
IDD_{Q_LDO2}		EN1 = EN2 = EN3 = LEN1 = 0 V, LFB2 = 0.8 V, LEN2 = 5 V		190		µA
V_{7V}	V7V LDO output voltage	VIN1 = 12 V; V7V load current = 0 A	6.0	6.3	6.6	V
I_{OCP_V7V}	V7V LDO current limit			175		mA
FEEDBACK VOLTAGE REFERENCE						
V_{FB}	Feedback voltage	V_{COMP} = 1.2 V, T_J = 25°C	0.595	0.6	0.605	V
		V_{COMP} = 1.2 V, T_J = –40°C to 125°C	0.594	0.6	0.606	V
$V_{LINEREG_Buck}$	Line regulation-DC (1)	I_{OUT1} = 1.5 A, I_{OUT2} = 1 A, I_{OUT3} = 1 A, 5 V < VINx < 18 V		0.002		%/V
$V_{LOADREG_Buck}$	Load regulation-DC (1)	V_{IN} = 12 V, I_{OUTx} = (10-100%) × I_{OUTx_max}		0.02		%/A
BUCK1, BUCK2, BUCK3						
V_{ENXH}	EN1/2/3 high level input voltage			1.2	1.27	V
V_{ENXL}	EN1/2/3 low level input voltage		1.0	1.15		V
I_{ENX}	EN1/2/3 pullup current	ENx = 1 V		3.6		µA
I_{ENX}	EN1/2/3 pullup current	ENx = 1.5 V		6.6		µA
I_{ENhys}	Hysteresis current			3		µA
I_{SS1}	Buck1 soft start charging current		4.3	5	6.1	µA
$T_{SS2/3}$	Buck2/3 soft start time			1		ms
T_{ON_MIN}	Minimum on time			80	100	ns
$G_{m_EA1/2/3}$	Error amplifier trans-conductance	–2 µA < I_{COMPX} < 2 µA		300		µS
$G_{m_PS1/2/3}$	COMP voltage to inductor current G_m (1)	I_{LX} = 0.5 A		7.4		A/V
I_{LIMIT1}	Buck1 peak inductor current limit		4.2	5.1	6	A
$I_{LIMITSOURCE1}$	Buck1 low-side source current limit			4.4		A
$I_{LIMITS1}$	Buck1 low-side sink current limit			1.3		A
$I_{LIMIT2/3}$	Buck2/3 peak inductor current limit		1.8	2.4	3	A
$I_{LIMITSOURCE2/3}$	Buck2/3 low-side source current limit			1.75		A
$I_{LIMITS2/3}$	Buck2/3 low-side sink current limit			1		A
t_{Hiccup_wait}	OC wait time (1)			0.5		ms
t_{Hiccup_re}	Hiccup time before restart (1)			14		ms
Rdson_HS1	Buck1 High-side switch resistance	VIN1 = 12 V		100		mΩ
Rdson_LS1	Buck1 low-side switch resistance	VIN1 = 12 V		65		mΩ
Rdson_HS2	Buck2 High-side switch resistance	VIN1 = 12 V		195		mΩ
Rdson_LS2	Buck2 low-side switch resistance	VIN1 = 12 V		145		mΩ
Rdson_HS3	Buck3 High-side switch resistance	VIN1 = 12 V		195		mΩ
Rdson_LS3	Buck3 low-side switch resistance	VIN1 = 12 V		145		mΩ

(1) Lab validation result.

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Electrical Characteristics (continued)

T_J = –40°C to 125°C, typical values are at T_J = 25°C (unless otherwise noted)

PARAMETER		TEST CONDITIONS	MIN	TYP	MAX	UNIT
POWER GOOD, MODE, POWER SEQUENCE						
V_{th_PG}	Feedback voltage threshold	FBx undervoltage falling		92.5%		V_{REF}
		FBx undervoltage rising		95%		
		FBx overvoltage rising		107.5%		
		FBx overvoltage falling		105%		
$t_{DEGLITCH(PG)_F}$	PGOOD falling edge deglitch time			0.19		ms
$t_{RDEGLITCH(PG)_R}$	PGOOD rising edge deglitch time			1		ms
I_{PG}	PGOOD pin leakage				0.05	µA
V_{LOW_PG}	PGOOD pin low voltage	I_{SINK} = 1 mA			0.4	V
V_{MODEH}	MODE high level input voltage			1.2	1.27	V
V_{MODEL}	MODE low level input voltage		1.0	1.15		V
I_{MODE}	MODE pullup current	MODE = 1 V		3.6		µA
I_{MODE}	MODE pullup current	MODE = 1.5 V		6.6		µA
LDO1 AND LDO2						
V_{LENXH}	LEN1, LEN2 high-level input voltage			1.2	1.27	V
V_{LENXL}	LEN1, LEN2 low-level input voltage		1.0	1.15		V
I_{LENX}	LEN1, LEN2 pullup current	LENx = 1 V		3.6		µA
		LENx = 1.5 V		6.6		
VIN_{LDO1}	LDO input voltage range		1.3		18	V
$VOUT_{LDO1}$	LDO output voltage range	load current = 350 mA, V_{IN} = 12 V	1		5.5	V
V_{LDOFB1}	LDO voltage reference	load current = 10 mA, V_{IN} = 12 V	0.593	0.6	0.607	V
I_{max_LDO1}	LDO current limit	T_J = 25°C	350	440	559	mA
$V_{dropout1}$	LDO dropout voltage	I_{OUT} = 20 mA		12		mV
		I_{OUT} = 200 mA		120		mV
$V_{LINEREG_LDO1}$	LDO line regulation-DC(1)	V_{OUT} = 1.8 V, I_{OUT} = 10 mA, LVIN1 changes from 2 to 18 V		0.002		%/V
$V_{LOADREG_LDO1}$	LDO load regulation-DC(1)	I_{OUT} = 1 mA to 350 mA		0.2		%/A
$PSRR_{LDO1}$	Ripple rejection(1)	Vin_LDO1 = 12 V, V_{OUT} = 1.8 V, I_{OUT} = 10 mA, f = 10 kHz		56		dB
VIN_{LDO2}	LDO input voltage range		1.3		18	V
$VOUT_{LDO2}$	LDO output voltage range	Load current = 150 mA, V_{IN} = 12 V	1		5.5	V
V_{LDOFB2}	LDO voltage reference	Load current = 10 mA, V_{IN} = 12 V	0.593	0.6	0.607	V
I_{max_LDO2}	LDO current limit	T_J = 25°C	160	230	295	mA
$V_{dropout2}$	LDO drop out voltage	I_{OUT} = 10 mA		12		mV
		I_{OUT} = 100 mA		120		mV
$V_{LINEREG_LDO2}$	LDO line regulation-DC(1)	V_{OUT} = 1.8 V, I_{OUT} = 10 mA, LVIN1 changes from 2 to 18 V		0.002		%/V
$V_{LOADREG_LDO2}$	LDO load regulation-DC(1)	I_{OUT} = 1 to 150 mA, V_{IN} = 12 V		0.2		%/A
$PSRR_{LDO2}$	Ripple rejection(1)	Vin_LDO2 = 12 V, V_{OUT} = 1.8 V, I_{OUT} = 10 mA, f = 10 kHz		56		dB
OSCILLATOR						
f_{SW}	Switching frequency		540	600	670	kHz
THERMAL PROTECTION						
T_{TRIP_OTP}	Thermal protection trip point(1)	Temperature rising		160		°C
T_{HYST_OTP}		Hysteresis		20		°C

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6.6 Typical Characteristics

T_A = 25°C, VIN = 12 V, VOUT1 = 1.2 V, VOUT2 = 1.8 V, VOUT3 = 3.3 V, f_{SW} = 600 kHz (unless otherwise noted)

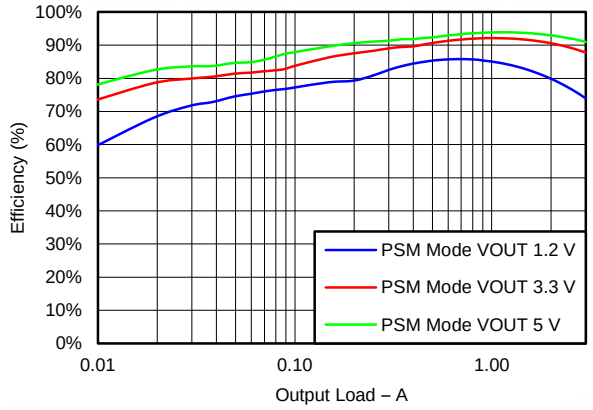


Figure 1. Buck1 Efficiency

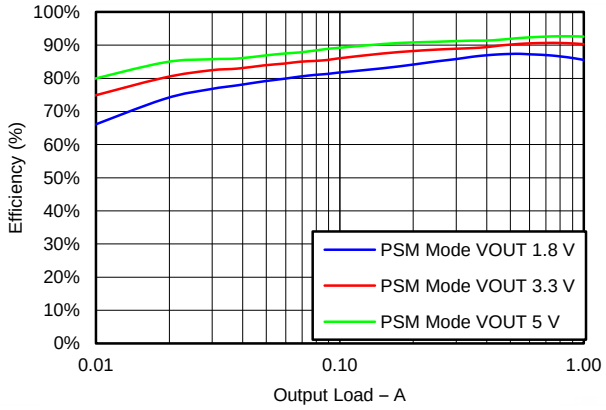


Figure 2. Buck2 Efficiency

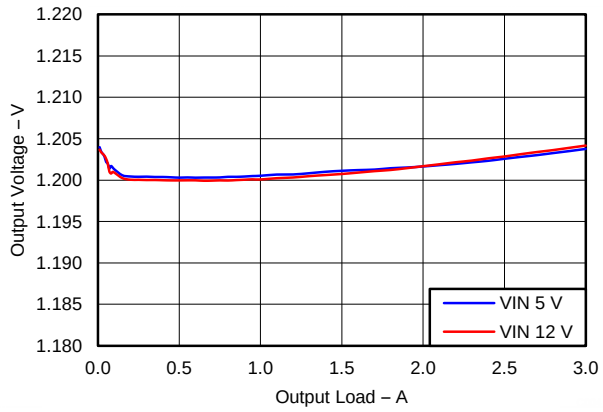


Figure 3. Buck1, PSM Mode Load Regulation

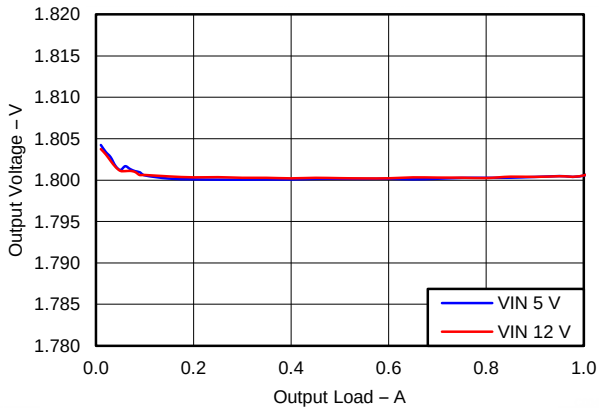


Figure 4. Buck2, PSM Mode Load Regulation

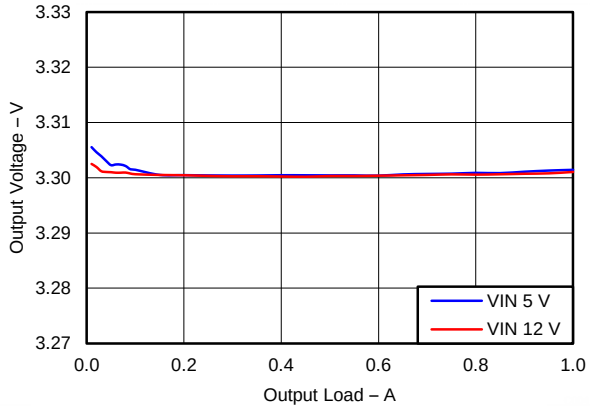


Figure 5. Buck3, PSM Mode Load Regulation

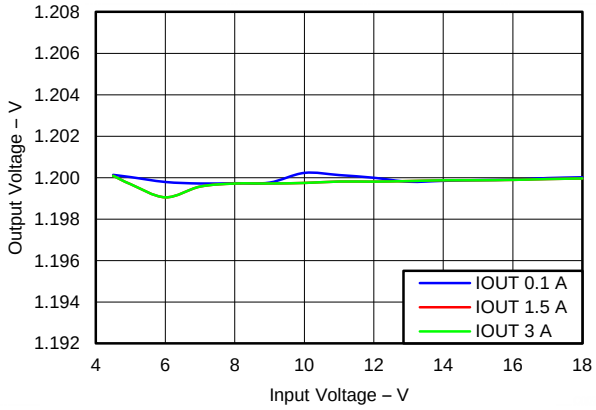


Figure 6. Buck1, PSM Mode Line Regulation

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Typical Characteristics (continued)

T_A = 25°C, VIN = 12 V, VOUT1 = 1.2 V, VOUT2 = 1.8 V, VOUT3 = 3.3 V, f_{SW} = 600 kHz (unless otherwise noted)

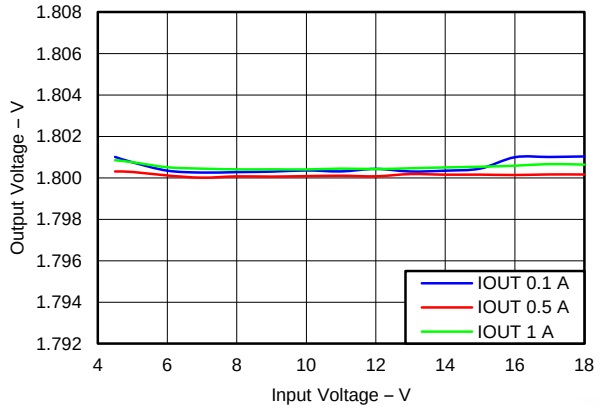


Figure 7. Buck2, PSM Mode Line Regulation

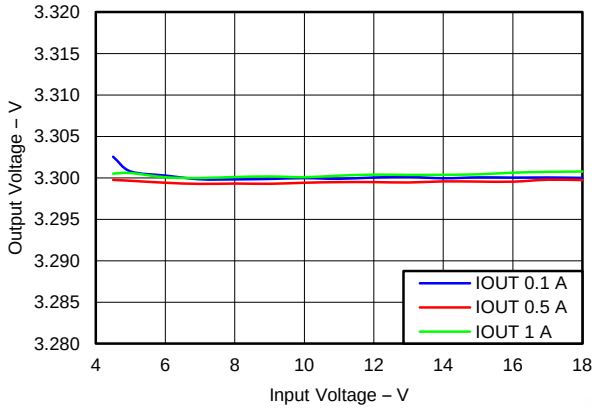


Figure 8. Buck3, PSM Mode Line Regulation

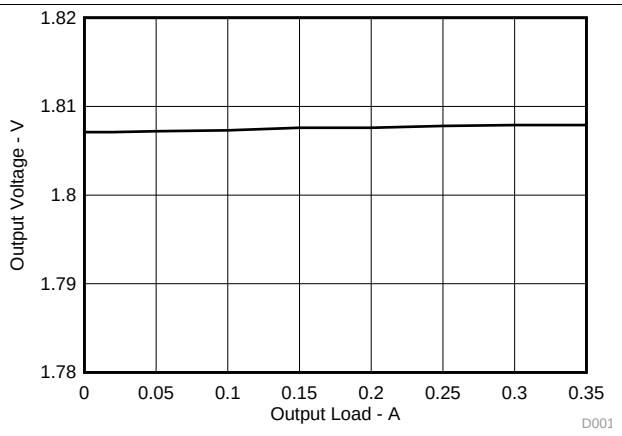


Figure 9. LDO1, Load Regulation, V_{IN} = 3.3 V

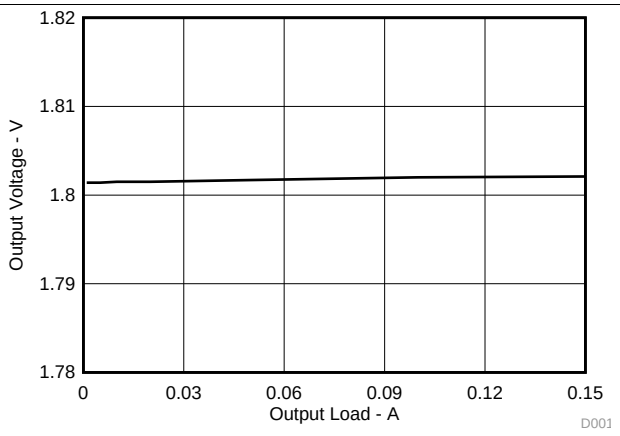


Figure 10. LDO2, Load Regulation, V_{IN} = 3.3 V

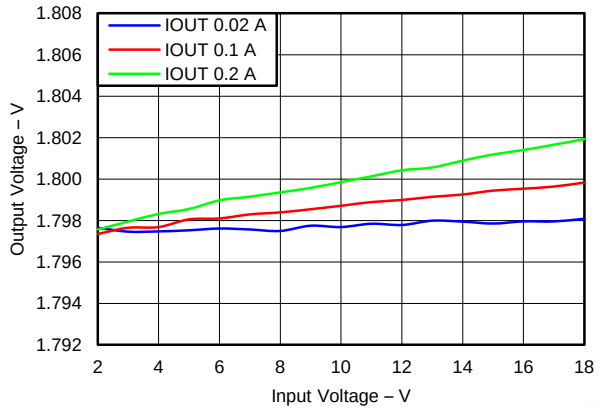


Figure 11. LDO1, Line Regulation

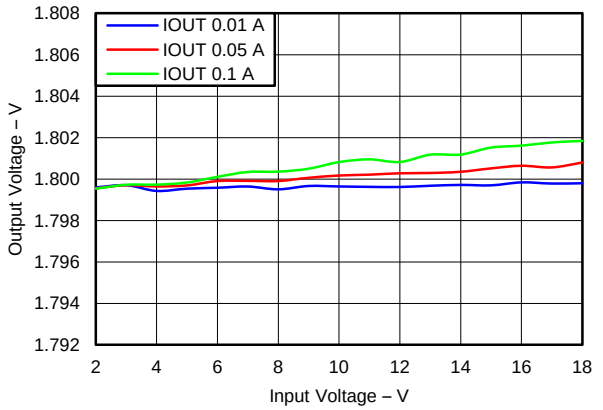


Figure 12. LDO2, Line Regulation

Typical Characteristics (continued)

T_A = 25°C, VIN = 12 V, VOUT1 = 1.2 V, VOUT2 = 1.8 V, VOUT3 = 3.3 V, f_{SW} = 600 kHz (unless otherwise noted)

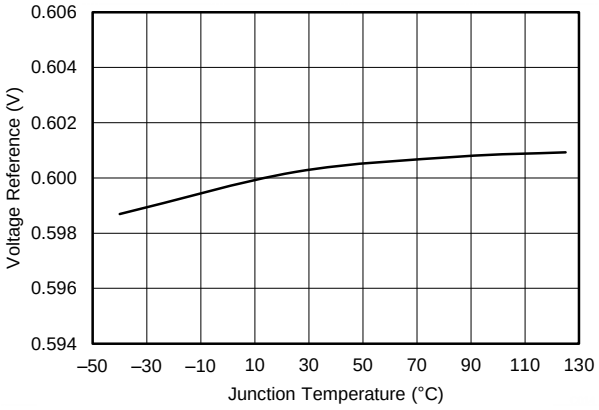


Figure 13. Voltage Reference vs Temperature

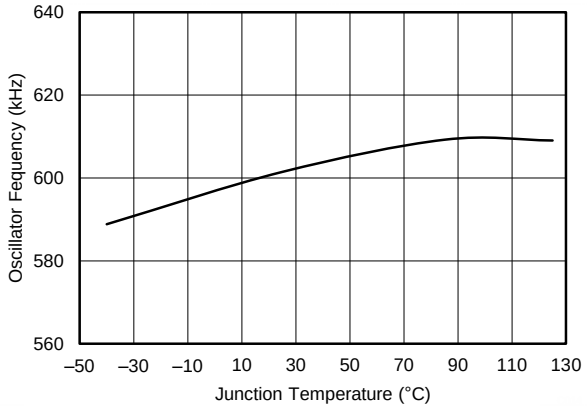


Figure 14. Oscillator Frequency vs Temperature

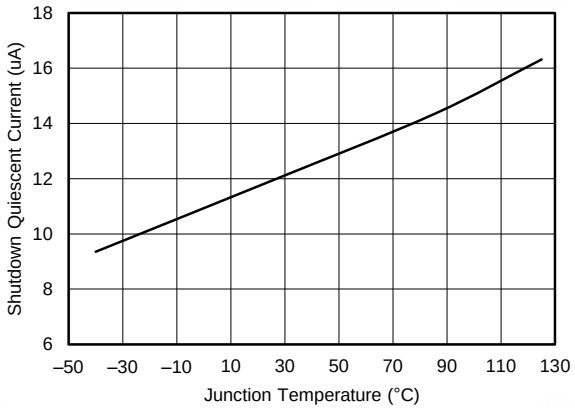


Figure 15. Shutdown Quiescent Current vs Temperature

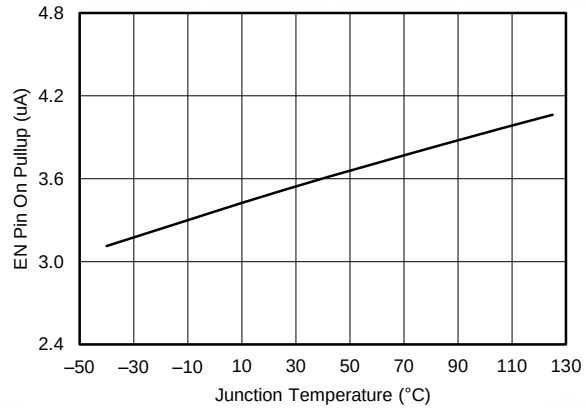


Figure 16. EN Pin Pullup Current vs Temperature, EN = 1 V

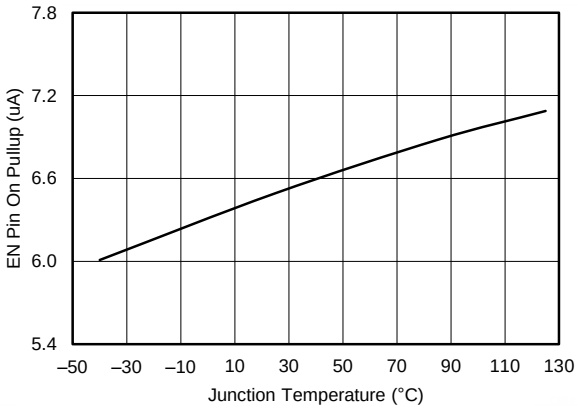


Figure 17. EN Pin Pullup Current vs Temperature, EN = 1.5 V

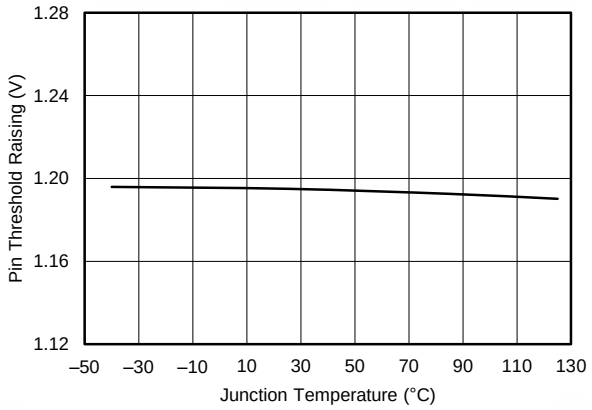


Figure 18. EN Pin Threshold Rising vs Temperature

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Typical Characteristics (continued)

T_A = 25°C, VIN = 12 V, VOUT1 = 1.2 V, VOUT2 = 1.8 V, VOUT3 = 3.3 V, f_{SW} = 600 kHz (unless otherwise noted)

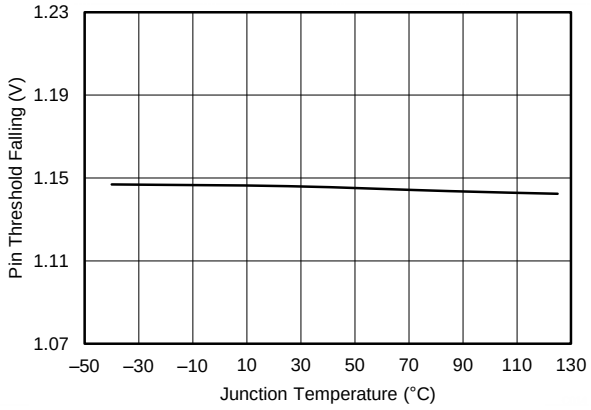


Figure 19. EN Pin Threshold Falling vs Temperature

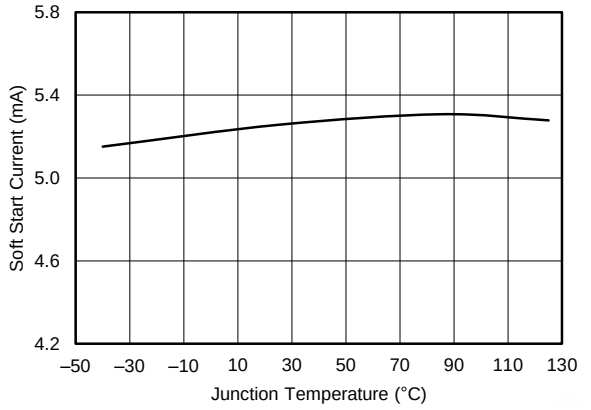


Figure 20. SS Pin Charge Current vs Temperature

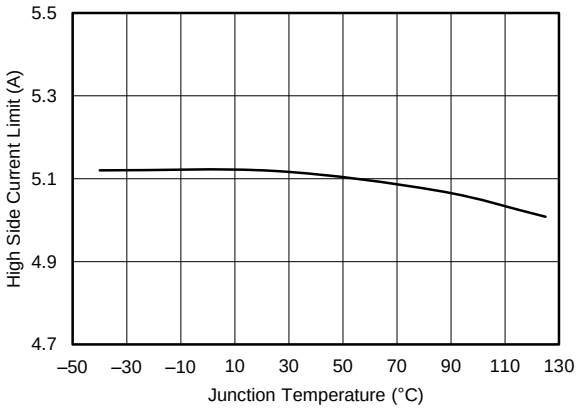


Figure 21. Buck1 High-Side Current Limit vs Temperature

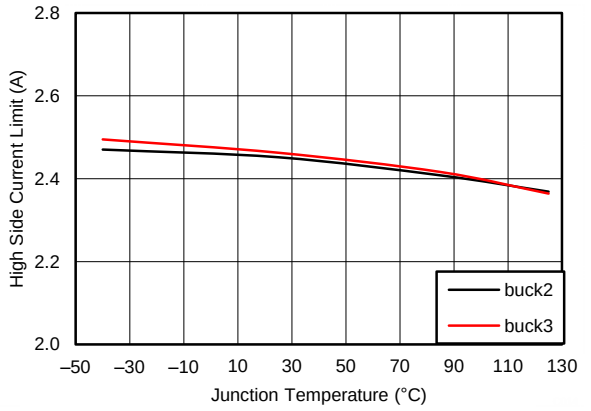


Figure 22. Buck2, 3 High-Side Current Limit vs Temperature

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7 Detailed Description

7.1 Overview

The TPS65262-2 is a monolithic triple synchronous step-down (buck) converter with 3-A/1-A/1-A output currents. A wide 4.5- to 18-V input supply voltage range encompasses most intermediate bus voltages operating off 5-, 9-, 12-, or 15-V power bus. The feedback voltage reference for each buck is 0.6V. Each buck is independent with dedicated enable, soft-start and loop compensation.

The TPS65262-2 implements a constant frequency, peak current mode control that simplifies external loop compensation. The switching frequency is fixed 600 kHz. The switching clock of buck1 is 180° out-of-phase operation from the clocks of buck2 and buck3 channels to reduce input current ripple, input capacitor size and power supply induced noise.

The TPS65262-2 has been designed for safe monotonic startup into pre-biased loads. The default start up is when VIN is typically 4.5 V. The ENx pin also can be used to adjust the input voltage undervoltage lockout (UVLO) with an external resistor divider. In addition, the ENx pin has an internal 3.6-µA current source, so the EN pin can be floating for automatically powering up the converters.

The TPS65262-2 reduces the external component count by integrating the bootstrap circuit. The bias voltage for the integrated high-side MOSFET is supplied by a capacitor between the BST and LX pins. A UVLO circuit monitors the bootstrap capacitor voltage VBST-VLX in each buck. When VBST-VLX voltage drops to the threshold, LX pin is pulled low to recharge the bootstrap capacitor. The TPS65262-2 can operate at 100% duty cycle as long as the bootstrap capacitor voltage is higher than the BOOT-LX UVLO threshold which is typically 2.1 V.

The TPS65262-2 features a PGOOD pin to supervise each output voltage of buck converters. The TPS65262-2 has power good comparators with hysteresis, which monitor the output voltages through feedback voltages. When all bucks are in regulation range and power sequence is done, PGOOD is asserted to high.

The SS (soft start/tracking) pin is used to minimize inrush currents during power up. A small value capacitor or resistor divider is coupled to the pin for soft start or voltage tracking.

The TPS65262-2 operates in pulse skipping mode (PSM) with connecting MODE pin to GND and operates in forced continuous current (FCC) mode with driving MODE pin to high or leaving float.

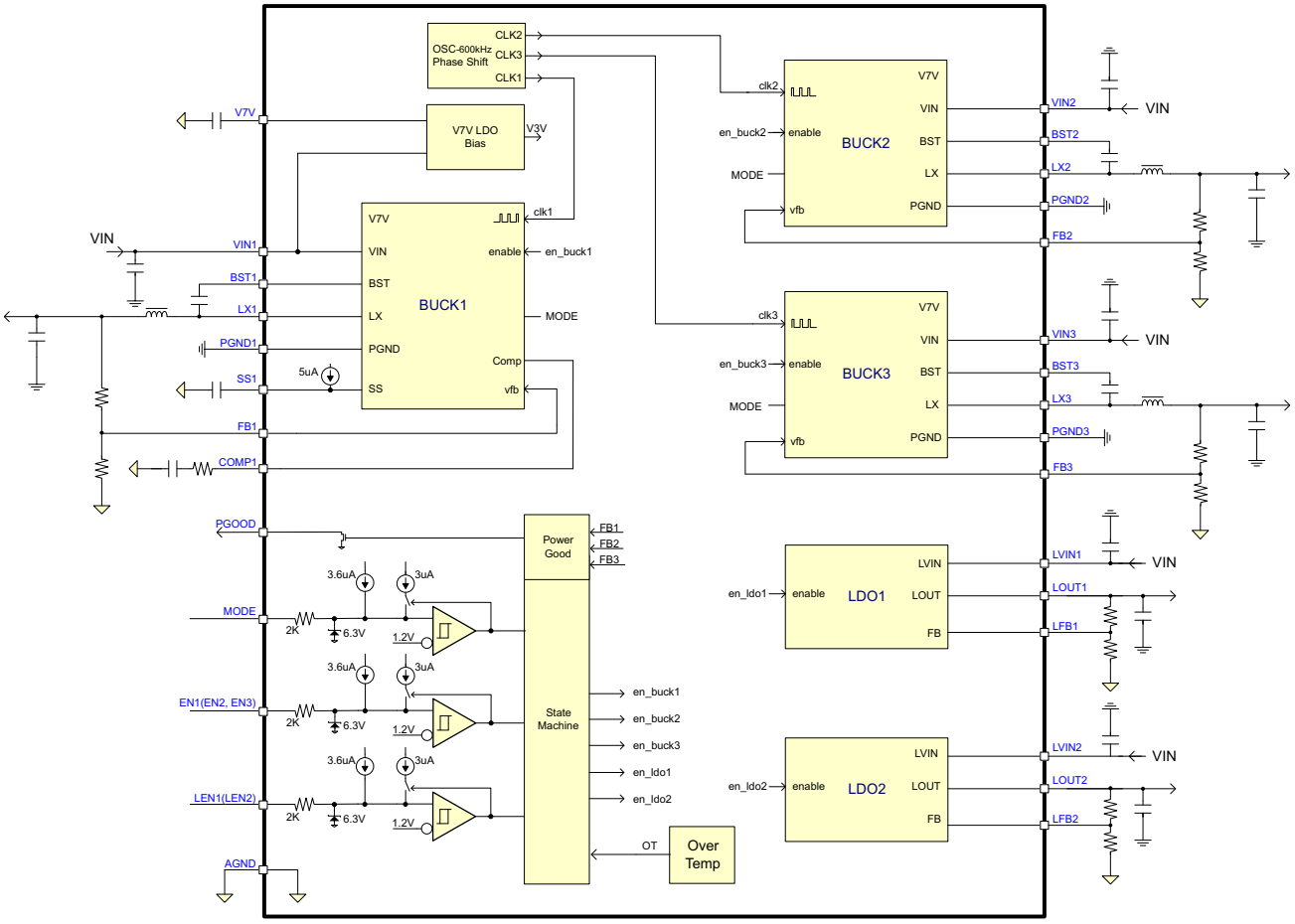
The TPS65262-2 integrates low drop-out voltage linear regulators (LDO) with input voltage from 1.3 to 18 V, independent enable and adjustable outputs, up to 350 mA for LDO1 and 150 mA for LDO2 continuous output current.

The TPS65262-2 is protected from overload and over temperature fault conditions. The converter minimizes excessive output overvoltage transients by taking advantage of the power good comparator. When the output is over, the high-side MOSFET is turned off until the internal feedback voltage is lower than 105% of the 0.6-V reference voltage. The TPS65262-2 implements both high-side MOSFET overload protection and bidirectional low-side MOSFET overload protections to avoid inductor current runaway. If the over current condition has lasted for more than the OC wait time (0.5 ms), the converter will shut down and restart after the hiccup time (14 ms). The TPS65262-2 shuts down if the junction temperature is higher than thermal shutdown trip point 160°C. When the junction temperature drops 20°C (typical) below the thermal shutdown trip point, the TPS65262-2 will be restarted under control of the soft-start circuit automatically.

The TPS65262-2 is available in a 32-lead thermally-enhanced VQFN (RHB) package.

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7.2 Functional Block Diagram



7.3 Feature Description

7.3.1 Adjusting the Output Voltage

The output voltage of each buck is set with a resistor divider from the output of buck to the FB pin. TI recommends to use 1% tolerance or better divider resistors.

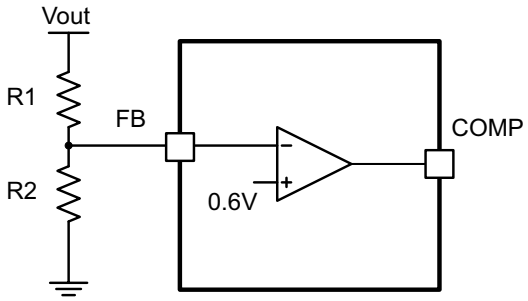


Figure 23. Voltage Divider Circuit

$$R_2 = R_1 \times \frac{0.6}{V_{out} - 0.6} \quad (1)$$

To improve efficiency at light loads consider using larger value resistors. If the values are too high, the regulator is more sensitive to noise. The recommended resistor values are shown in Table 1.

Table 1. Output Resistor Divider Selection

OUTPUT VOLTAGE (V)	R1 (kΩ)	R2 (kΩ)
1	10	15
1.2	10	10
1.5	15	10
1.8	20	10
2.5	31.6	10
3.3	45.3	10
3.3	22.6	4.99
5	73.2	10
5	36.5	4.99

7.3.2 Enable and Adjusting Undervoltage Lockout

The EN1/2/3 pin provides electrical on/off control of the device. After the EN1/2/3 pin voltage exceeds the threshold voltage, the device starts operation. If each ENx pin voltage is pulled below the threshold voltage, the regulator stops switching and enters low Iq state.

The EN pin has an internal pullup current source, allowing the user to float the EN pin for enabling the device. If an application requires controlling the EN pin, use open drain or open collector output logic to interface with the pin.

The device implements internal UVLO circuitry on the VIN pin. The device is disabled when the VIN pin voltage falls below the internal VIN UVLO threshold. The internal VIN UVLO threshold has a hysteresis of 500mV. If an application requires a higher UVLO threshold on the VIN pin, then the ENx pin can be configured as shown in Figure 24. When using the external UVLO function it is recommended to set the hysteresis to be greater than 500mV.

The EN pin has a small pullup current I_p which sets the default state of the pin to enable when no external components are connected. The pullup current is also used to control the voltage hysteresis for the UVLO function since it increases by I_h once the EN pin crosses the enable threshold. The UVLO thresholds can be calculated using Equation 2 and Equation 3.

$$R_1 = \frac{V_{START}\left(\frac{V_{ENFALLING}}{V_{ENRISING}}\right) - V_{STOP}}{I_P\left(1 - \frac{V_{ENFALLING}}{V_{ENRISING}}\right) + I_h} \quad (2)$$

$$R_2 = \frac{R_1 \times V_{ENFALLING}}{V_{STOP} - V_{ENFALLING} + R_1\left(I_h + I_p\right)}$$

where

- I_h= 3 µA
- I_p= 3.6 µA
- $V_{ENRISING}$= 1.2 V
- $V_{ENFALLING}$= 1.15 V (3)

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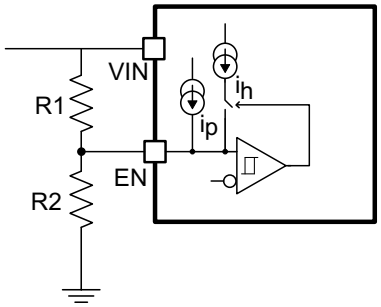


Figure 24. Adjustable VIN Undervoltage Lockout

7.3.3 Soft-Start Time

The voltage on the SS1 pin controls the start-up of buck1 output. When the voltage on the SS1 pin is less than the internal 0.6-V reference, The TPS65262-2 regulates the internal feedback voltage to the voltage on the SS1 pin instead of 0.6 V, allowing VOUT to rise smoothly from 0 V to its regulated voltage without inrush current. The device has an internal pullup current source of 5 µA (typical) that charges an external soft-start capacitor to provide a linear ramping voltage at SS1 pin.

Buck1's soft-start time can be calculated approximately by Equation 4.

Buck2 and Buck3 have fixed 1-ms soft start time.

$$Tss(ms) = Css(nF) \times \left(\frac{0.6V}{5\mu A} \right) \quad (4)$$

7.3.4 Power-Up Sequencing

The TPS65262-2 has dedicated enable pin for each converter. The converter enable pins are biased by a current source that allows for easy sequencing by the addition of an external capacitor. Disabling the converter with an active pull-down transistor on the ENx pin allows for a predictable power-down timing operation. Figure 25 shows the timing diagram of a typical buck power-up sequence with connecting a capacitor at ENx pin.

A typical 1.4-µA current is charging ENx pin from input supply. When ENx pin voltage rise to typical 0.4 V, the internal V7V LDO turns on. A 3.6-µA pullup current is sourcing ENx. After ENx pin voltage reaches to 1.2 V typical, 3-µA hysteresis current sources to the pin to improve noise sensitivity. If all output voltages are in the regulation, PGOOD is asserted after PGOOD deglitch time.

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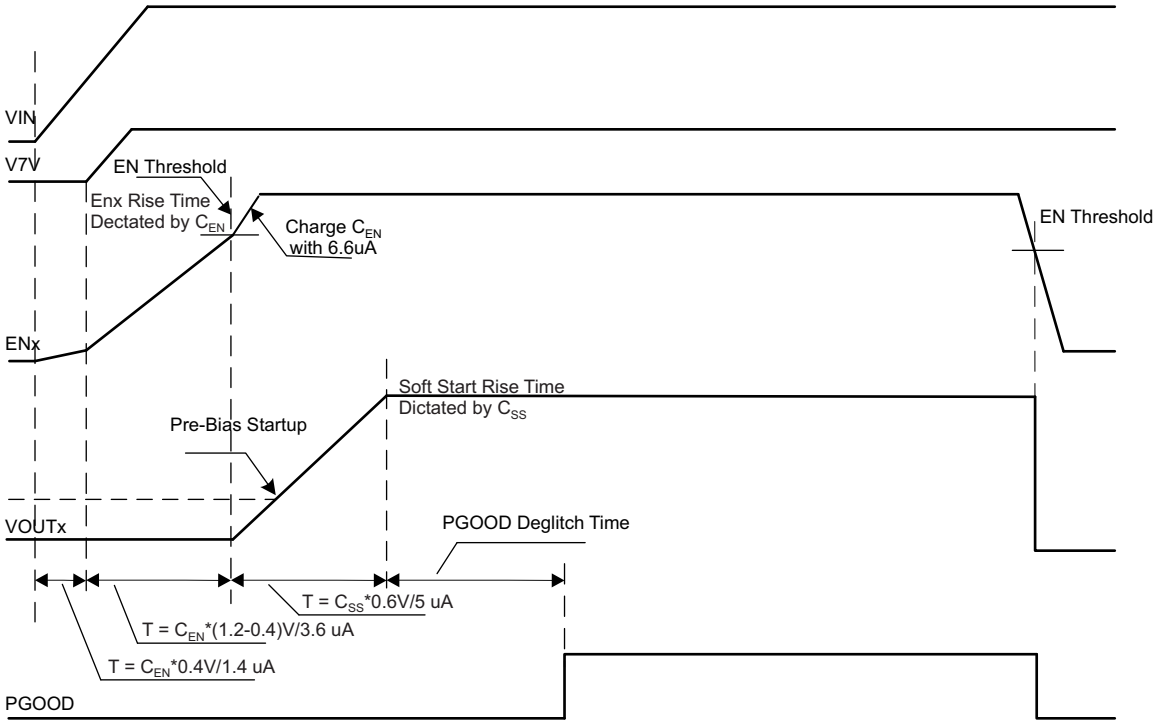


Figure 25. Startup Power Sequence

7.3.5 V7V Low Dropout Regulator and Bootstrap

Power for the high-side and low-side MOSFET drivers and most other internal circuitry is derived from the V7V pin. The internal built-in low dropout linear regulator (LDO) supplies 6.3 V (typical) from VIN to V7V. A 1-µF ceramic capacitor should be connected from V7V pin to power ground.

If the input voltage, VIN decreases to UVLO threshold voltage, the UVLO comparator detects V7V pin voltage and forces the converter off.

Each high-side MOSFET driver is biased from the floating bootstrap capacitor, CB, shown in Figure 26, which is normally recharged during each cycle through an internal low-side MOSFET or the body diode of low-side MOSFET when the high-side MOSFET turns off. The boot capacitor is charged when the BST pin voltage is less than VIN and BST-LX voltage is below regulation. The recommended value of this ceramic capacitor is 47 nF. A ceramic capacitor with an X7R or X5R grade dielectric with a voltage rating of 10 V or higher is recommended because of the stable characteristics over temperature and voltage. Each low-side MOSFET driver is powered from V7V pin directly.

To improve drop out, the device is designed to operate at 100% duty cycle as long as the BST to LX pin voltage is greater than the BST-LX UVLO threshold, which is typically 2.1 V. When the voltage between BST and LX drops below the BST-LX UVLO threshold, the high-side MOSFET is turned off and the low-side MOSFET is turned on allowing the boot capacitor to be recharged.

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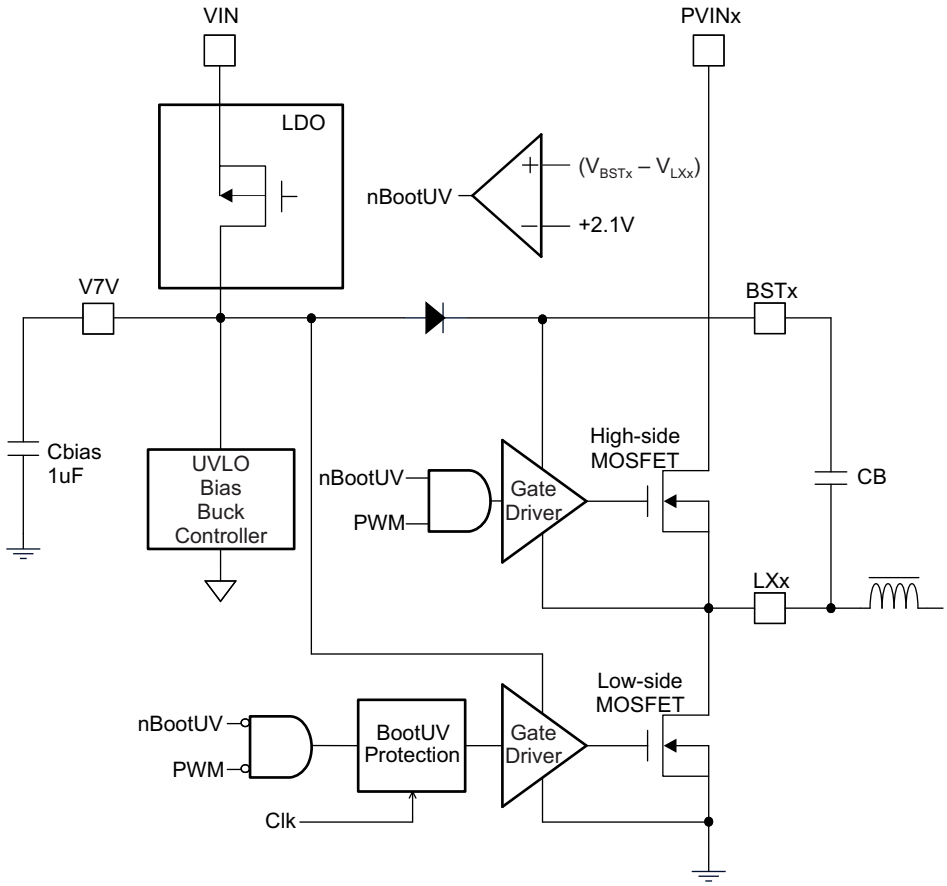


Figure 26. V7V Linear Dropout Regulator and Bootstrap Voltage Diagram

7.3.6 Out-of-Phase Operation

To reduce input ripple current, the switch clock of buck1 is 180° out-of-phase from the clock of buck2 and buck3. This enables the system having less input current ripple to reduce input capacitors' size, cost, and EMI.

7.3.7 Output Overvoltage Protection (OVP)

The device incorporates an OVP circuit to minimize output voltage overshoot. When the output is overloaded, the error amplifier compares the actual output voltage to the internal reference voltage. If the FB pin voltage is lower than the internal reference voltage for a considerable time, the output of the error amplifier demands maximum output current. Once the condition is removed, the regulator output rises and the error amplifier output transitions to the steady state voltage. In some applications with small output capacitance, the load can respond faster than the error amplifier. This leads to the possibility of an output overshoot. Each buck compares the FB pin voltage to the OVP threshold. If the FB pin voltage is greater than the OVP threshold, the high-side MOSFET is turned off preventing current from flowing to the output and minimizing output overshoot. When the FB voltage drops lower than the OVP threshold, the high-side MOSFET turns on at the next clock cycle.

7.3.8 PSM

If the MODE pin is connected to GND, the TPS65262-2 can enter high-efficiency PSM operation at light load current.

When a controller is enabled for PSM operation, the peak inductor current is sensed and compared with 230-mA current typically. Since the integrated current comparator catches the peak inductor current only, the average load current entering PSM varies with the applications and external output filters. In PSM, the sensed peak inductor current is clamped at 230 mA.

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When a controller operates in PSM, the inductor current is not allowed to reverse. The reverse current comparator turns off the low-side MOSFET when the inductor current reaches zero, preventing it from reversing and going negative.

Due to the delay in the circuit and current comparator tdly (typical 50 ns at Vin = 12 V), the real peak inductor current threshold to turn off high-side power MOSFET could shift higher depending on inductor inductance and input/output voltages. The threshold of peak inductor current to turn off high-side power MOSFET can be calculated by Equation 5.

$$IL_{PEAK} = 230mA + \frac{vin - vout}{L} \times tdly \quad (5)$$

Once the charge accumulated on Vout capacitor is more than loading need, COMP pin voltage drops to low voltage driven by error amplifier. There is an internal comparator at COMP pin. If comp voltage is lower than 0.35 V, power stage stops switching to save power.

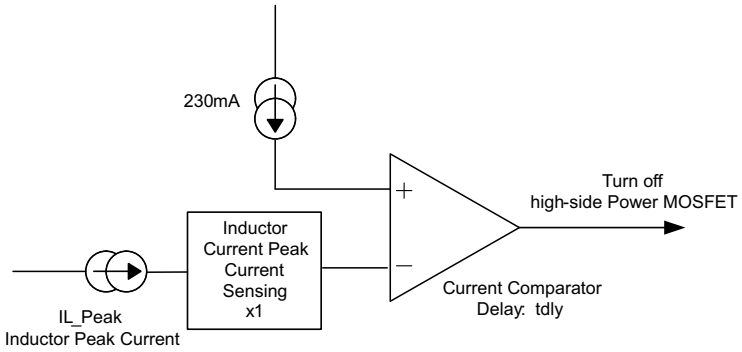


Figure 27. PSM Current Comparator

7.3.9 Slope Compensation

In order to prevent the sub-harmonic oscillations when the device operates at duty cycles greater than 50%, the device adds built-in slope compensation, which is a compensating ramp to the switch current signal.

7.3.10 Overcurrent Protection

The device is protected from over current conditions by cycle-by-cycle current limiting on both the high-side MOSFET and the low-side MOSFET.

7.3.10.1 High-Side MOSFET Overcurrent Protection

The device implements current mode control which uses the COMP pin voltage to control the turn off of the high-side MOSFET and the turn on of the low-side MOSFET on a cycle by cycle basis. Each cycle the switch current and the current reference generated by the COMP pin voltage are compared. When the peak switch current intersects the current reference, the high-side switch is turned off.

7.3.10.2 Low-Side MOSFET Overcurrent Protection

While the low-side MOSFET is turned on, its conduction current is monitored by the internal circuitry. During normal operation the low-side MOSFET sources current to the load. At the end of every clock cycle, the low-side MOSFET sourcing current is compared to the internally set low-side sourcing current limit. If the low-side sourcing current is exceeded, the high-side MOSFET is not turned on and the low-side MOSFET stays on for the next cycle. The high-side MOSFET is turned on again when the low-side current is below the low-side sourcing current limit at the start of a cycle.

The low-side MOSFET may also sink current from the load. If the low-side sinking current limit is exceeded, the low-side MOSFET is turned off immediately for the rest of that clock cycle. In this scenario both MOSFETs are off until the start of the next cycle.

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Furthermore, if an output overload condition (as measured by the COMP pin voltage) has lasted for more than the hiccup wait time which is programmed for 0.5 ms shown in Figure 28, the device will shut down itself and restart after the hiccup time 14ms. The hiccup mode helps to reduce the device power dissipation under severe overcurrent condition.

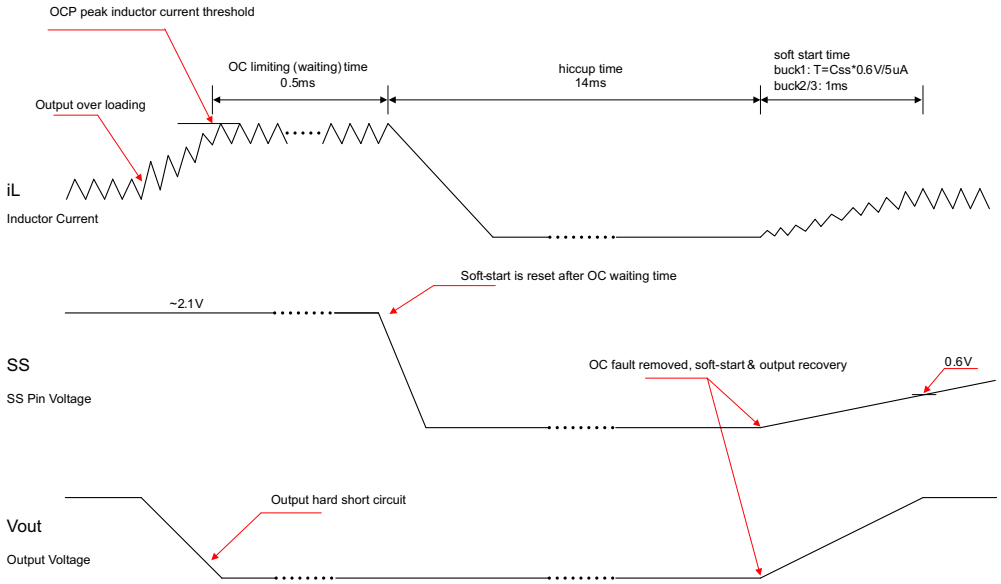


Figure 28. Overcurrent Protection

7.3.11 Power Good

The PGOOD pin is an open drain output. Once feedback voltage of each buck is between 95% (rising) and 105% (falling) of the internal voltage reference, the PGOOD pin pull-down is de-asserted and the pin floats. It is recommended to use a pullup resistor between the values of 10 and 100 kΩ to a voltage source that is 5.5 V or less. The PGOOD is in a defined state once the VIN input voltage is greater than 1 V, but with reduced current sinking capability. The PGOOD achieves full current sinking capability once the VIN input voltage is above UVLO threshold, which is 4.25 V.

The PGOOD pin is pulled low when any feedback voltage of buck is lower than 92.5% (falling) or greater than 107.5% (rising) of the nominal internal reference voltage. Also, the PGOOD is pulled low, if the input voltage is under-voltage locked up, thermal shutdown is asserted, the EN pin is pulled low or the converter is in a soft-start period.

7.3.12 Thermal Shutdown

The internal thermal shutdown circuitry forces the device to stop switching if the junction temperature exceeds 160°C typically. The device reinitiates the power up sequence when the junction temperature drops below 140°C typically.

Table 2. Related Parts

PART NUMBER	DESCRIPTION	COMMENTS
TPS65261	4.5- to 18-V, triple buck with input voltage power failure indicator	Triple buck 3-A/2-A/2-A output current, features an open drain RESET signal to monitor power down, automatic power sequencing
TPS65263	4.5- to 18-V, triple buck with I^2C interface	Triple buck 3-A/2-A/2-A output current, I2C controlled dynamic voltage scaling (DVS)
TPS65287	4.5- to 18-V, triple buck with power switch and push button control	Triple buck 3-A/2-A/2-A output current, up to 2.1-A USB power with over current setting by external resistor, push button control for intelligent system power-on/power-off operation
TPS65288	4.5- to 18-V, triple buck with dual power switches	Triple buck 3-A/2-A/2-A output current, 2 USB power switches current limiting at typical 1.2 A (0.8/1.0/1.4/1.6/1.8/2.0/2.2 A available with manufacture trim options)

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7.4 Device Functional Modes

7.4.1 Operation With V_{IN} < 4.5 V (Minimum V_{IN})

The device operates with input voltages above 4.5 V. The maximum UVLO voltage is 4.5 V and operates at input voltages above 4.5 V. The typical UVLO voltage is 4.25 V, and the device may operate at input voltages above that point. The device also may operate at lower input voltages; the minimum UVLO voltage is 4 V (rising) and 3.5 V (falling). At input voltages below the UVLO minimum voltage, the device does not operate.

7.4.2 Operation With EN Control

The enable rising edge threshold voltage is 1.2 V typical and 1.26 V maximum. With EN held below that voltage, the device is disabled and switching is inhibited. The IC quiescent current is reduced in this state. When the input voltage is above the UVLO threshold and the EN voltage is increased above the rising edge threshold, the device becomes active. Switching is enabled, and the soft-start sequence is initiated. The device starts at the soft-start time determined by the external soft start capacitor as shown in Figure 31 to Figure 36.

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8 Application and Implementation

NOTE

Information in the following applications sections is not part of the TI component specification, and TI does not warrant its accuracy or completeness. TI's customers are responsible for determining suitability of components for their purposes. Customers should validate and test their design implementation to confirm system functionality.

8.1 Application Information

The device is triple-synchronous, step-down DC/DC converter with dual LDOs. The device is typically used to convert a higher DC voltage to lower DC voltages with continuous available output current of 3 A/1 A/1 A. The following design procedure can be used to select component values for the TPS65262-2. This section presents a simplified discussion of the design process.

8.2 Typical Application

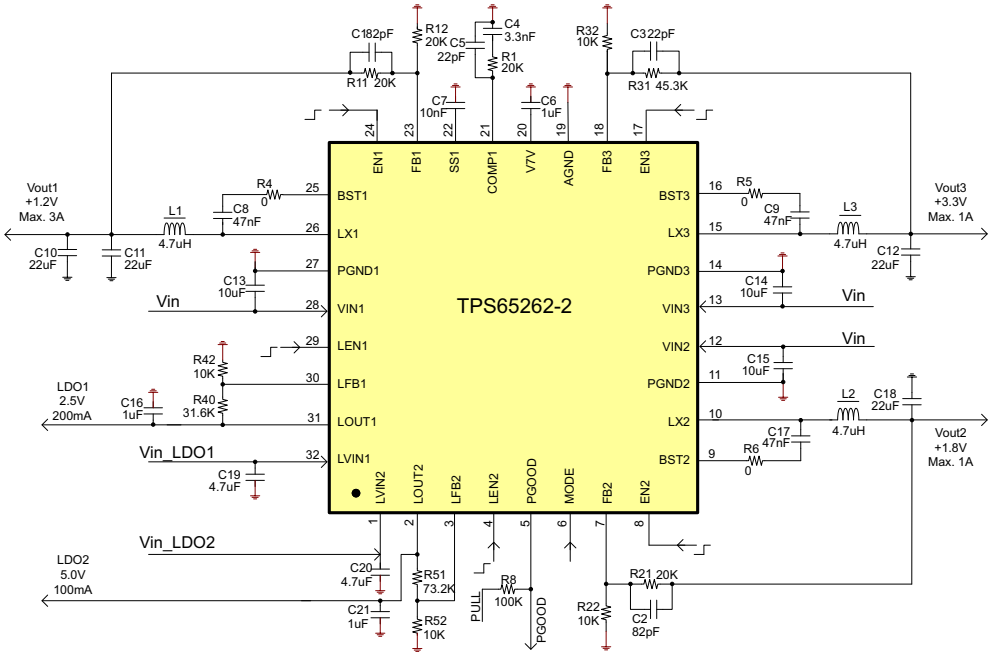


Figure 29. Typical Application Schematic

8.2.1 Design Requirements

This example details the design of a triple-synchronous step-down converter. A few parameters must be known to start the design process. These parameters are typically determined at the system level. For this example, start with the following known parameters shown in Table 3.

Table 3. Design Parameters

PARAMETER	VALUE
Vout1	1.2 V
Iout1	3 A
Vout2	1.8 V
Iout2	1 A
Vout3	3.3 V
Iout3	1 A
Buck1 transient response 1-A load step	±5%
Buck2, buck3 transient response 0.5-A load step	±5%
Input voltage	12 V normal, 4.5 to 18 V
Output voltage ripple	±1%
Switching frequency	600 kHz

8.2.2 Detailed Design Procedure

8.2.2.1 Output Inductor Selection

To calculate the value of the output inductor, use Equation 6. LIR is a coefficient that represents the amount of inductor ripple current relative to the maximum output current. The inductor ripple current is filtered by the output capacitor. Therefore, choosing high inductor ripple currents impact the selection of the output capacitor since the output capacitor must have a ripple current rating equal to or greater than the inductor ripple current. In general, the inductor ripple value is at the discretion of the designer; however, LIR is normally from 0.1 to 0.3 for the majority of applications.

$$L = \frac{V_{inmax} - V_{out}}{I_o \times LIR} \times \frac{V_{out}}{V_{inmax} \times f_{sw}} \quad (6)$$

For the output filter inductor, it is important that the RMS current and saturation current ratings not be exceeded. The RMS and peak inductor current can be found from Equation 8 and Equation 9.

$$I_{ripple} = \frac{V_{inmax} - V_{out}}{L} \times \frac{V_{out}}{V_{inmax} \times f_{sw}} \quad (7)$$

$$I_{Lrms} = \sqrt{I_O^2 + \frac{\left(\frac{V_{out} \times (V_{inmax} - V_{out})}{V_{inmax} \times L \times f_{sw}}\right)^2}{12}} \quad (8)$$

$$I_{Lpeak} = I_{out} + \frac{I_{ripple}}{2} \quad (9)$$

The current flowing through the inductor is the inductor ripple current plus the output current. During power up, faults or transient load conditions, the inductor current can increase above the calculated peak inductor current level calculated above. In transient conditions, the inductor current can increase up to the switch current limit of the device. For this reason, the most conservative approach is to specify an inductor with a saturation current rating equal to or greater than the switch current limit rather than the peak inductor current.

8.2.2.2 Output Capacitor Selection

There are three primary considerations for selecting the value of the output capacitor. The output capacitor determines the modulator pole, the output voltage ripple, and how the regulator responds to a large change in load current. The output capacitance needs to be selected based on the most stringent of these three criteria.

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The desired response to a large change in the load current is the first criteria. The output capacitor needs to supply the load with current when the regulator cannot. This situation would occur if there are desired hold-up times for the regulator where the output capacitor must hold the output voltage above a certain level for a specified amount of time after the input power is removed. The regulator is also temporarily not able to supply sufficient output current if there is a large, fast increase in the current needs of the load such as a transition from no load to full load. The regulator usually needs two or more clock cycles for the control loop to see the change in load current and output voltage and adjust the duty cycle to react to the change. The output capacitor must be sized to supply the extra current to the load until the control loop responds to the load change. The output capacitance must be large enough to supply the difference in current for 2 clock cycles while only allowing a tolerable amount of droop in the output voltage. Equation 10 shows the minimum output capacitance necessary to accomplish this.

$$C_o = \frac{2 \times \Delta I_{out}}{f_{sw} \times \Delta V_{out}}$$

where

- ΔIout is the change in output current.
- f_{sw} is the regulator's switching frequency.
- ΔVout is the allowable change in the output voltage. (10)

Equation 11 calculates the minimum output capacitance needed to meet the output voltage ripple specification.

$$C_o > \frac{1}{8 \times f_{sw}} \times \frac{1}{\frac{V_{oripple}}{I_{oripple}}}$$

where

- f_{sw} is the switching frequency
- $V_{oripple}$ is the maximum allowable output voltage ripple
- $I_{oripple}$ is the inductor ripple current (11)

Equation 12 calculates the maximum ESR an output capacitor can have to meet the output voltage ripple specification.

$$R_{esr} < \frac{V_{oripple}}{I_{oripple}} \quad (12)$$

Additional capacitance de-ratings for aging, temperature and DC bias should be factored in which increases this minimum value. Capacitors generally have limits to the amount of ripple current they can handle without failing or producing excess heat. An output capacitor that can support the inductor ripple current must be specified. Some capacitor data sheets specify the root mean square (RMS) value of the maximum ripple current. Equation 13 can be used to calculate the RMS ripple current the output capacitor needs to support.

$$I_{corms} = \frac{V_{out} \times (V_{inmax} - V_{out})}{\sqrt{12} \times V_{inmax} \times L \times f_{sw}} \quad (13)$$

8.2.2.3 Input Capacitor Selection

The TPS65262-2 requires a high quality ceramic, type X5R or X7R, input decoupling capacitor of at least 10 µF of effective capacitance on the VIN input voltage pins. In some applications additional bulk capacitance may also be required for the VIN input. The effective capacitance includes any DC bias effects. The voltage rating of the input capacitor must be greater than the maximum input voltage. The capacitor must also have a ripple current rating greater than the maximum input current ripple of The TPS65262-2. The input ripple current can be calculated using Equation 14.

$$I_{inrms} = I_{out} \times \sqrt{\frac{V_{out}}{V_{inmin}} \times \frac{(V_{inmin} - V_{out})}{V_{inmin}}} \quad (14)$$

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The value of a ceramic capacitor varies significantly over temperature and the amount of DC bias applied to the capacitor. The capacitance variations due to temperature can be minimized by selecting a dielectric material that is stable over temperature. X5R and X7R ceramic dielectrics are usually selected for power regulator capacitors because they have a high capacitance to volume ratio and are fairly stable over temperature. The output capacitor must also be selected with the DC bias taken into account. The capacitance value of a capacitor decreases as the DC bias across a capacitor increases. The input capacitance value determines the input ripple voltage of the regulator. The input voltage ripple can be calculated using Equation 15.

$$\Delta V_{in} = \frac{I_{outmax} \times 0.25}{C_{in} \times f_{sw}} \quad (15)$$

8.2.2.4 Loop Compensation

The TPS65262-2 incorporates a peak current mode control scheme. The error amplifier is a transconductance amplifier with a gain of 300 µS. A typical type II compensation circuit adequately delivers a phase margin between 60° to 90°. C_b adds a high-frequency pole to attenuate high frequency noise when needed. To calculate the external compensation components, follow the following steps.

1. Switching frequency f_{sw} 600 kHz is appropriate for application depending on L and C sizes, output ripple, EMI, and so forth, also gives best trade-off between performance and cost.
2. Set up crossover frequency, fc, which is typically between 1/5 and 1/20 of f_{sw}.
3. R_C can be determined by

$$R_C = \frac{2\pi \times fc \times Vo \times Co}{G_{m-EA} \times Vref \times G_{m-PS}} \quad (16)$$

   Where G_{m_EA} is the error amplifier gain (300 µS), G_{m_PS} is the power stage voltage to current conversion gain (7.4 A/V).

4. Calculate C_C by placing a compensation zero at or before the dominant pole $\left(fp = \frac{1}{C_o \times R_L \times 2\pi} \right)$.

$$C_C = \frac{R_L \times Co}{R_C} \quad (17)$$

5. Optional C_b can be used to cancel the zero from the ESR associated with C_O.

$$C_b = \frac{R_{ESR} \times Co}{R_C} \quad (18)$$

6. Type III compensation can be implemented with the addition of one capacitor, C1. This allows for slightly higher loop bandwidths and higher phase margins. If used, C1 is calculated from Equation 19.

$$C1 = \frac{1}{2\pi \times R1 \times f_c} \quad (19)$$

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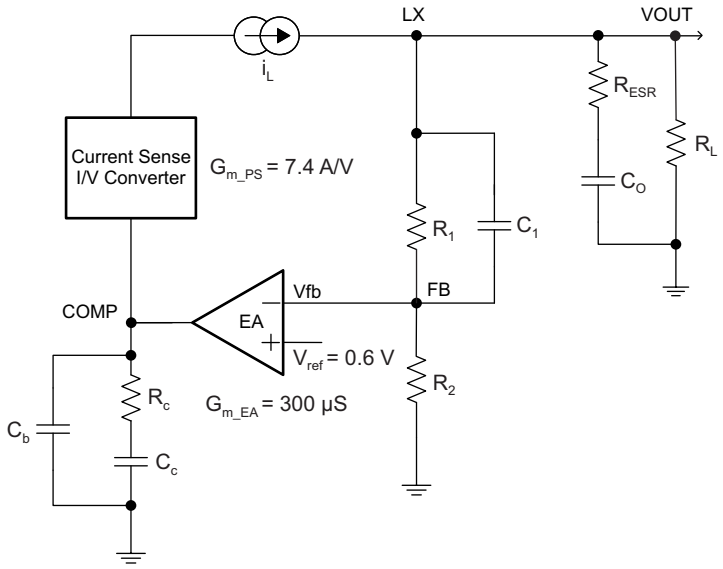


Figure 30. DC/DC Loop Compensation

8.2.3 Application Curves

T_A = 25°C, VIN = 12 V, VOUT1 = 1.2 V, VOUT2 = 1.8 V, VOUT3 = 3.3 V, f_{SW} = 600 kHz, PSM mode (unless otherwise noted)

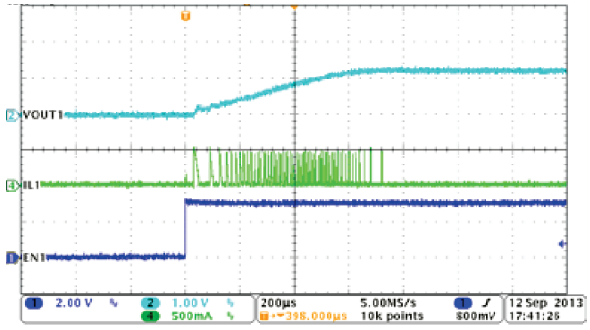


Figure 31. PSM Mode Buck1, Soft-Start With No Load

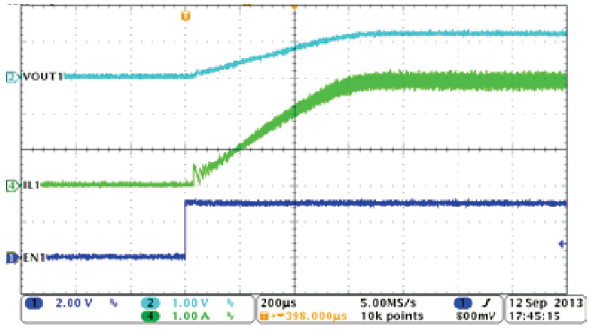


Figure 32. PSM Mode Buck1, Soft-Start With Full Load

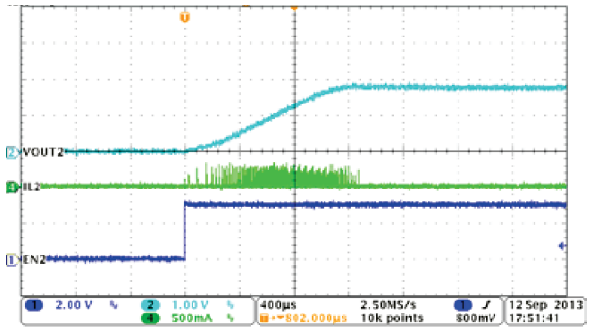


Figure 33. PSM Mode Buck2, Soft-Start With No Load

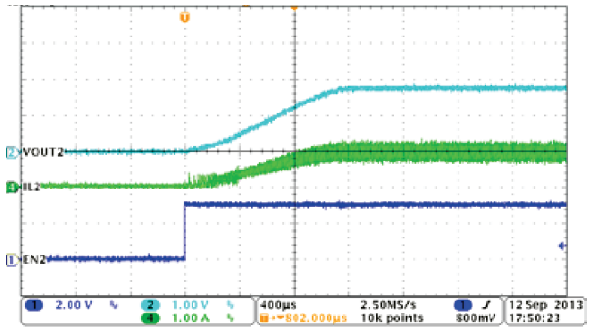


Figure 34. PSM Mode Buck2, Soft-Start With Full Load

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T_A = 25°C, VIN = 12 V, VOUT1 = 1.2 V, VOUT2 = 1.8 V, VOUT3 = 3.3 V, f_{SW} = 600 kHz, PSM mode (unless otherwise noted)

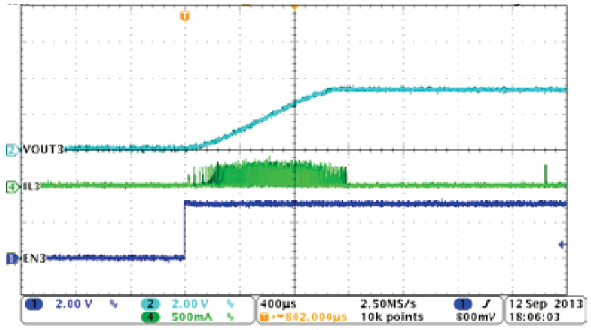


Figure 35. PSM Mode Buck3, Soft-Start With No Load

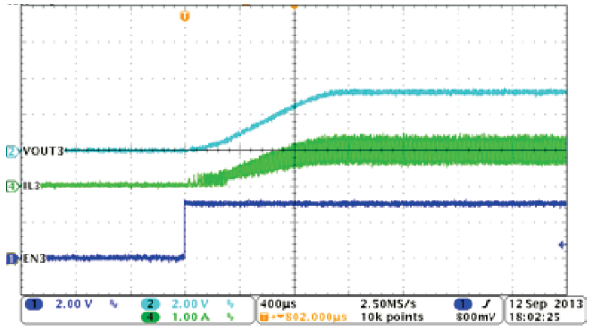


Figure 36. PSM Mode Buck3, Soft-Start With Full Load

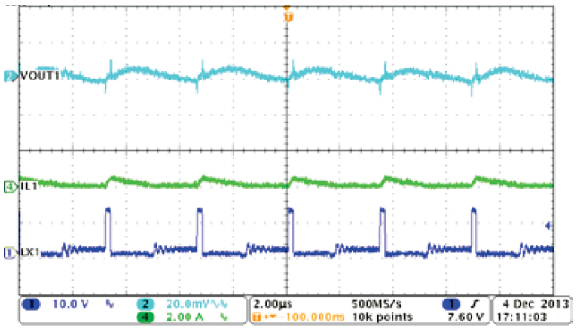


Figure 37. PSM Mode Buck1, Steady State Operation With Light Load

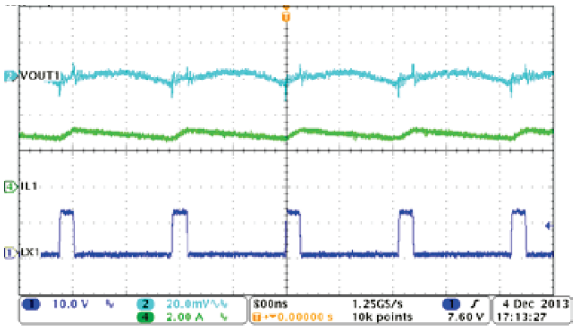


Figure 38. Buck1, Steady State Operation With Full Load

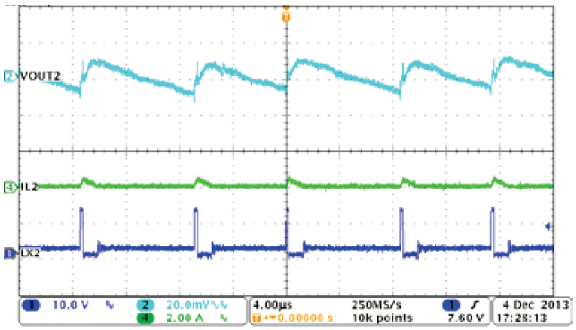


Figure 39. PSM Mode Buck2, Steady State Operation With Light Load

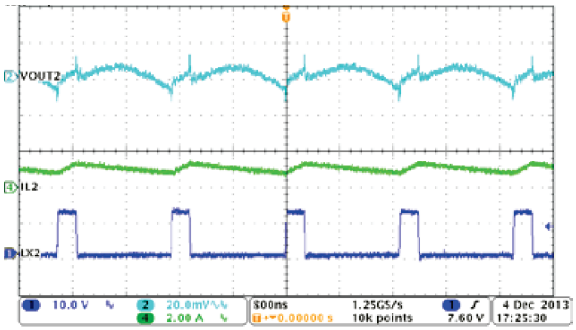


Figure 40. Buck2, Steady State Operation With Full Load

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T_A = 25°C, VIN = 12 V, VOUT1 = 1.2 V, VOUT2 = 1.8 V, VOUT3 = 3.3 V, f_{SW} = 600 kHz, PSM mode (unless otherwise noted)

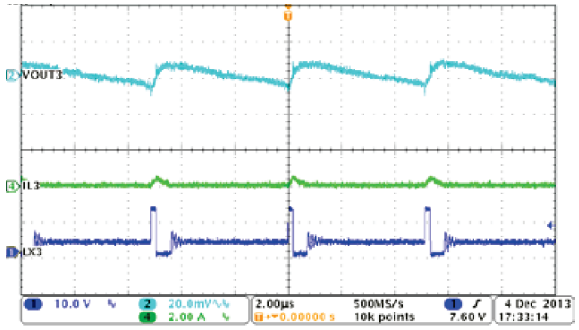


Figure 41. PSM Mode Buck3, Steady State Operation With Light Load

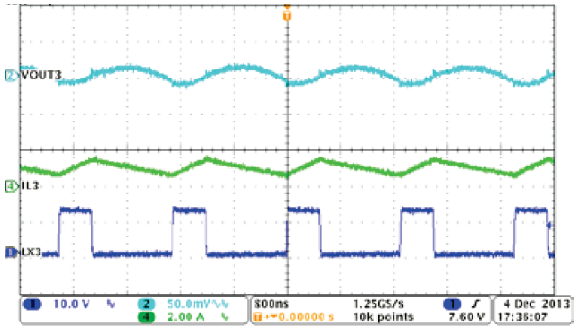


Figure 42. Buck3, Steady State Operation With Full Load

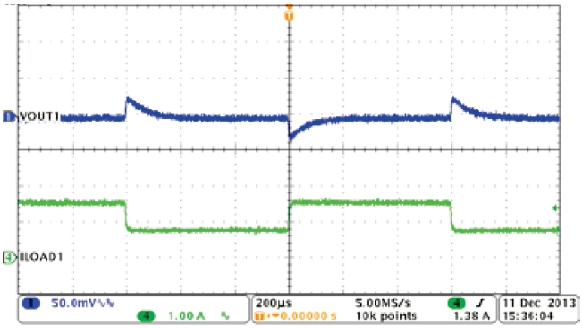


Figure 43. Buck1, Load Transient, 0.75 to 1.5 A SR = 0.25 A/µs

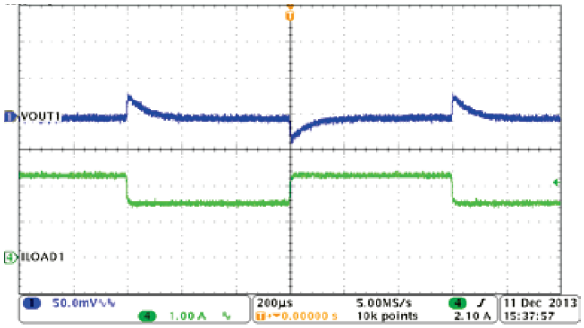


Figure 44. Buck1, Load Transient, 1.5 to 2.25 A SR = 0.25 A/µs

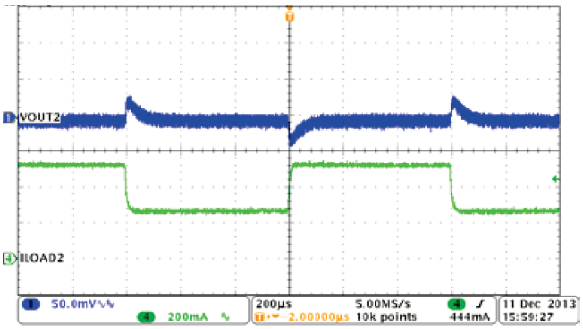


Figure 45. Buck2, Load Transient, 0.25 to 0.5 A SR = 0.25 A/µs

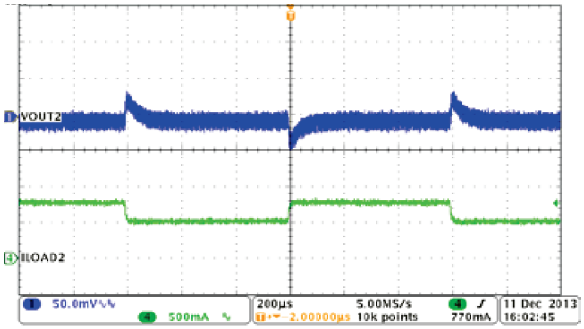


Figure 46. Buck2, Load Transient, 0.5 to 0.75 A SR = 0.25A/µs

T_A = 25°C, VIN = 12 V, VOUT1 = 1.2 V, VOUT2 = 1.8 V, VOUT3 = 3.3 V, f_{SW} = 600 kHz, PSM mode (unless otherwise noted)

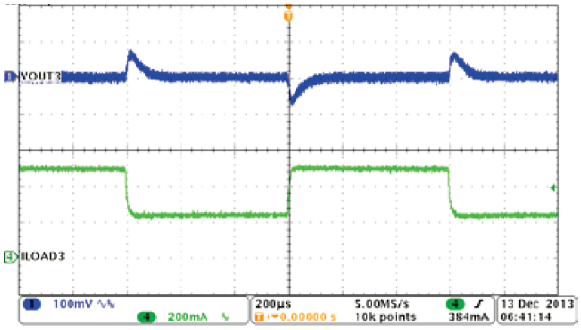


Figure 47. Buck3, Load Transient, 0.25 to 0.5 A SR = 0.25 A/µs

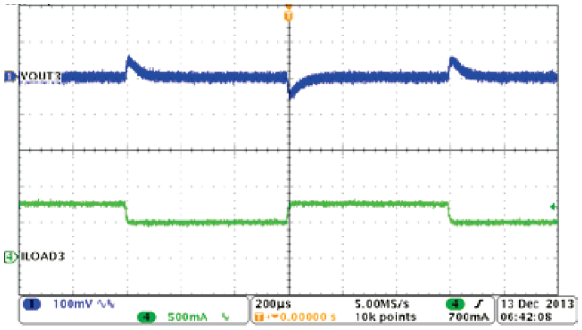


Figure 48. Buck3, Load Transient, 0.5 to 0.75 A SR = 0.25A/µs

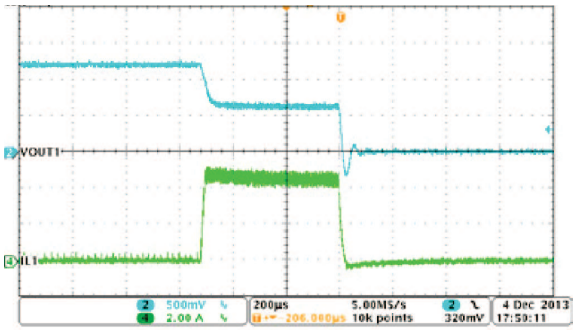


Figure 49. Buck1, Overcurrent Protection

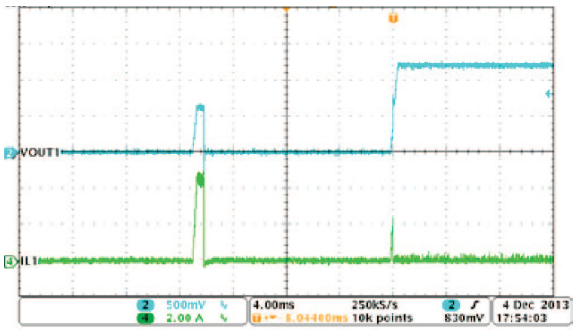


Figure 50. Buck1, Hiccup and Recovery

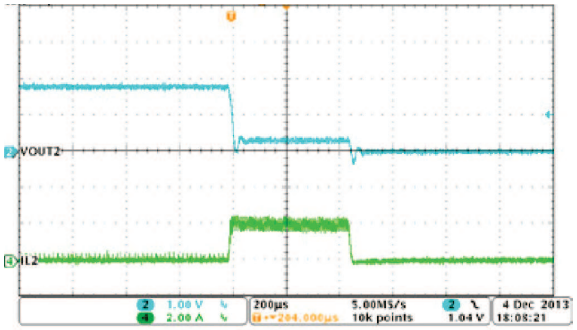


Figure 51. Buck2, Overcurrent Protection

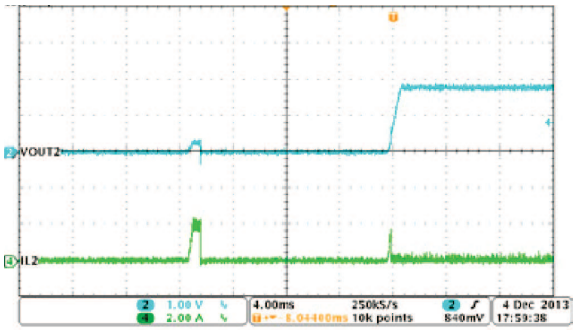


Figure 52. Buck2, Hiccup and Recovery

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T_A = 25°C, VIN = 12 V, VOUT1 = 1.2 V, VOUT2 = 1.8 V, VOUT3 = 3.3 V, f_{SW} = 600 kHz, PSM mode (unless otherwise noted)

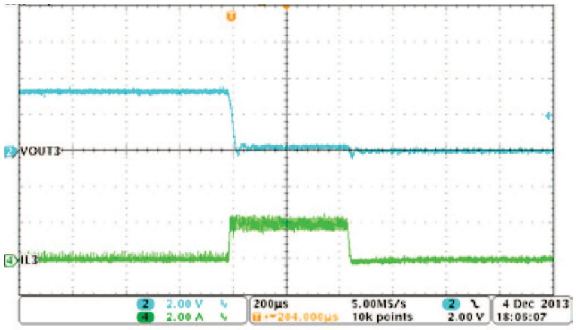


Figure 53. Buck3, Overcurrent Protection

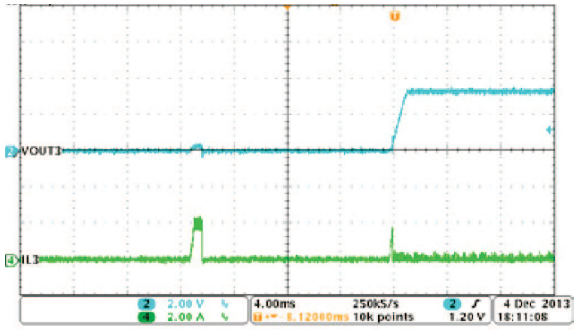


Figure 54. Buck3, Hiccup and Recovery

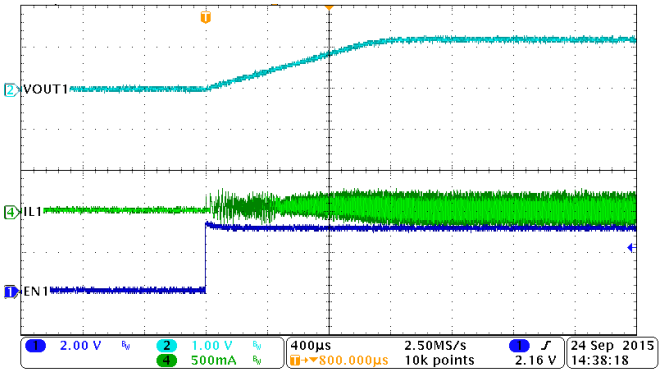


Figure 55. PWM Mode, Buck1, Soft-Start With No Load

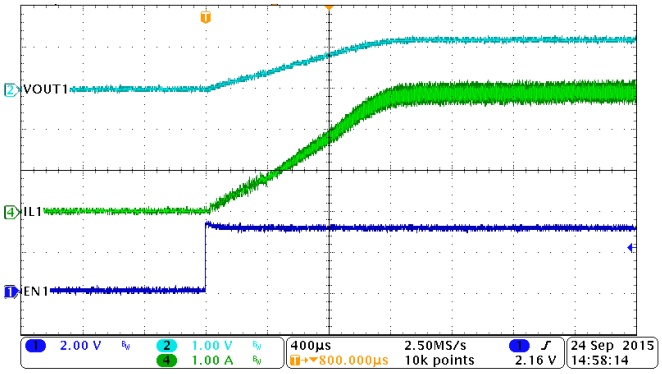


Figure 56. PWM Mode, Buck1, Soft-Start With Full Load

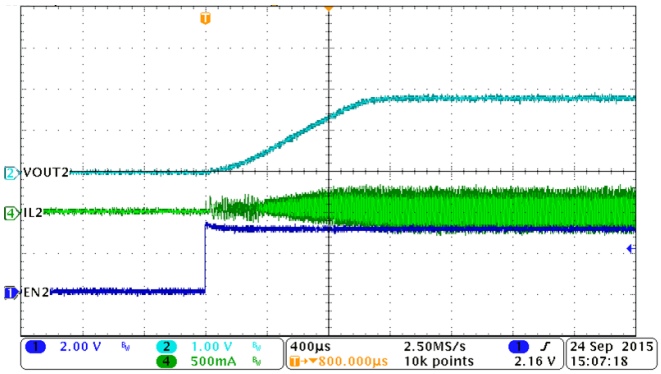


Figure 57. PWM Mode, Buck2, Soft-Start With No Load

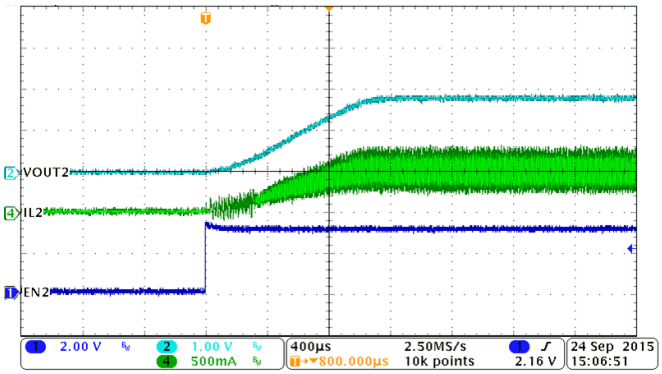


Figure 58. PWM Mode, Buck2, Soft-Start With Full Load

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T_A = 25°C, VIN = 12 V, VOUT1 = 1.2 V, VOUT2 = 1.8 V, VOUT3 = 3.3 V, f_{SW} = 600 kHz, PSM mode (unless otherwise noted)

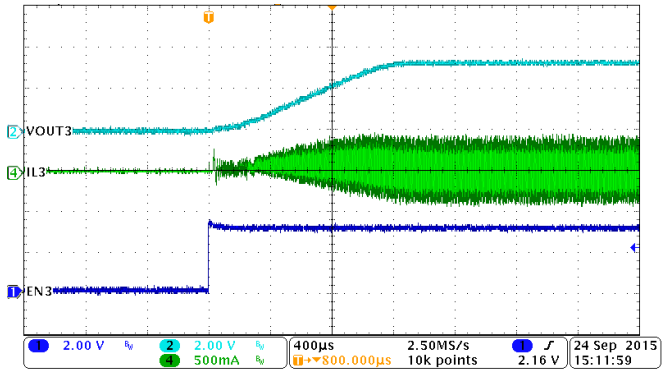


Figure 59. PWM Mode, Buck3, Soft-Start With No Load

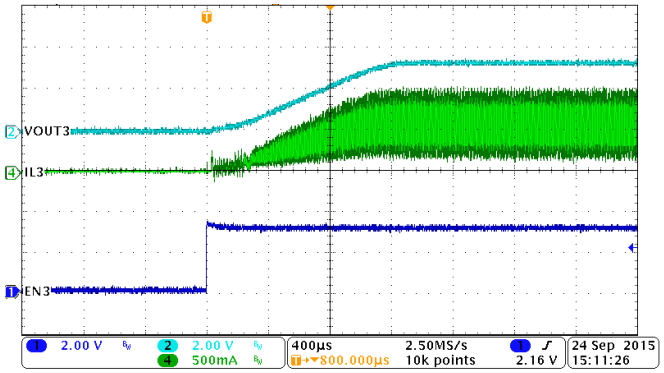


Figure 60. PWM Mode, Buck3, Soft-Start With Full Load

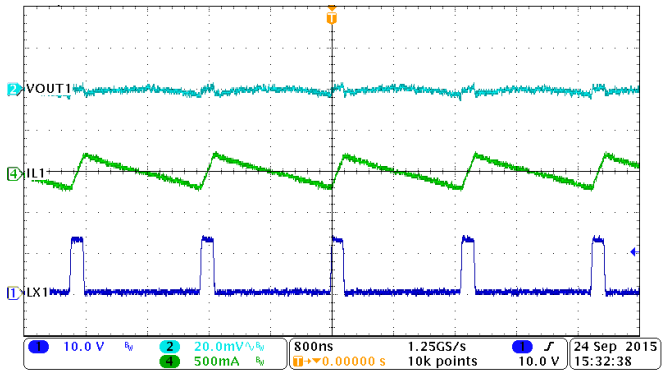


Figure 61. PWM Mode, Buck1, Steady State Operation With No Load

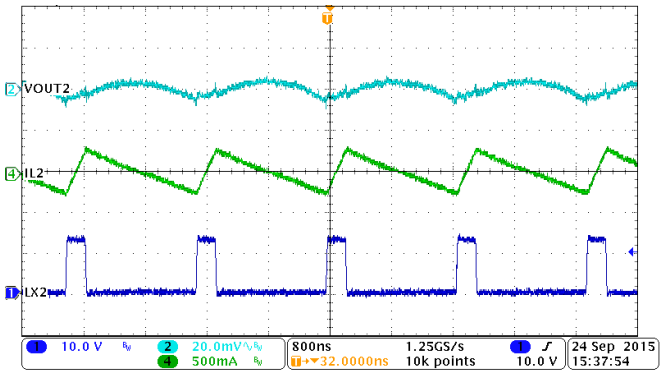
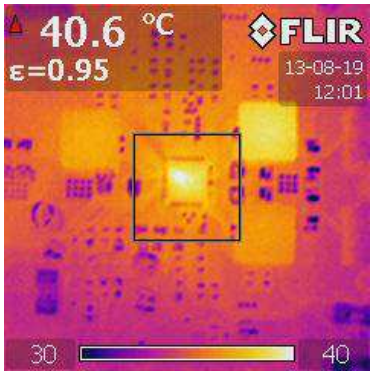
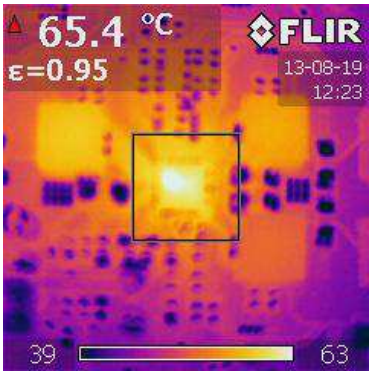


Figure 62. PWM Mode, Buck2, Steady State Operation With No Load



Operating at VIN = 12 V VOUT1 = 1.2 V/1.5 A
VOUT3 = 3.3 V/0.5 A VOUT2 = 1.8 V/0.5 A

Figure 63. Thermal Signature of TPS65262-2EVM EVM Condition 4 Layers, 64 mm × 69 mm, T_A = 30.5°C



Operating at VIN = 12 V VOUT1 = 1.2 V/3 A
VOUT3 = 3.3 V/1 A VOUT2 = 1.8 V/1 A

Figure 64. Thermal Signature of TPS65262-2EVM EVM Condition 4 Layers, 64 mm × 69 mm, T_A = 30.5°C

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9 Power Supply Recommendations

A wide 4.5- to 18-V input supply voltage range encompasses the most intermediate bus voltage operating off 5-, 9-, 12-, or 15-V power bus. The converter, with constant frequency peak current mode, is designed to simplify its application while giving designers options to optimize the system according to targeted applications.

10 Layout

10.1 Layout Guidelines

The TPS65262-2 supports a 2-layer PCB layout, shown in Figure 65.

Layout is a critical portion of good power supply design. See Figure 65 for a PCB layout example. The top contains the main power traces for VIN, VOUT, and LX. Also on the top layer are connections for the remaining pins of the TPS65262-2 and a large top side area filled with ground. The top layer ground area should be connected to the bottom layer ground using vias at the input bypass capacitor, the output filter capacitor and directly under the TPS65262-2 device to provide a thermal path from the exposed thermal pad land to ground. The bottom layer acts as ground plane connecting analog ground and power ground.

For operation at full rated load, the top side ground area together with the bottom side ground plane must provide adequate heat dissipating area. There are several signals paths that conduct fast changing currents or voltages that can interact with stray inductance or parasitic capacitance to generate noise or degrade the power supplies performance. To help eliminate these problems, the VIN pin should be bypassed to ground with a low ESR ceramic bypass capacitor with X5R or X7R dielectric. Care should be taken to minimize the loop area formed by the bypass capacitor connections, the VIN pins, and the ground connections. The VIN pin must also be bypassed to ground using a low-ESR ceramic capacitor with X5R or X7R dielectric.

Since the LX connection is the switching node, the output inductor should be located close to the LX pins, and the area of the PCB conductor minimized to prevent excessive capacitive coupling. The output filter capacitor ground should use the same power ground trace as the VIN input bypass capacitor. Try to minimize this conductor length while maintaining adequate width. The small signal components should be grounded to the analog ground path.

The FB and COMP pins are sensitive to noise so the resistors and capacitors should be located as close as possible to the IC and routed with minimal lengths of trace. The additional external components can be placed approximately as shown.

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10.2 Layout Example

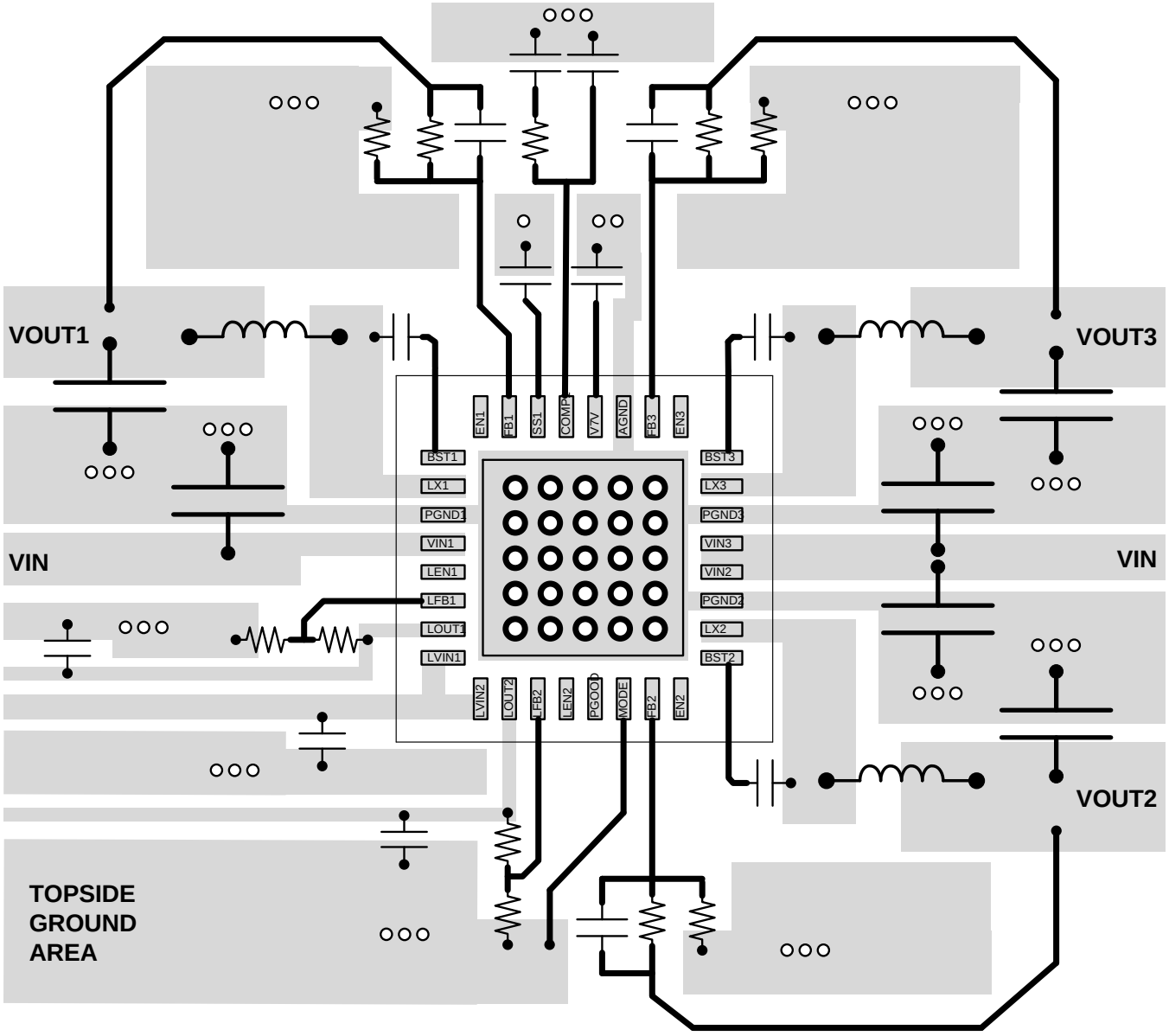


Figure 65. PCB Layout

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11 Device and Documentation Support

11.1 Community Resources

The following links connect to TI community resources. Linked contents are provided "AS IS" by the respective contributors. They do not constitute TI specifications and do not necessarily reflect TI's views; see TI's Terms of Use.

TI E2E™ Online Community ***TI's Engineer-to-Engineer (E2E) Community.*** Created to foster collaboration among engineers. At e2e.ti.com, you can ask questions, share knowledge, explore ideas and help solve problems with fellow engineers.

Design Support ***TI's Design Support*** Quickly find helpful E2E forums along with design support tools and contact information for technical support.

11.2 Trademarks

E2E is a trademark of Texas Instruments.
All other trademarks are the property of their respective owners.

11.3 Electrostatic Discharge Caution



These devices have limited built-in ESD protection. The leads should be shorted together or the device placed in conductive foam during storage or handling to prevent electrostatic damage to the MOS gates.

11.4 Glossary

SLYZ022 — *TI Glossary*.

This glossary lists and explains terms, acronyms, and definitions.

12 Mechanical, Packaging, and Orderable Information

The following pages include mechanical, packaging, and orderable information. This information is the most current data available for the designated devices. This data is subject to change without notice and revision of this document. For browser-based versions of this data sheet, refer to the left-hand navigation.

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PACKAGING INFORMATION

Orderable Device	Status (1)	Package Type	Package Drawing	Pins	Package Qty	Eco Plan (2)	Lead/Ball Finish (6)	MSL Peak Temp (3)	Op Temp (°C)	Device Marking (4/5)	Samples
TPS65262-2RHBR	ACTIVE	VQFN	RHB	32	3000	Green (RoHS & no Sb/Br)	NIPDAU	Level-2-260C-1 YEAR	-40 to 85	TPS 65262-2	Samples
TPS65262-2RHBT	ACTIVE	VQFN	RHB	32	250	Green (RoHS & no Sb/Br)	NIPDAU	Level-2-260C-1 YEAR	-40 to 85	TPS 65262-2	Samples

(1) The marketing status values are defined as follows:
ACTIVE: Product device recommended for new designs.
LIFEBUY: TI has announced that the device will be discontinued, and a lifetime-buy period is in effect.
NRND: Not recommended for new designs. Device is in production to support existing customers, but TI does not recommend using this part in a new design.
PREVIEW: Device has been announced but is not in production. Samples may or may not be available.
OBSOLETE: TI has discontinued the production of the device.

(2) **RoHS:** TI defines "RoHS" to mean semiconductor products that are compliant with the current EU RoHS requirements for all 10 RoHS substances, including the requirement that RoHS substance do not exceed 0.1% by weight in homogeneous materials. Where designed to be soldered at high temperatures, "RoHS" products are suitable for use in specified lead-free processes. TI may reference these types of products as "Pb-Free".
RoHS Exempt: TI defines "RoHS Exempt" to mean products that contain lead but are compliant with EU RoHS pursuant to a specific EU RoHS exemption.
Green: TI defines "Green" to mean the content of Chlorine (Cl) and Bromine (Br) based flame retardants meet JS709B low halogen requirements of <=1000ppm threshold. Antimony trioxide based flame retardants must also meet the <=1000ppm threshold requirement.

(3) MSL, Peak Temp. - The Moisture Sensitivity Level rating according to the JEDEC industry standard classifications, and peak solder temperature.

(4) There may be additional marking, which relates to the logo, the lot trace code information, or the environmental category on the device.

(5) Multiple Device Markings will be inside parentheses. Only one Device Marking contained in parentheses and separated by a "~" will appear on a device. If a line is indented then it is a continuation of the previous line and the two combined represent the entire Device Marking for that device.

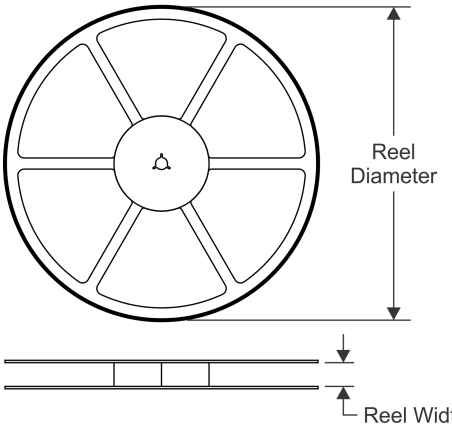
(6) Lead/Ball Finish - Orderable Devices may have multiple material finish options. Finish options are separated by a vertical ruled line. Lead/Ball Finish values may wrap to two lines if the finish value exceeds the maximum column width.

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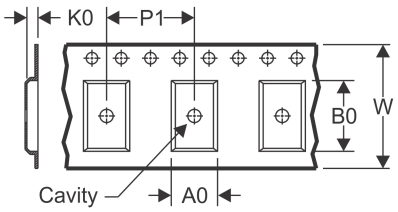
In no event shall TI's liability arising out of such information exceed the total purchase price of the TI part(s) at issue in this document sold by TI to Customer on an annual basis.

TAPE AND REEL INFORMATION

REEL DIMENSIONS

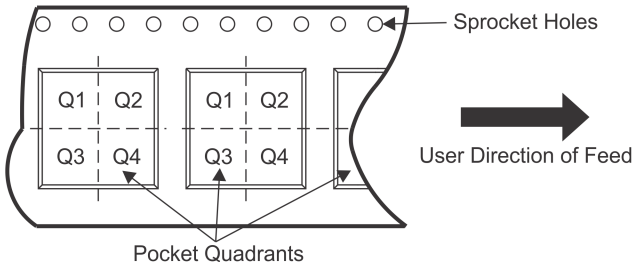


TAPE DIMENSIONS



A0	Dimension designed to accommodate the component width
B0	Dimension designed to accommodate the component length
K0	Dimension designed to accommodate the component thickness
W	Overall width of the carrier tape
P1	Pitch between successive cavity centers

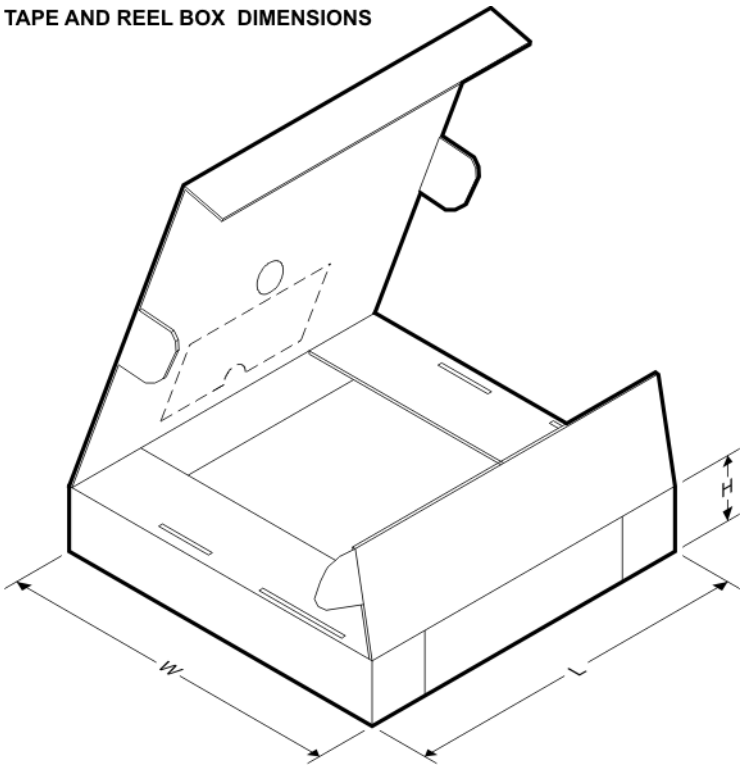
QUADRANT ASSIGNMENTS FOR PIN 1 ORIENTATION IN TAPE



*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Reel Diameter (mm)	Reel Width W1 (mm)	A0 (mm)	B0 (mm)	K0 (mm)	P1 (mm)	W (mm)	Pin1 Quadrant
TPS65262-2RHBR	VQFN	RHB	32	3000	330.0	12.4	5.3	5.3	1.1	8.0	12.0	Q2
TPS65262-2RHBT	VQFN	RHB	32	250	180.0	12.4	5.3	5.3	1.1	8.0	12.0	Q2

TAPE AND REEL BOX DIMENSIONS



*All dimensions are nominal

Device	Package Type	Package Drawing	Pins	SPQ	Length (mm)	Width (mm)	Height (mm)
TPS65262-2RHBR	VQFN	RHB	32	3000	367.0	367.0	35.0
TPS65262-2RHBT	VQFN	RHB	32	250	210.0	185.0	35.0

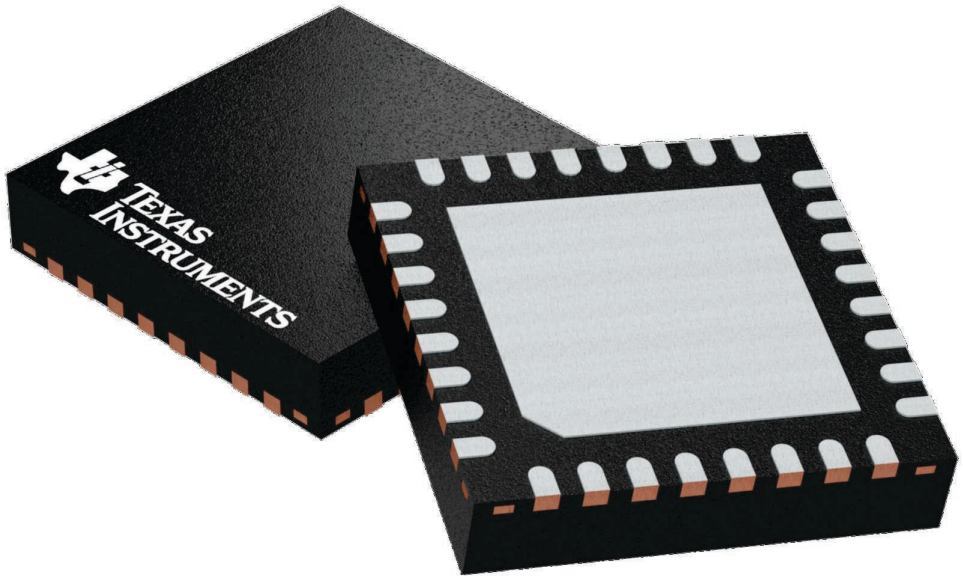
GENERIC PACKAGE VIEW

RHB 32

VQFN - 1 mm max height

5 x 5, 0.5 mm pitch

PLASTIC QUAD FLATPACK - NO LEAD



Images above are just a representation of the package family, actual package may vary.
Refer to the product data sheet for package details.

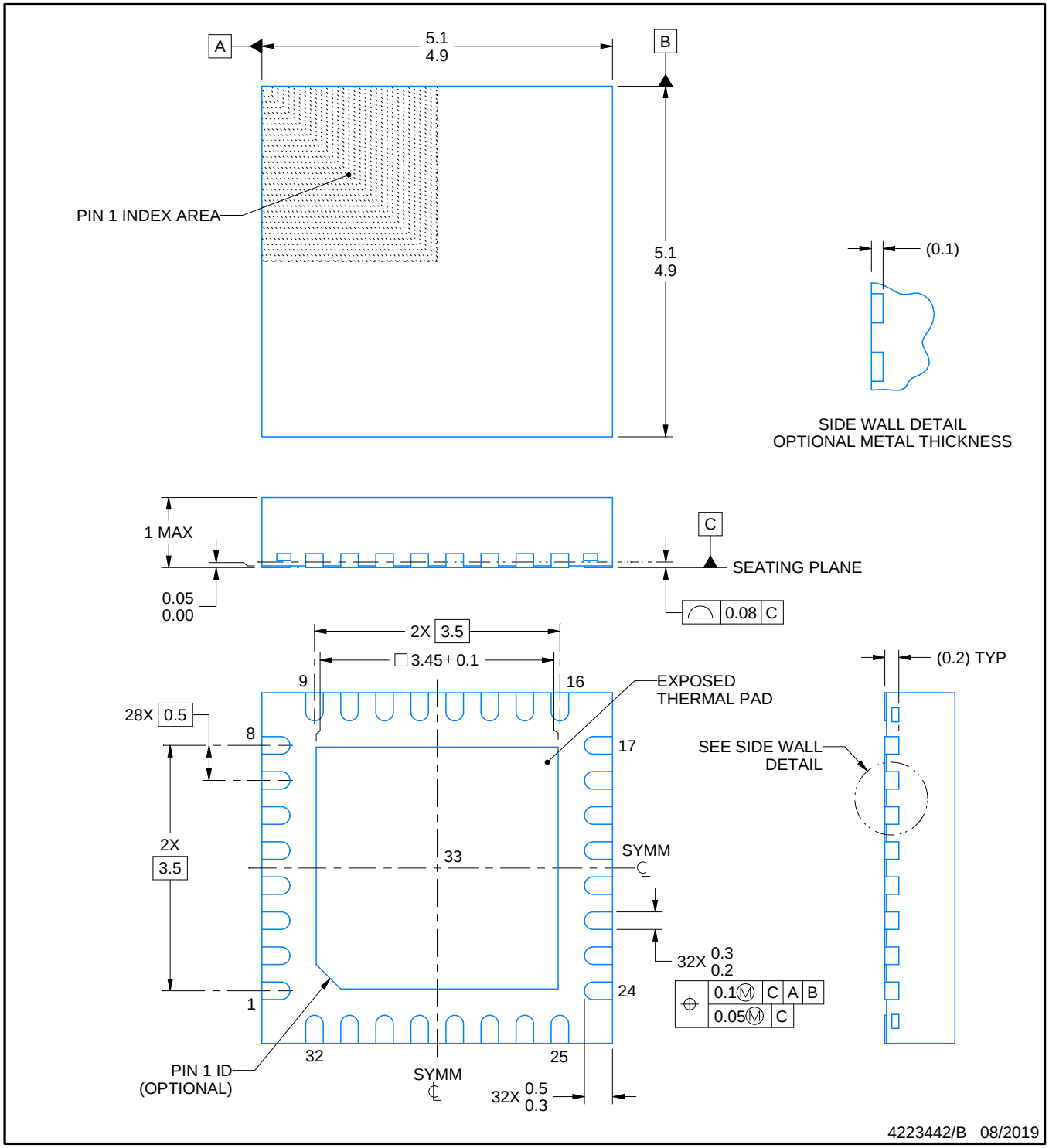
4224745/A

RHB0032E

PACKAGE OUTLINE

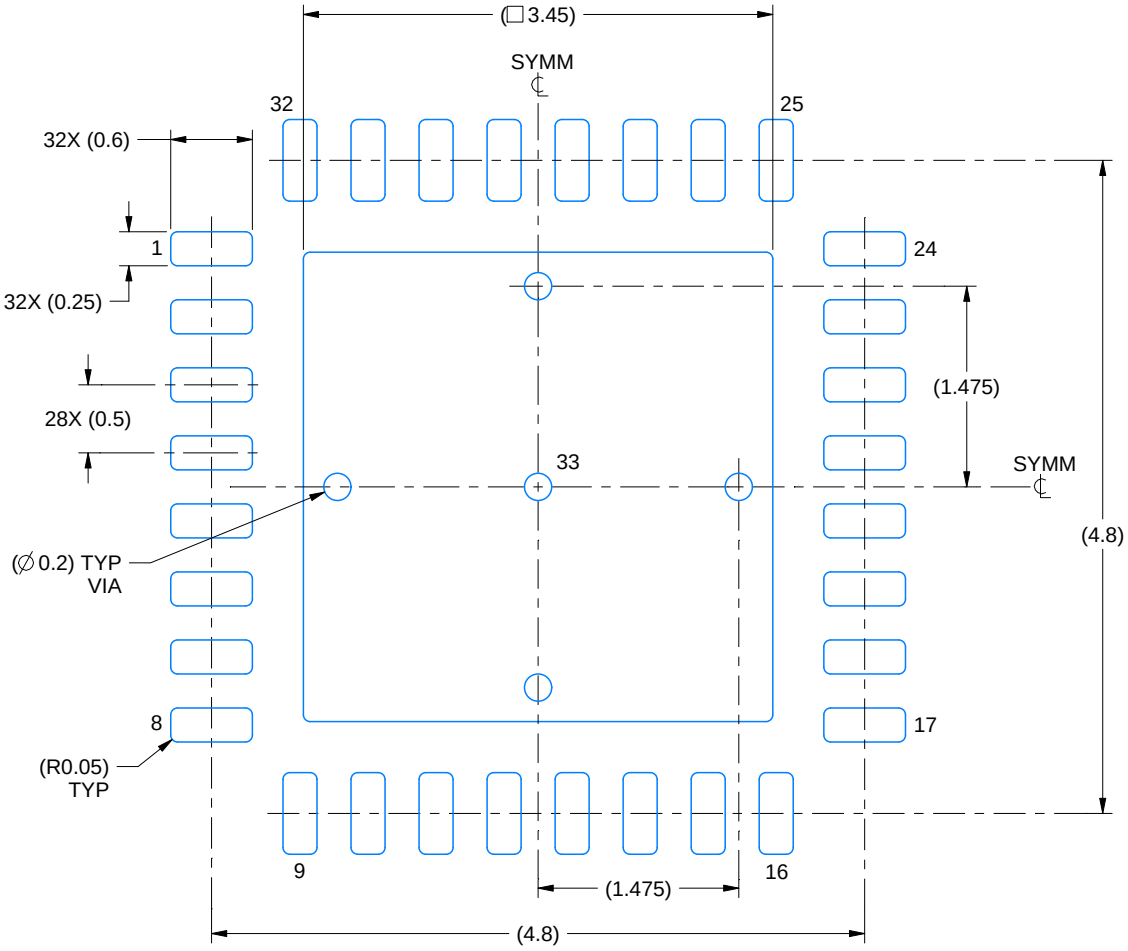
VQFN - 1 mm max height

PLASTIC QUAD FLATPACK - NO LEAD

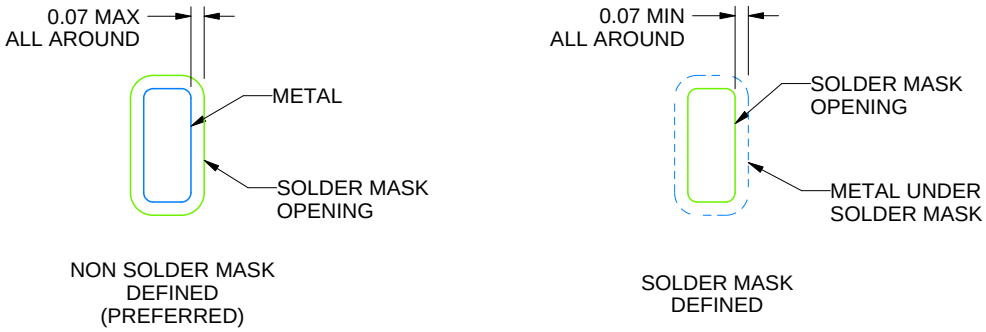


NOTES:

1. All linear dimensions are in millimeters. Any dimensions in parenthesis are for reference only. Dimensioning and tolerancing per ASME Y14.5M.
2. This drawing is subject to change without notice.
3. The package thermal pad must be soldered to the printed circuit board for thermal and mechanical performance.



LAND PATTERN EXAMPLE
SCALE:18X

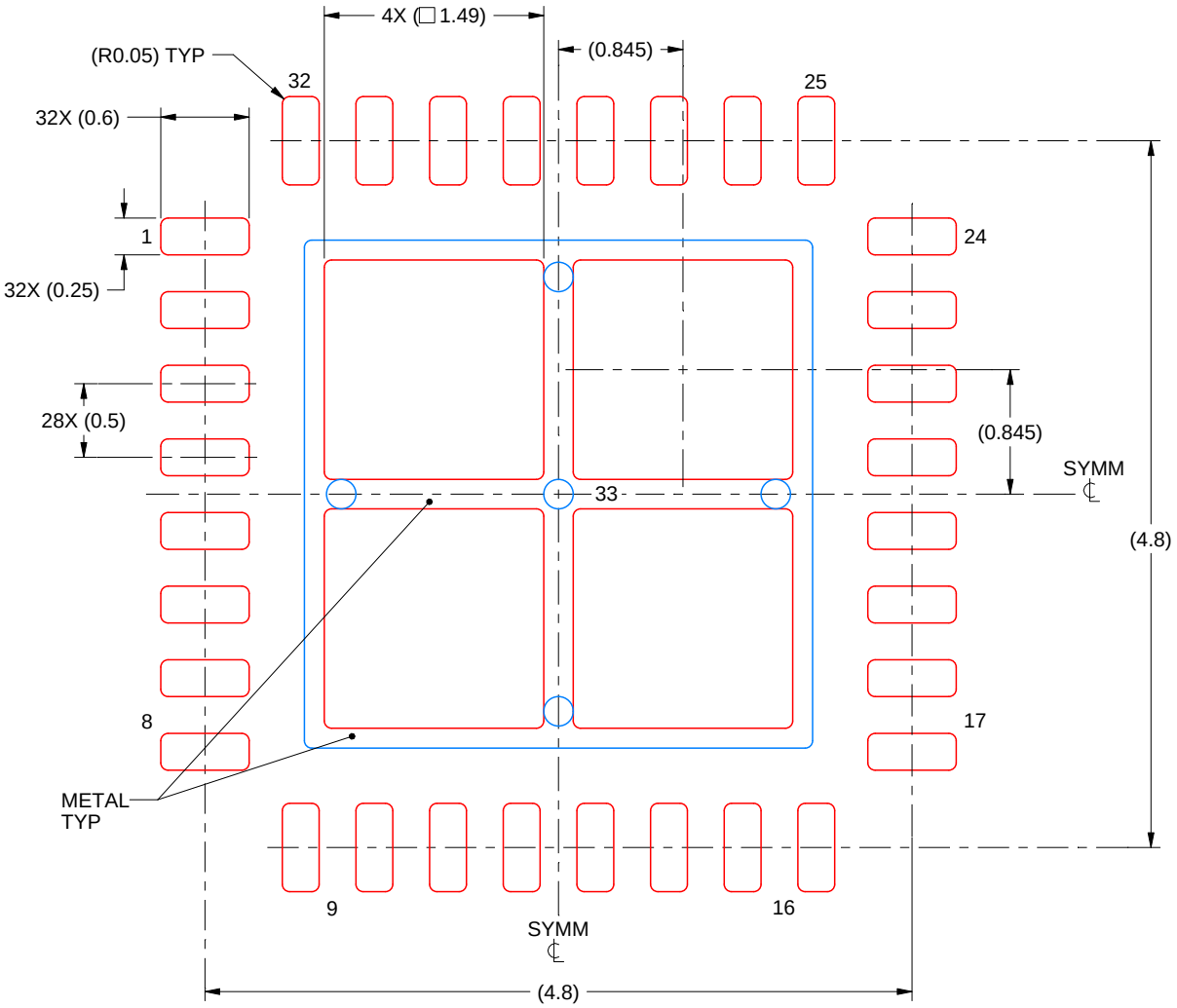


SOLDER MASK DETAILS

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NOTES: (continued)

4. This package is designed to be soldered to a thermal pad on the board. For more information, see Texas Instruments literature number SLUA271 (www.ti.com/lit/slua271).
5. Vias are optional depending on application, refer to device data sheet. If any vias are implemented, refer to their locations shown on this view. It is recommended that vias under paste be filled, plugged or tented.



SOLDER PASTE EXAMPLE
BASED ON 0.125 mm THICK STENCIL

EXPOSED PAD 33:
75% PRINTED SOLDER COVERAGE BY AREA UNDER PACKAGE
SCALE:20X

4223442/B 08/2019

NOTES: (continued)

6. Laser cutting apertures with trapezoidal walls and rounded corners may offer better paste release. IPC-7525 may have alternate design recommendations.

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